

REIVINDICACIONES

1. Una sonda de guía de onda superficial guiada (400, 400a, 400b, 400c), que comprende:

una terminal de carga (T) elevada por encima de un medio conductor con pérdidas (403); y

un circuito de acoplamiento (409) configurado para acoplar una fuente de excitación (412, 912) a la terminal de carga, el circuito de acoplamiento configurado para proporcionar un voltaje a la terminal de carga que establece un campo eléctrico que tiene una inclinación de onda (W) que se cruza con el medio conductor con pérdidas a una tangente de un ángulo de Brewster complejo ($\psi_{i,B}$) a una distancia crítica de Hankel (R_x) de la sonda de guía de onda superficial guiada.

2. La sonda de guía de onda superficial guiada de la reivindicación 1, en donde el circuito de acoplamiento comprende una bobina acoplada entre la fuente de excitación y la terminal de carga.

3. La sonda de guía de onda superficial guiada de la reivindicación 2, en donde la bobina es una bobina helicoidal.

4. La sonda de guía de onda superficial guiada de cualquiera de las reivindicaciones 2 y 3, en donde la fuente de excitación se acopla a la bobina a través de una conexión

de derivación.

5. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-4, en donde la conexión de derivación está en un punto de acoplamiento de impedancias en la bobina.

6. La sonda de guía de onda superficial guiada de cualquiera de las reivindicaciones 2-5, en donde se una red de acoplamiento de impedancias se acopla entre la fuente de excitación y la conexión de derivación en la bobina.

7. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-6, en donde la fuente de excitación se acopla magnéticamente a la bobina.

8. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-7, en donde la terminal de carga se acopla a la bobina a través de una conexión de derivación.

9. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 1-8 en donde la terminal de carga se coloca a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la sonda de guía de onda superficial guiada, donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y Φ es una

fase de la altura efectiva.

10. La sonda de guía de onda superficial guiada de la reivindicación 9, en donde la fase Φ es aproximadamente igual a un ángulo Ψ de la inclinación de la onda que corresponde al ángulo de Brewster complejo.

11. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 1-10, en donde la terminal de carga tiene un diámetro esférico efectivo, y la terminal de carga se coloca a una altura que es al menos cuatro veces el diámetro esférico efectivo.

12. La sonda de guía de onda superficial guiada de la reivindicación 11, en donde la terminal de carga es una terminal esférica con el diámetro esférico efectivo igual a un diámetro de la terminal esférica.

13. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11 y 12, en donde la altura de la terminal de carga es mayor que una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la sonda de guía de onda superficial guiada, donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$.

14. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11-13, que comprende

además una terminal de compensación (T) colocada por debajo de la terminal de carga, la terminal de compensación acoplada al circuito de acoplamiento.

15. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11-14, en donde la terminal de compensación se coloca por debajo de la terminal de carga a una distancia igual a la altura física (h_p).

16. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11-15, en donde Φ es una diferencia de fase compleja entre la terminal de compensación y la terminal de carga.

17. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 1-16, en donde el medio conductor con pérdidas es un medio terrestre.

18. Un sistema para excitar un modo de guía de onda superficial guiada a lo largo de un medio con pérdidas, que comprende:

una sonda de guía de onda superficial guiada (400, 400a, 400b, o 400c), que incluye:

una terminal de carga (T) elevada por encima de un medio conductor con pérdidas (403); y

un circuito de acoplamiento (409) configurado para proporcionar un voltaje a la terminal de carga que establece

un campo eléctrico que tiene una inclinación de onda (W) que se cruza con el medio conductor con pérdidas a una tangente de un ángulo de Brewster complejo ($\psi_{i,B}$) a una distancia crítica de Hankel (R_x) de la sonda de guía de onda superficial guiada (400); y

una fuente de excitación (412, 912) acoplada a la terminal de carga a través del circuito de acoplamiento.

19. El sistema de la reivindicación 18, que comprende además un sistema de control de sonda (418) configurado para ajustar la sonda de guía de onda superficial guiada con base al menos en parte en las características del medio conductor con pérdidas.

20. El sistema de cualquiera de una de las reivindicaciones 18 y 19, en donde el medio conductor con pérdidas es un medio terrestre.

21. El sistema de cualquiera de una de las reivindicaciones 18-20, en donde el circuito de acoplamiento comprende una bobina acoplada entre la fuente de excitación y la terminal de carga, la terminal de carga acoplada a la bobina a través de una derivación variable.

22. El sistema de la reivindicación 21, en donde la bobina es una bobina helicoidal.

23. El sistema de cualquiera de una de las

reivindicaciones 21 y 22, en donde el sistema de control de sonda (418) ajusta una posición de la derivación variable en respuesta a un cambio en las características del medio conductor con pérdidas.

24. El sistema de cualquiera de una de las reivindicaciones 21-23, en donde el ajuste de la posición de la derivación variable ajusta la inclinación de onda de campo eléctrico para corresponder a una iluminación de onda que se cruza con el medio conductor con pérdidas al ángulo de Brewster complejo ($\psi_{i,B}$) a la distancia crítica de Hankel (R_x).

25. El sistema de cualquiera de una de las reivindicaciones 21-24, en donde la sonda de guía de onda superficial guiada comprende además una terminal de compensación (T_2) colocada por debajo de la terminal de carga, la terminal de compensación acoplada al circuito de acoplamiento.

26. El sistema de cualquiera de una de las reivindicaciones 21-25, en donde la terminal de compensación se coloca por debajo de la terminal de carga a una distancia igual a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la sonda de guía de onda superficial guiada, donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p$

$e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y en donde Φ es una diferencia de fase compleja entre la terminal de compensación y la terminal de carga.

27. El sistema de cualquiera de una de las reivindicaciones 21-26, en donde el sistema de control de sonda ajusta una posición de la terminal de compensación en respuesta a un cambio en las características del medio conductor con pérdidas.

28. Un método para excitar una sonda de guía de onda superficial guiada, que comprende:

colocar una terminal de carga (T) a una altura definida (H_1 , h_T) sobre un medio conductor con pérdidas (403);

colocar una terminal de compensación (T) por debajo de la terminal de carga, la terminal de compensación separada por una distancia definida (h); y

excitar la terminal de carga y la terminal de compensación con voltajes de excitación que tienen una diferencia de fase compleja, en donde los voltajes de excitación establecen un campo eléctrico que tiene una inclinación de onda (W) que corresponde a una onda que ilumina el medio conductor con pérdidas a un ángulo de Brewster complejo ($\psi_{i,B}$) a una distancia crítica de Hankel (R_x) de la terminal de carga y la terminal

de compensación.

29. El método de la reivindicación 28, en donde la terminal de carga tiene un diámetro esférico efectivo, y la terminal de carga se coloca a la altura definida que es al menos cuatro veces el diámetro esférico efectivo.

30. El método de cualquiera de una de las reivindicaciones 28 y 29, en donde la distancia definida es igual a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la terminal de carga, en donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y en donde Φ es la diferencia de fase compleja entre la terminal de compensación y la terminal de carga.

31. El método de cualquiera de una de las reivindicaciones 28-30, en donde la terminal de carga y la terminal de compensación se acoplan a una fuente de excitación a través de una bobina, la terminal de carga acoplada a la bobina por una derivación variable.

32. El método de la reivindicación 31, que comprende además el ajuste de una posición de la derivación variable para establecer el campo eléctrico que tiene la inclinación de onda que se cruza con el medio conductor con pérdidas al ángulo de Brewster complejo ($\psi_{i,B}$) a la distancia crítica de Hankel (R_x).

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de superar las objeciones de claridad planteadas por el examinador en su concepto técnico.

2. Pago de tasas

En relación con el número de reivindicaciones, atentamente nos permitimos decir que no se adjunta tasa por reivindicaciones adicionales, toda vez que el nuevo capítulo reivindicatorio tiene el mismo número de cláusulas que el originalmente presentado y es en esencia el mismo objeto, pero más limitado y definido con mayor claridad.

De otro lado, se adjunta recibo por concepto de examen de patentabilidad, según lo estipulado en la Resolución No. 3719 del 2016.

3. Claridad y concisión de las reivindicaciones

El solicitante manifiesta que mediante la presentación del nuevo capítulo reivindicatorio quedan subsanadas la totalidad de las objeciones, de modo tal que las nuevas reivindicaciones proporcionan claridad y concisión a la invención descrita, siguiendo las recomendaciones realizadas por el examinador en su concepto técnico.

En particular y tal como se indicó arriba, las nuevas reivindicaciones incluyen los números de referencia, permitiendo una mejor comprensión de la invención.

De otro lado, en cuanto a las demás objeciones de claridad, se desea manifestar lo siguiente:

3.1. Parámetros indefinidos

El examinador objeta el parámetro “*inclinación de onda (W)*” descrito en las reivindicaciones 1, 18 y 28. El solicitante respetuosamente expresa su desacuerdo y señala que un experto entenderá fácilmente el significado del parámetro, utilizando los conocimientos generales comunes en el campo y especialmente en vista de los párrafos [0048] - [0051] y [0072] - [0074] (y las Figuras 3A, 3B y 8A) de la Solicitud Internacional tal como fue presentada. En consecuencia, el parámetro “*inclinación de onda (W)*” es suficientemente claro para una persona experta.

El examinador también objeta el parámetro “*ángulo de Brewster complejo ($\psi_{i,B}$)*” mencionado en las reivindicaciones 1, 18, 24 y 28. El solicitante respetuosamente expresa su desacuerdo y señala que una persona experta entendería fácilmente el significado del parámetro, dado el conocimiento general común en el campo y especialmente en vista de la Descripción. Se proporciona una discusión del término en, por ejemplo, párrafos [0048-0051] y [0070-0074] (y las Figuras 7, 8A y 8B), de la Solicitud Internacional tal como fue presentada. Por consiguiente, el parámetro “*ángulo de Brewster complejo ($\psi_{i,B}$)*” es suficientemente claro para una persona experta.

El examinador también objeta el parámetro “*distancia crítica de Hankel (R_x)*” incluido en las reivindicaciones 1, 18, 24, 28 y 32. El solicitante respetuosamente expresa su desacuerdo y señala que una persona experta entenderá fácilmente el significado del parámetro, dado el conocimiento general común en el campo y especialmente en vista de los párrafos [0047] y [0067-0068] (y la figura 5) de la Solicitud Internacional tal como fue presentada. En consecuencia, la definición del parámetro “*distancia crítica de Hankel (R_x)*” es suficientemente clara.

El examinador también objeta el parámetro “*altura física (h_p)*” que se encuentra en las reivindicaciones 9, 13, 15, 26 y 30. El solicitante respetuosamente expresa su desacuerdo y señala que un experto comprenderá fácilmente el significado del parámetro, dado el conocimiento general común en el campo y especialmente en vista de los párrafos [0072-0076] y [0081-0084] (y las Figuras 8A, 8B, 9A, 9B, 17 y 18) de la Solicitud Internacional tal como fue presentada. En consecuencia, la definición del parámetro “*altura física (h_p)*” es suficientemente clara.

El examinador también objeta el parámetro “*fase Φ* ” descrito en las reivindicaciones 9 y 10. El solicitante respetuosamente expresa su desacuerdo y señala que un experto en la materia entenderá fácilmente que la “*fase Φ* ” es una diferencia de fase compleja entre el terminal de compensación y el terminal de carga. Por ejemplo, la Descripción trata la fase Φ en numerosos puntos, incluyendo en, por ejemplo, párrafos [0052], [0072-0109], [0132] y [0133] de la Solicitud Internacional tal como fue presentada. En consecuencia, la “*fase Φ* ” es clara para una persona experta.

El examinador también objeta el parámetro “*ángulo (ψ) de la inclinación de onda de iluminación*”. La reivindicación 10 se ha modificado para aclarar aún más el significado del parámetro para recitar “*ángulo ψ de la inclinación de la onda*”. Sin embargo, el

solicitante desea señalar que una persona experta entendería fácilmente el significado del parámetro, dado el conocimiento general común en el campo y especialmente en vista de los párrafos [0081], [0087-0088] y [0144] (y las Figs. 8A y 8B) de la Solicitud Internacional tal como fue presentada. En consecuencia, el parámetro "*ángulo ψ de la inclinación de la onda*" es suficientemente claro.

El examinador también objeta el parámetro "*diámetro esférico efectivo*" incluido en las reivindicaciones 11, 12 y 29. El solicitante respetuosamente expresa su desacuerdo y señala que un experto en la materia entenderá fácilmente el significado de un diámetro esférico efectivo. Por ejemplo, la Descripción discute dicho término en los párrafos [0083], [0103], [0109] y [0144] de la Solicitud Internacional tal como fue presentada. El párrafo [0083] de la Descripción, por ejemplo, recita: "*Con la configuración seleccionada de la terminal de carga T1, se puede determinar un diámetro esférico (o el diámetro esférico efectivo)*". Por consiguiente, el parámetro "*diámetro esférico efectivo*", es claro para una persona experta.

El examinador también objeta el parámetro " $\theta_{i,B}$ " descrito en las reivindicaciones 9, 13, 26 y 30. El solicitante respetuosamente expresa su desacuerdo y señala que la relación de este ángulo $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ se menciona claramente en las reivindicaciones con respecto al ángulo de Brewster. En consecuencia, la definición del parámetro " $\theta_{i,B}$ " está es suficientemente clara.

3.2. Reivindicaciones no claras

El examinador considera que las reivindicaciones 9, 13, 16 y 30 no son claras porque recitan un parámetro (h_{eff}) definido por una ecuación con parámetros indefinidos, donde dicha ecuación viene dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$. El solicitante respetuosamente expresa su desacuerdo y señala que la invención no puede definirse adecuadamente de otra manera. Además, estos parámetros pueden determinarse de manera clara y fiable, según se enseña en la Descripción. Por ejemplo, la Descripción proporciona una discusión del parámetro "*altura efectiva (h_{eff})*" en los párrafos [0081], [0087-0088] y [0144] (y las Figuras 8A y 8B) de la Solicitud Internacional tal como fue publicada. En consecuencia, las reivindicaciones 6, 13, 16 y 30 son suficientemente claras para una persona experta a la luz de la Descripción.

3.3. Términos no claros

El examinador afirma que los términos “*conexión de derivación*” y “*derivación variable*” incluidos en las reivindicaciones 4, 5, 21, 23 y 31 no son claros por que no definen con exactitud un tipo o componente de conexión. El solicitante expresa su desacuerdo, por al menos las siguientes razones:

En primer lugar, el Diccionario Autorizado de Términos de Estándares IEEE (7ma Ed.) *Describe “una derivación”* como:

IEEE Estándar en español

“una conexión sacada de un devanado en algún punto entre sus extremidades, para permitir cambiar la relación de voltaje o corriente”.

En segundo lugar, la reivindicación 21 depende de las reivindicaciones 23 y 24, la reivindicación 4 depende de la reivindicación 5 y la reivindicación 31 depende de la reivindicación 32. Las reivindicaciones 5, 23, 24 y 32, recitan entonces (énfasis añadido):

5. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-4, en donde la conexión de derivación **está en un punto de acoplamiento de impedancias en la bobina.**

23. El sistema de cualquiera de una de las reivindicaciones 21 y 22, en donde **el sistema de control de sonda (418) ajusta una posición de la derivación variable en respuesta a un cambio en las características del medio conductor con pérdidas.**

24. El sistema de cualquiera de una de las reivindicaciones 21-23, **en donde el ajuste de la posición de la derivación variable ajusta la inclinación de onda de campo eléctrico** para corresponder a una iluminación de onda que se cruza con el medio conductor con pérdidas al ángulo de Brewster complejo ($\psi_{i,B}$) a la distancia crítica de Hankel (R_x).

32. El método de la reivindicación 31, **que comprende además el ajuste de una posición de la derivación variable para establecer el campo eléctrico** que tiene

la inclinación de onda que se cruza con el medio conductor con pérdidas al ángulo de Brewster complejo ($\psi_{i,B}$) a la distancia crítica de Hankel (R_x).

En tercer lugar, los términos “*conexión de derivación*” y “*derivación variable*” son adecuados y se utilizan de manera uniforme en la Descripción tal como fue presentada. Se proporciona una discusión de los términos en, por ejemplo, párrafos 0093 y 0138 (y las Figuras 17, 18, 24A y 24B), de la Solicitud Internacional tal como fue presentada.

Por al menos las siguientes razones, un experto entendería fácilmente el significado de los términos “*conexión de derivación*” y “*derivación variable*”, usando el conocimiento general común en el campo y especialmente en vista de la Descripción. En consecuencia, los términos “*conexión de derivación*” y “*derivación variable*” son suficientemente claros.

3.4. Términos Generales

El examinador considera que el término “*distancia definida*” incluido en la reivindicación 28 es general e indefinido. Sin embargo, la reivindicación 30 depende de “*cualquiera de una de las reivindicaciones 28 y 29*”. La reivindicación 28 por su parte, hace referencia a “*colocar una terminal de compensación (T) por debajo de la terminal de carga, la terminal de compensación separada por una distancia definida (h)*”. Por lo tanto, la distancia definida “*es igual a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la terminal de carga, en donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y en donde Φ es la diferencia de fase compleja entre la terminal de compensación y la terminal de carga*”, tal como se menciona en la reivindicación 30. Por consiguiente, el término “*distancia definida*” está claramente definido.

El examinador también afirma que el término “*altura definida*” incluido en la reivindicación 28 es general e indefinido. Sin embargo, la reivindicación 30 depende de “*cualquiera de una de las reivindicaciones 28 y 29*”. La reivindicación 29 por su parte, menciona que la altura definida es “*al menos cuatro veces el diámetro esférico efectivo*”. Por lo tanto, una persona experta entendería fácilmente el significado del parámetro “*altura definida*” mediante el uso de los conocimientos generales comunes en el campo y especialmente en vista de los párrafos [0084] - [0085] (y las figuras 9A y 9B) de la

Solicitud Internacional tal como fue presentada. En consecuencia, el término “*distancia definida*” está claramente definido.

Así, se superan todas las objeciones formuladas por el examinador.

En consecuencia, nos permitimos indicar que el presente capítulo reivindicatorio, que incluye 32 reivindicaciones, se ajusta a las disposiciones del artículo 30 de la Decisión 486/00.

4. Novedad

El examinador establece en su concepto técnico la falta de novedad de las anteriores reivindicaciones 1 – 4, 7, 8, 14, 16 – 25, 27, 28, 31 y 32 a la luz de las enseñanzas técnicas descritas el documento D1: CO 15220552.

A este respecto, me permito indicar que el artículo 16 de la Decisión 486 establece que “*Una invención se considerará nueva cuando no está comprendida en el estado de la técnica*”.

Lo anterior significa que para que un documento del Estado de la Técnica pueda afectar la novedad de una solicitud deberá revelar todas y cada una de las características que la definen.

El solicitante respetuosamente expresa su desacuerdo con la opinión del examinador y desea manifestar que en el oficio no se proporciona una base suficiente para demostrar que el objeto de las reivindicaciones de la presente solicitud se describe en D1.

Específicamente, el examinador afirma incorrectamente que la referencia D1 describe el objeto de las reivindicaciones 1, 18 y 28. Este no es el caso. D1 menciona que “*se describen varias sondas de guía de ondas de superficie guiadas*”. Sin embargo, D1 no describe una inclinación de onda como se expone en las presentes reivindicaciones, y mucho menos “un circuito de acoplamiento... configurado para proporcionar un voltaje a la terminal de carga que establece un campo eléctrico que tiene una inclinación de onda (W) que se cruza con el medio conductor con pérdidas a una tangente de un ángulo de Brewster complejo (ψ_{LB}) a una distancia crítica de Hankel (R_h) de la sonda de guía de onda superficial guiada, como se menciona en la reivindicación 1.

En consecuencia, el documento D1 NO revela todas y cada una de las características técnicas que definen la sonda de guía de onda superficial guiada, como se recita en la presente solicitud.

Del mismo modo, D1 tampoco describe, enseña o sugiere todas las características de las reivindicaciones 18 o 28.

Así, tanto las reivindicaciones independientes como dependientes resultan novedosas sobre D1, superando la objeción del examinador.

De esta forma, se demuestra que las nuevas reivindicaciones 1 a 32 cumplen con el requisito de novedad según los lineamientos del artículo 16 de la Decisión 486/00.

4.1. Patente otorgada en Estados Unidos

Si bien se reconoce la autonomía que cada jurisdicción tiene para decidir sobre temas de Propiedad Industrial, es importante mencionar que una patente equivalente a la de la presente solicitud ha sido otorgada por la Oficina de Patentes y Marcas de los Estados Unidos (Patente No. US 9,941,566), con la cual se tiene actualmente un acuerdo de PPH, es decir, que es posible reconocer los resultados del examen de patentabilidad proporcionados por dicha Oficina.

Vale mencionar que el alcance de las reivindicaciones en Estados Unidos es similar al de las reivindicaciones como se presentan en esta oportunidad.

5. **Conclusión**

Con las modificaciones introducidas y los argumentos presentados puede concluirse que:

- i) La presente solicitud es clara, concisa y está debidamente soportada en la descripción, cumpliendo con los requerimientos del Artículo 30 de la Decisión 486; y
- ii) Las reivindicaciones actuales son patentables sobre D1, según ha reconocido la Oficina de Patentes de Estados Unidos, cumpliendo así con los requerimientos del Artículo 16 de la Decisión 486.

En consecuencia, se solicita atentamente otorgar el privilegio de patente solicitado, toda vez que esta solicitud cumple con los requerimientos de la Decisión 486.

Habiendo atendido cabalmente las objeciones presentadas por ese despacho, atentamente solicitamos se conceda el privilegio de patente de invención a la solicitud en estudio o si el señor examinador considera que subsisten razones para objetar la presente invención, rogamos expedir otro examen de fondo con los debidos motivos y razones que sustenten su objeción con el fin de que nuestro mandante tenga la posibilidad de exponer sus argumentos con base en la interpretación de los artículos 45 de la Decisión 486 -el cual otorga la facultad al examinador para emitir los exámenes de fondo- y 42 del Código de Procedimiento Administrativo y de lo Contencioso Administrativo que señala que: *“Habiéndose dado oportunidad a los interesados para expresar sus opiniones, y con base en las pruebas e informes disponibles, se tomará la decisión, que será motivada. La decisión resolverá todas las peticiones que hayan sido oportunamente planteadas dentro de la actuación por el peticionario y por los terceros reconocidos”*, (el subrayado es nuestro).

Finalmente, solicitamos a ese Despacho pronunciarse en relación con todos los argumentos presentados en este memorial dando estricta aplicación al principio del debido proceso consagrado en el artículo 29 de la Constitución Nacional.

6. Anexos

- Nuevo capítulo reivindicatorio que incluye 32 reivindicaciones.
- Copia de la Patente de EEUU No. US 9,941,566.
- Recibo por concepto de examen de patentabilidad, en vista de las modificaciones realizadas sobre el pliego reivindicatorio, según lo estipulado en la Resolución No. 3719 del 2016.

Señor Director,


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REIVINDICACIONES

1. Una sonda de guía de onda superficial guiada (400, 400a, 400b, 400c), que comprende:

una terminal de carga (T) elevada por encima de un medio conductor con pérdidas (403); y

un circuito de acoplamiento (409) configurado para acoplar una fuente de excitación (412, 912) a la terminal de carga, el circuito de acoplamiento configurado para proporcionar un voltaje a la terminal de carga que establece un campo eléctrico que tiene una inclinación de onda (W) que se cruza con el medio conductor con pérdidas a una tangente de un ángulo de Brewster complejo ($\psi_{i,B}$) a una distancia crítica de Hankel (R_x) de la sonda de guía de onda superficial guiada.

2. La sonda de guía de onda superficial guiada de la reivindicación 1, en donde el circuito de acoplamiento comprende una bobina acoplada entre la fuente de excitación y la terminal de carga.

3. La sonda de guía de onda superficial guiada de la reivindicación 2, en donde la bobina es una bobina helicoidal.

4. La sonda de guía de onda superficial guiada de cualquiera de las reivindicaciones 2 y 3, en donde la fuente de excitación se acopla a la bobina a través de una conexión

de derivación.

5. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-4, en donde la conexión de derivación está en un punto de acoplamiento de impedancias en la bobina.

6. La sonda de guía de onda superficial guiada de cualquiera de las reivindicaciones 2-5, en donde se una red de acoplamiento de impedancias se acopla entre la fuente de excitación y la conexión de derivación en la bobina.

7. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-6, en donde la fuente de excitación se acopla magnéticamente a la bobina.

8. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 2-7, en donde la terminal de carga se acopla a la bobina a través de una conexión de derivación.

9. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 1-8 en donde la terminal de carga se coloca a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la sonda de guía de onda superficial guiada, donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y Φ es una fase de la altura efectiva.

10. La sonda de guía de onda superficial guiada de la reivindicación 9, en donde la fase Φ es aproximadamente igual a un ángulo Ψ de la inclinación de la onda que corresponde al ángulo de Brewster complejo.

11. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 1-10, en donde la terminal de carga tiene un diámetro esférico efectivo, y la terminal de carga se coloca a una altura que es al menos cuatro veces el diámetro esférico efectivo.

12. La sonda de guía de onda superficial guiada de la reivindicación 11, en donde la terminal de carga es una terminal esférica con el diámetro esférico efectivo igual a un diámetro de la terminal esférica.

13. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11 y 12, en donde la altura de la terminal de carga es mayor que una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la sonda de guía de onda superficial guiada, donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$.

14. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11-13, que comprende

además una terminal de compensación (T) colocada por debajo de la terminal de carga, la terminal de compensación acoplada al circuito de acoplamiento.

15. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11-14, en donde la terminal de compensación se coloca por debajo de la terminal de carga a una distancia igual a la altura física (h_p).

16. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 11-15, en donde Φ es una diferencia de fase compleja entre la terminal de compensación y la terminal de carga.

17. La sonda de guía de onda superficial guiada de cualquiera de una de las reivindicaciones 1-16, en donde el medio conductor con pérdidas es un medio terrestre.

18. Un sistema para excitar un modo de guía de onda superficial guiada a lo largo de un medio con pérdidas, que comprende:

una sonda de guía de onda superficial guiada (400, 400a, 400b, o 400c), que incluye:

una terminal de carga (T) elevada por encima de un medio conductor con pérdidas (403); y

un circuito de acoplamiento (409) configurado para proporcionar un voltaje a la terminal de carga que establece

un campo eléctrico que tiene una inclinación de onda (W) que se cruza con el medio conductor con pérdidas a una tangente de un ángulo de Brewster complejo ($\psi_{i,B}$) a una distancia crítica de Hankel (R_x) de la sonda de guía de onda superficial guiada (400); y

una fuente de excitación (412, 912) acoplada a la terminal de carga a través del circuito de acoplamiento.

19. El sistema de la reivindicación 18, que comprende además un sistema de control de sonda (418) configurado para ajustar la sonda de guía de onda superficial guiada con base al menos en parte en las características del medio conductor con pérdidas.

20. El sistema de cualquiera de una de las reivindicaciones 18 y 19, en donde el medio conductor con pérdidas es un medio terrestre.

21. El sistema de cualquiera de una de las reivindicaciones 18-20, en donde el circuito de acoplamiento comprende una bobina acoplada entre la fuente de excitación y la terminal de carga, la terminal de carga acoplada a la bobina a través de una derivación variable.

22. El sistema de la reivindicación 21, en donde la bobina es una bobina helicoidal.

23. El sistema de cualquiera de una de las

reivindicaciones 21 y 22, en donde el sistema de control de sonda (418) ajusta una posición de la derivación variable en respuesta a un cambio en las características del medio conductor con pérdidas.

24. El sistema de cualquiera de una de las reivindicaciones 21-23, en donde el ajuste de la posición de la derivación variable ajusta la inclinación de onda de campo eléctrico para corresponder a una iluminación de onda que se cruza con el medio conductor con pérdidas al ángulo de Brewster complejo ($\psi_{i,B}$) a la distancia crítica de Hankel (R_x).

25. El sistema de cualquiera de una de las reivindicaciones 21-24, en donde la sonda de guía de onda superficial guiada comprende además una terminal de compensación (T_2) colocada por debajo de la terminal de carga, la terminal de compensación acoplada al circuito de acoplamiento.

26. El sistema de cualquiera de una de las reivindicaciones 21-25, en donde la terminal de compensación se coloca por debajo de la terminal de carga a una distancia igual a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la sonda de guía de onda superficial guiada, donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} =$

$h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y en donde Φ es una diferencia de fase compleja entre la terminal de compensación y la terminal de carga.

27. El sistema de cualquiera de una de las reivindicaciones 21-26, en donde el sistema de control de sonda ajusta una posición de la terminal de compensación en respuesta a un cambio en las características del medio conductor con pérdidas.

28. Un método para excitar una sonda de guía de onda superficial guiada, que comprende:

colocar una terminal de carga (T) a una altura definida (H_1 , h_T) sobre un medio conductor con pérdidas (403);

colocar una terminal de compensación (T) por debajo de la terminal de carga, la terminal de compensación separada por una distancia definida (h); y

excitar la terminal de carga y la terminal de compensación con voltajes de excitación que tienen una diferencia de fase compleja, en donde los voltajes de excitación establecen un campo eléctrico que tiene una inclinación de onda (W) que corresponde a una onda que ilumina el medio conductor con pérdidas a un ángulo de Brewster complejo ($\psi_{i,B}$) a una distancia crítica de Hankel (R_x) de la terminal de carga y la terminal

de compensación.

29. El método de la reivindicación 28, en donde la terminal de carga tiene un diámetro esférico efectivo, y la terminal de carga se coloca a la altura definida que es al menos cuatro veces el diámetro esférico efectivo.

30. El método de cualquiera de una de las reivindicaciones 28 y 29, en donde la distancia definida es igual a una altura física (h_p) que corresponde a una magnitud de una altura efectiva de la terminal de carga, en donde la altura efectiva está dada por $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, con $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ y en donde Φ es la diferencia de fase compleja entre la terminal de compensación y la terminal de carga.

31. El método de cualquiera de una de las reivindicaciones 28-30, en donde la terminal de carga y la terminal de compensación se acoplan a una fuente de excitación a través de una bobina, la terminal de carga acoplada a la bobina por una derivación variable.

32. El método de la reivindicación 31, que comprende además el ajuste de una posición de la derivación variable para establecer el campo eléctrico que tiene la inclinación de onda que se cruza con el medio conductor con pérdidas al ángulo de Brewster complejo ($\psi_{i,B}$) a la distancia crítica de Hankel (R_x).



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(12) **United States Patent**
Corum et al.

(10) **Patent No.:** **US 9,941,566 B2**

(45) **Date of Patent:** **Apr. 10, 2018**

(54) **EXCITATION AND USE OF GUIDED
SURFACE WAVE MODES ON LOSSY MEDIA**

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17/00; H02J 50/20; H01P 3/00; H01P
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USPC 333/24 R, 240

See application file for complete search history.

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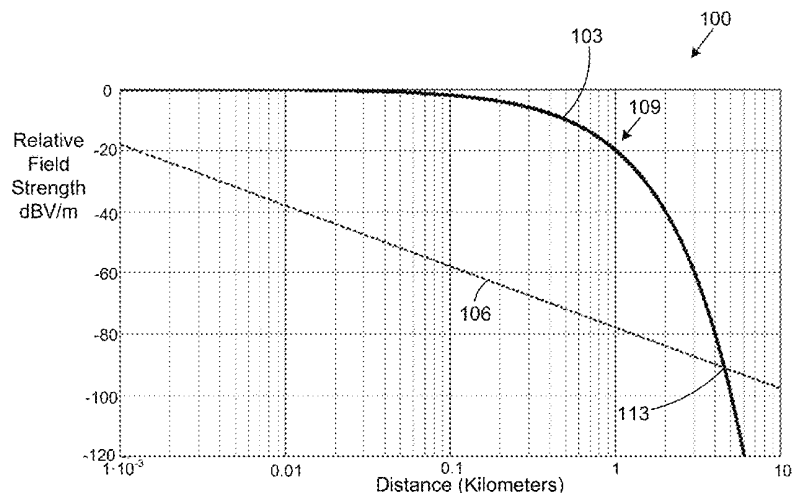
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(57) **ABSTRACT**

Disclosed are various embodiments for transmitting energy
conveyed in the form of a guided surface-waveguide mode
along the surface of a lossy medium such as, e.g., a terres-
trial medium by exciting a guided surface waveguide probe.

32 Claims, 23 Drawing Sheets



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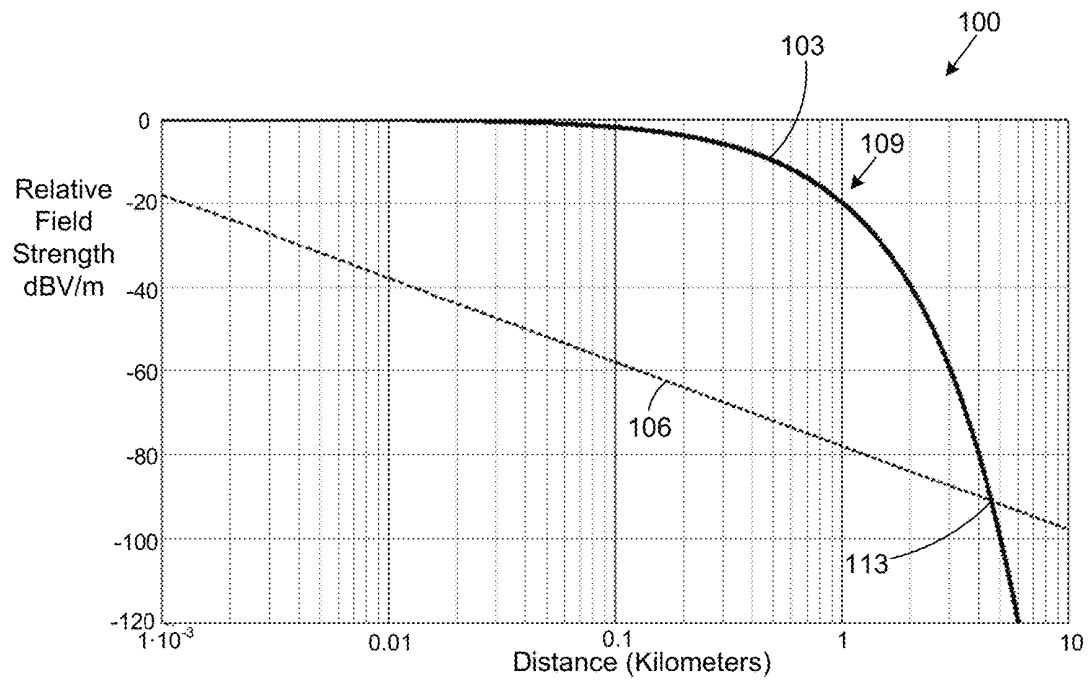
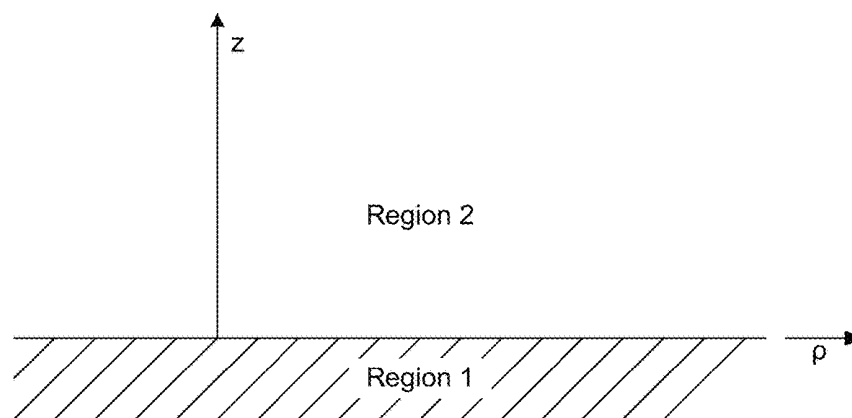
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**FIG. 1****FIG. 2**

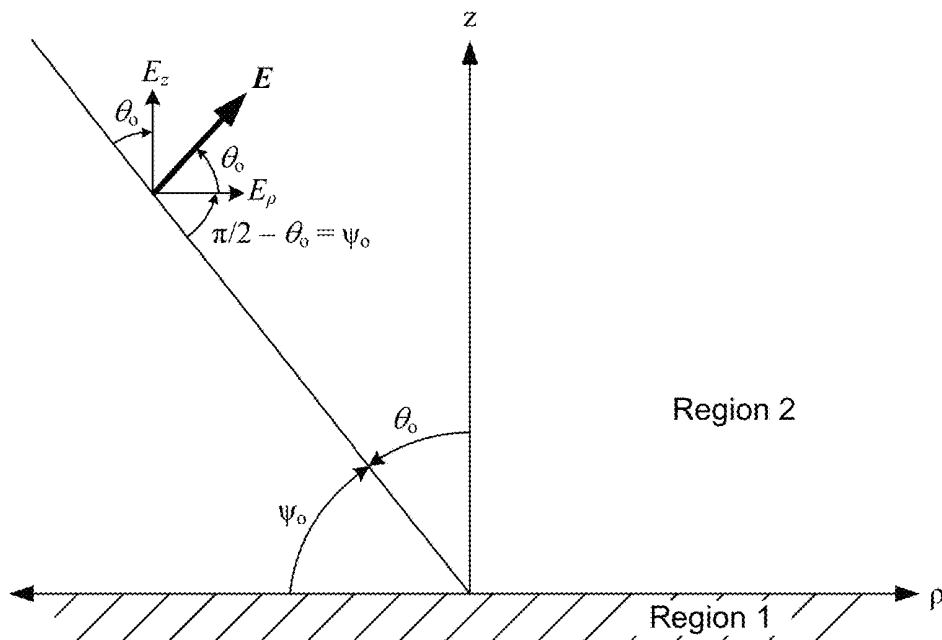
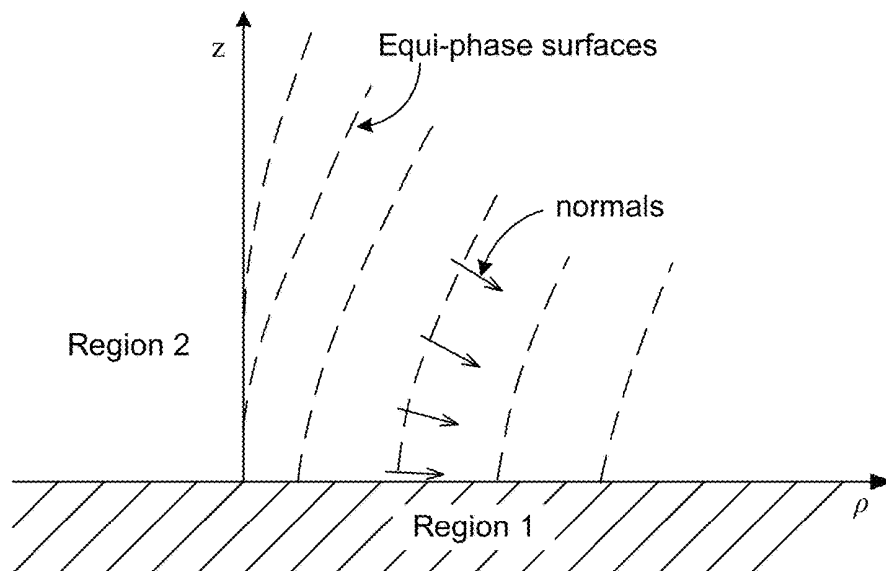
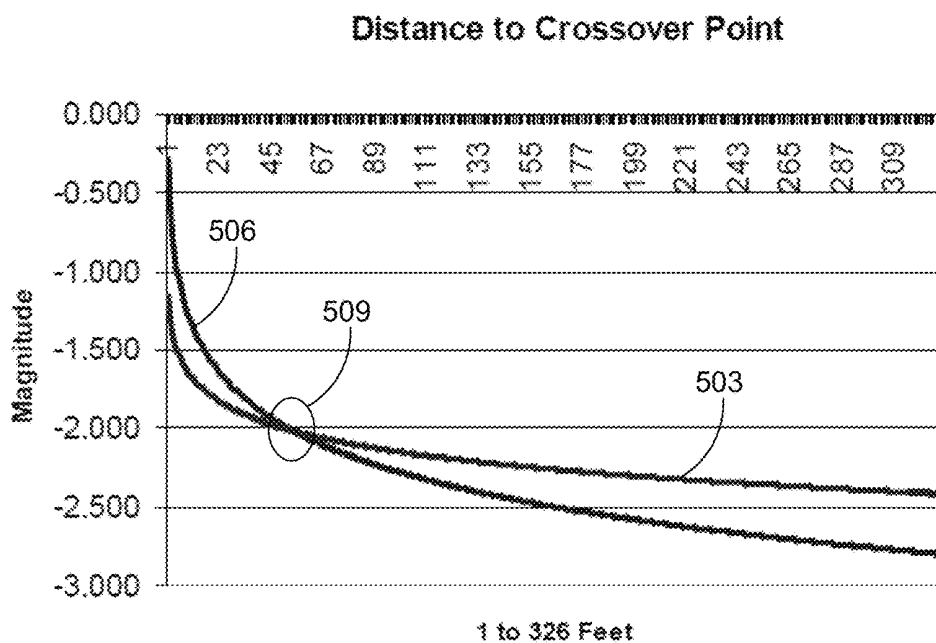
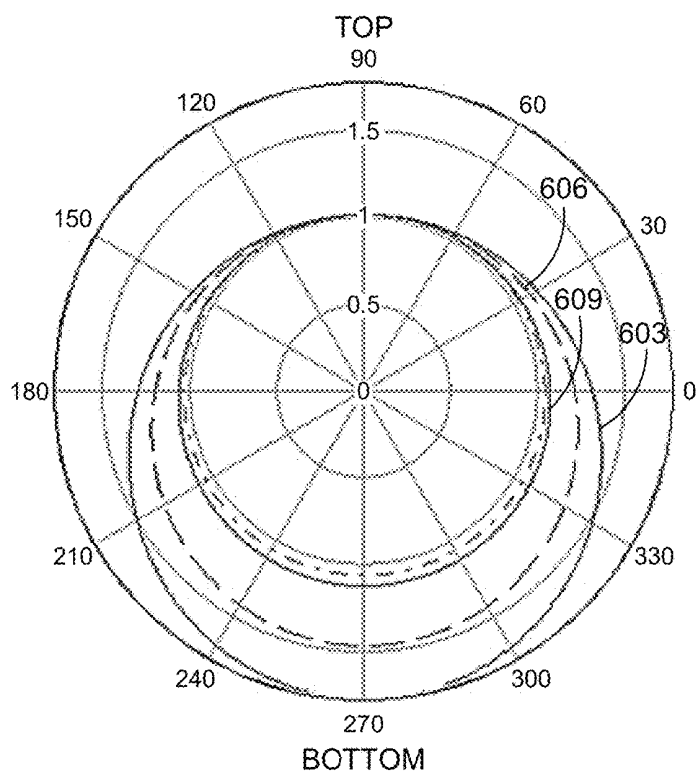
**FIG. 3A****FIG. 3B**

FIG. 4

**FIG. 5****FIG. 6A**

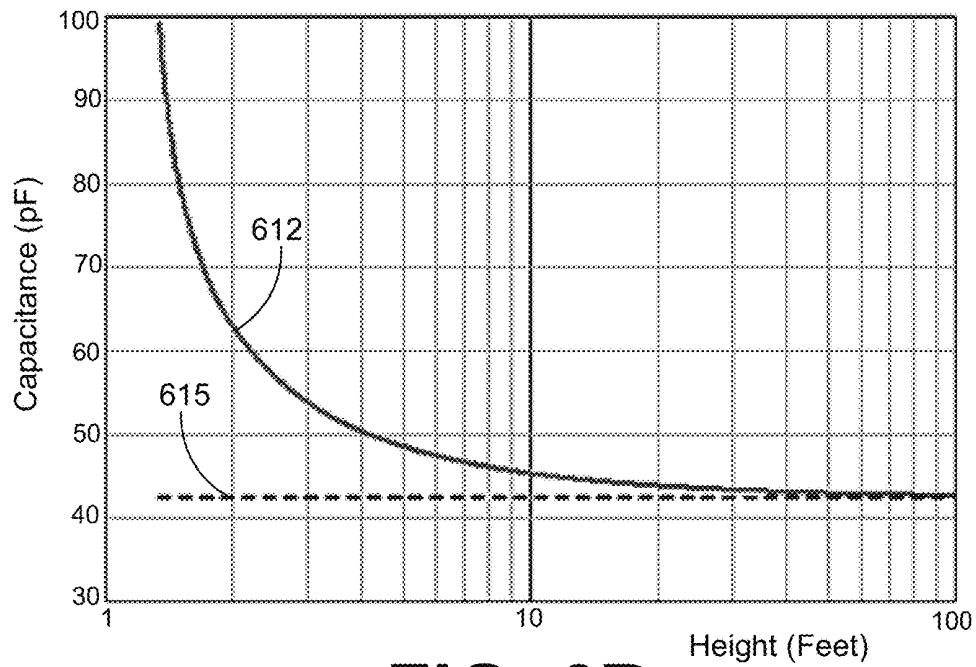


FIG. 6B

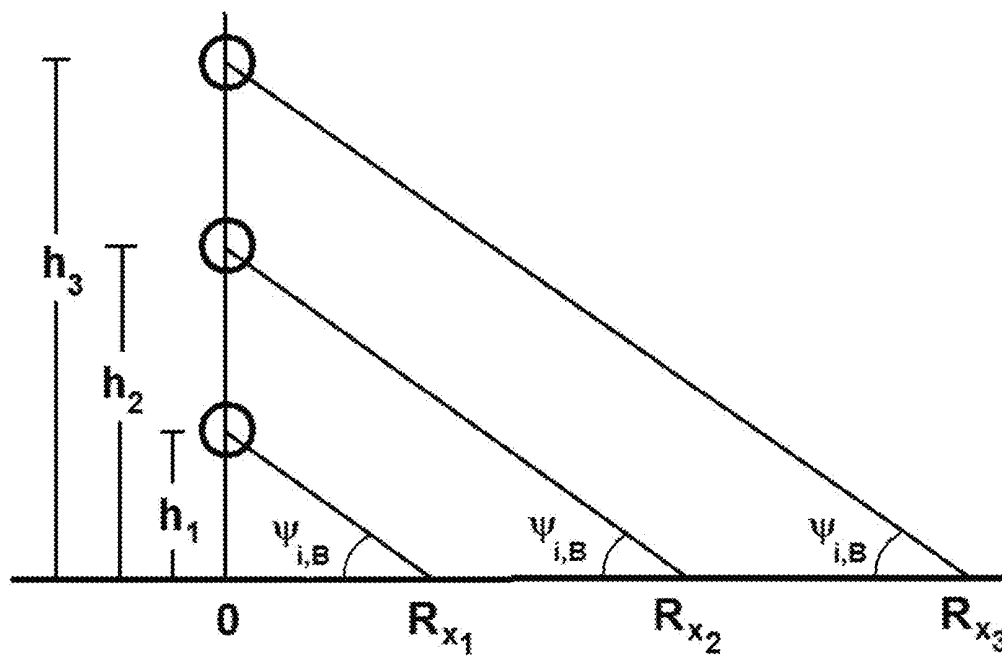
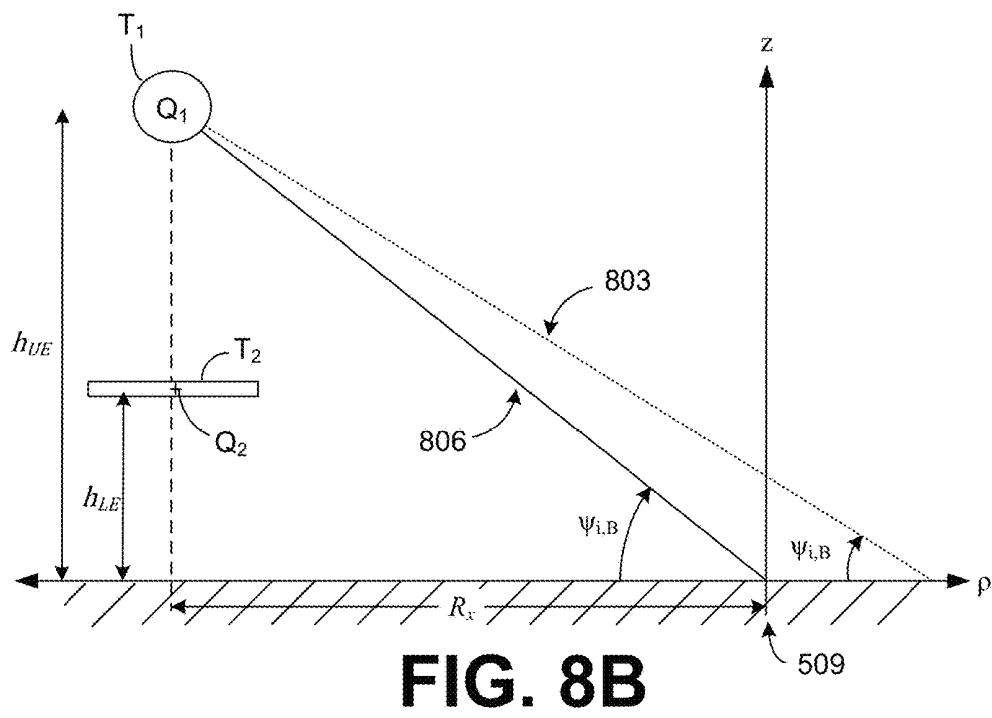
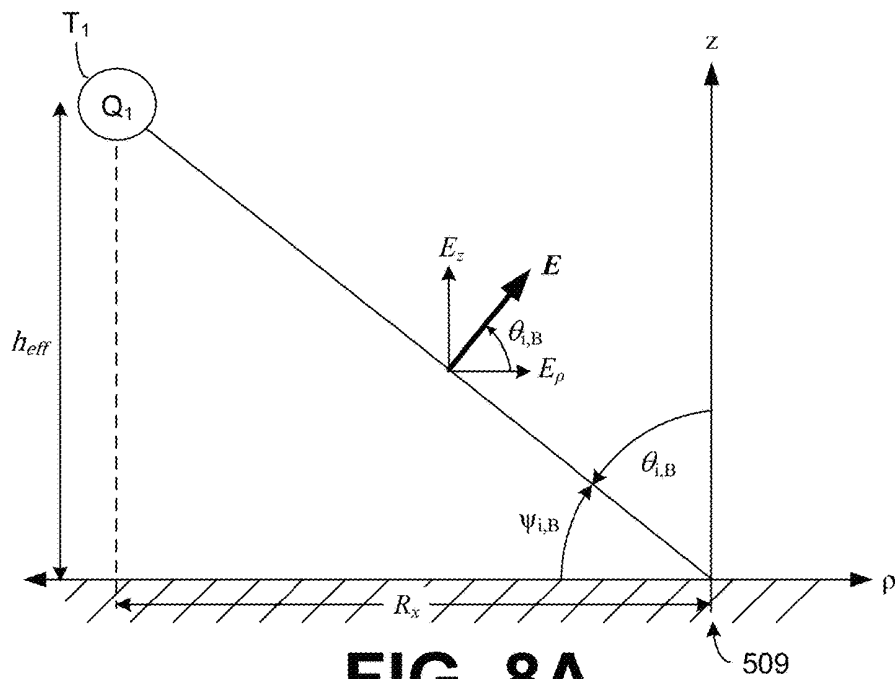
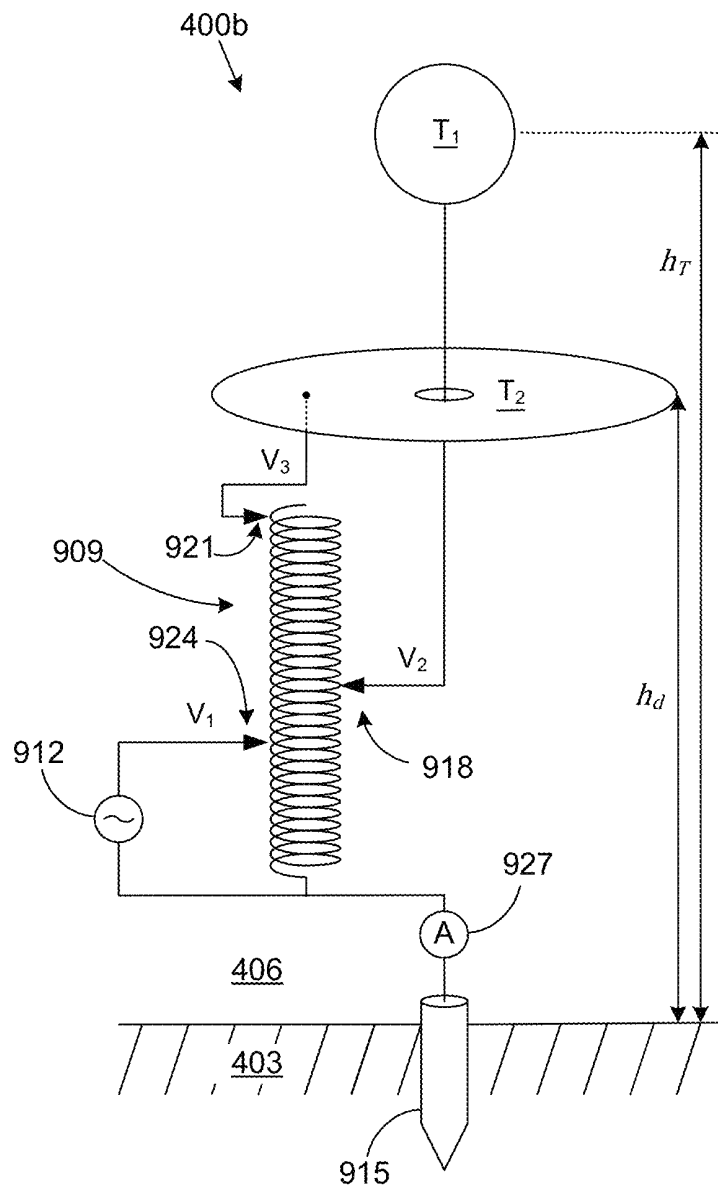


FIG. 7



**FIG. 9A**

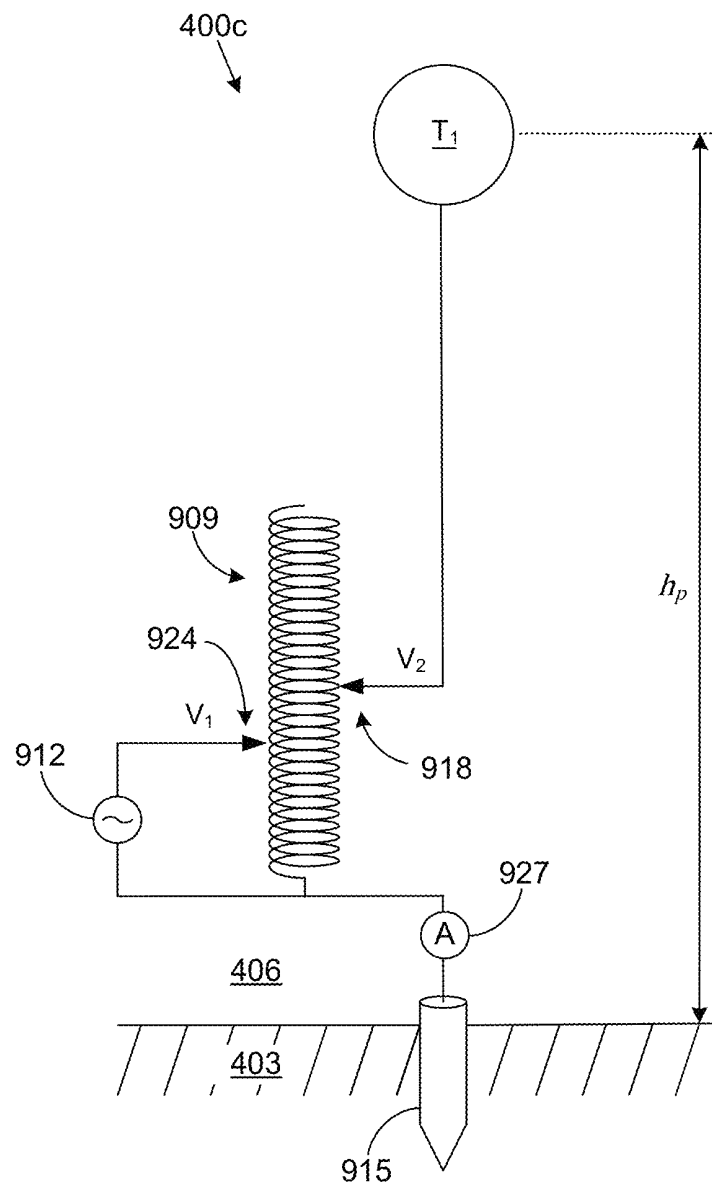


FIG. 9B

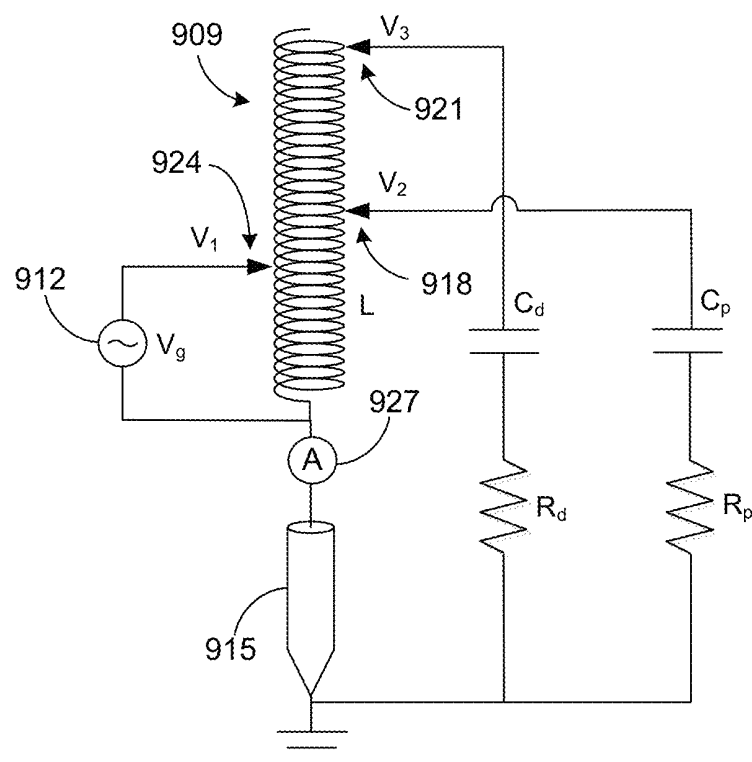
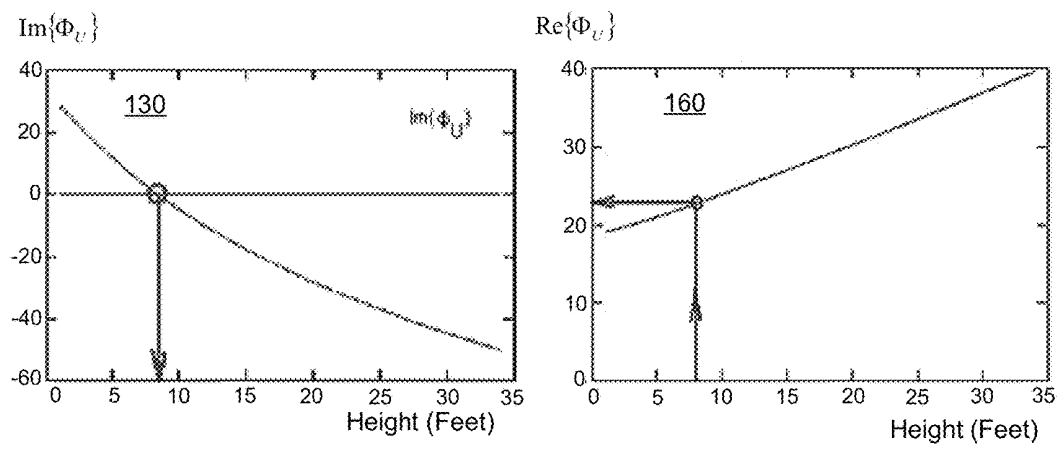
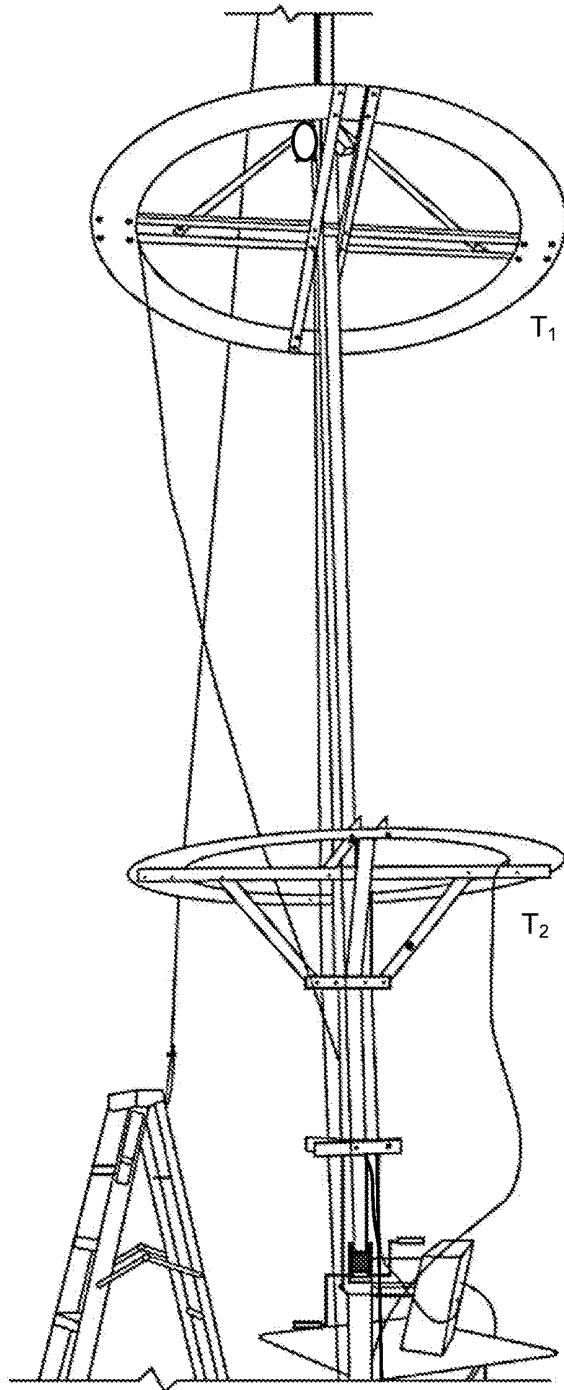
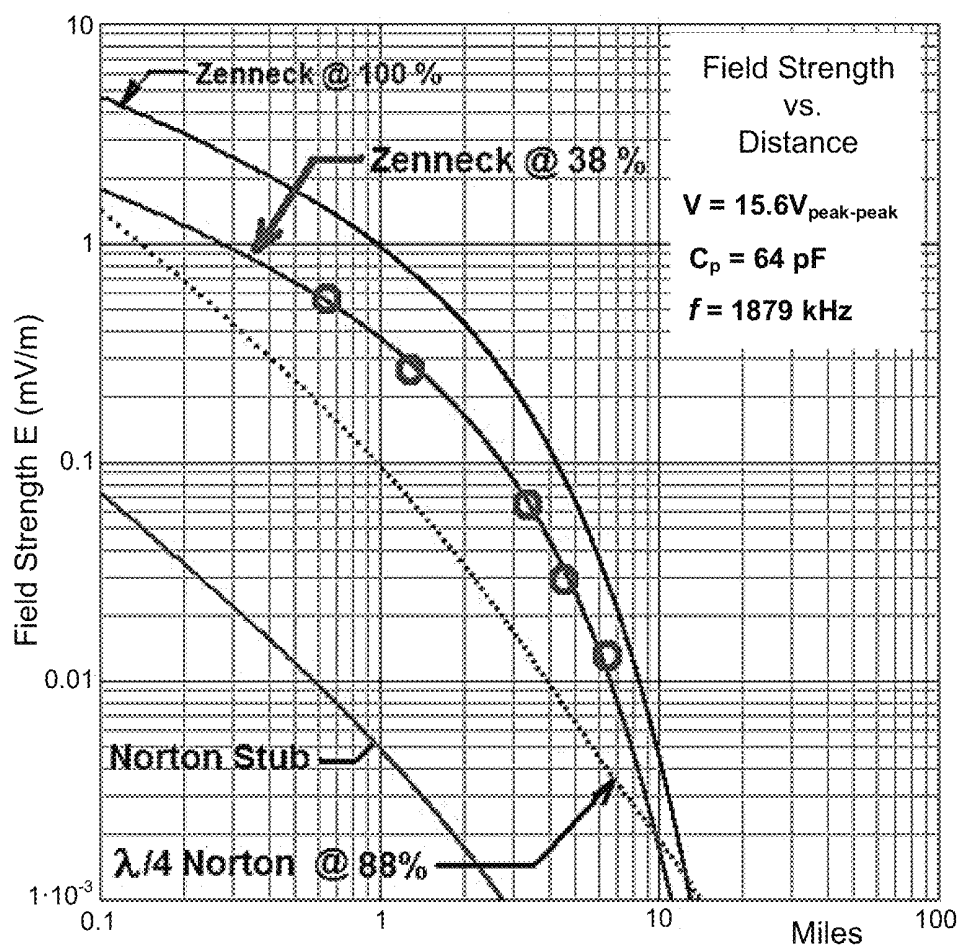


FIG. 10

**FIG. 11**

**FIG. 12**

**FIG. 13**

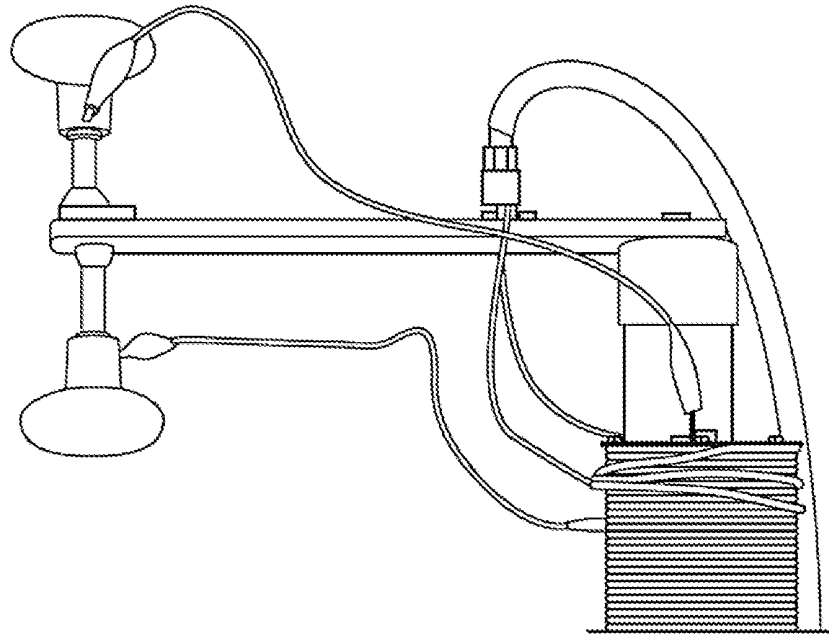


FIG. 14A

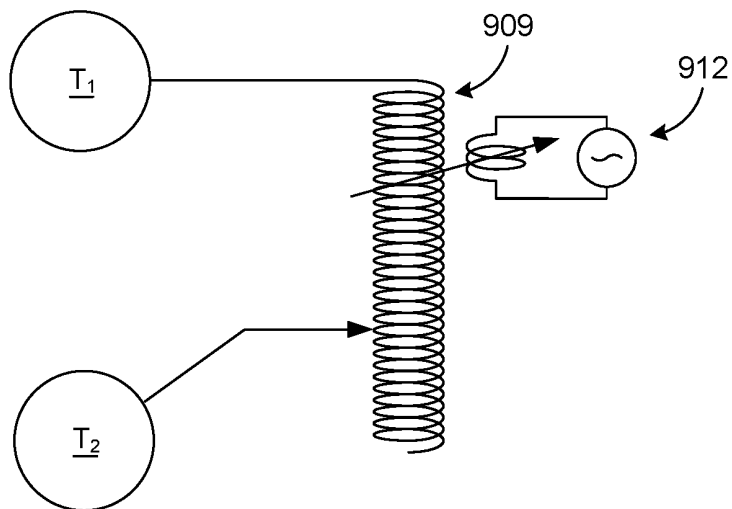
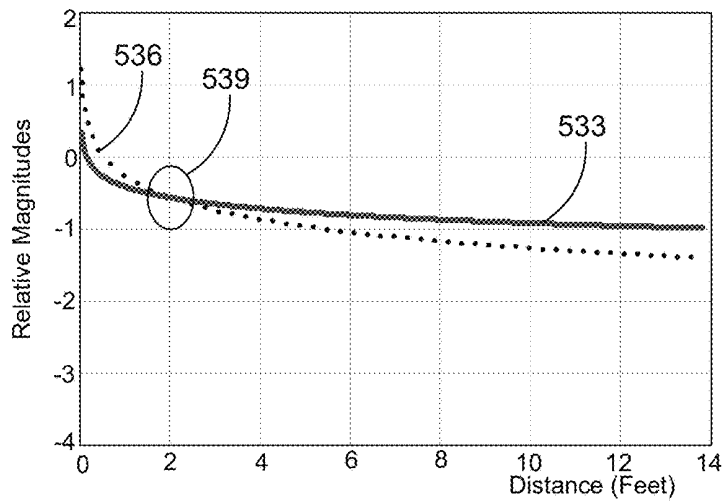
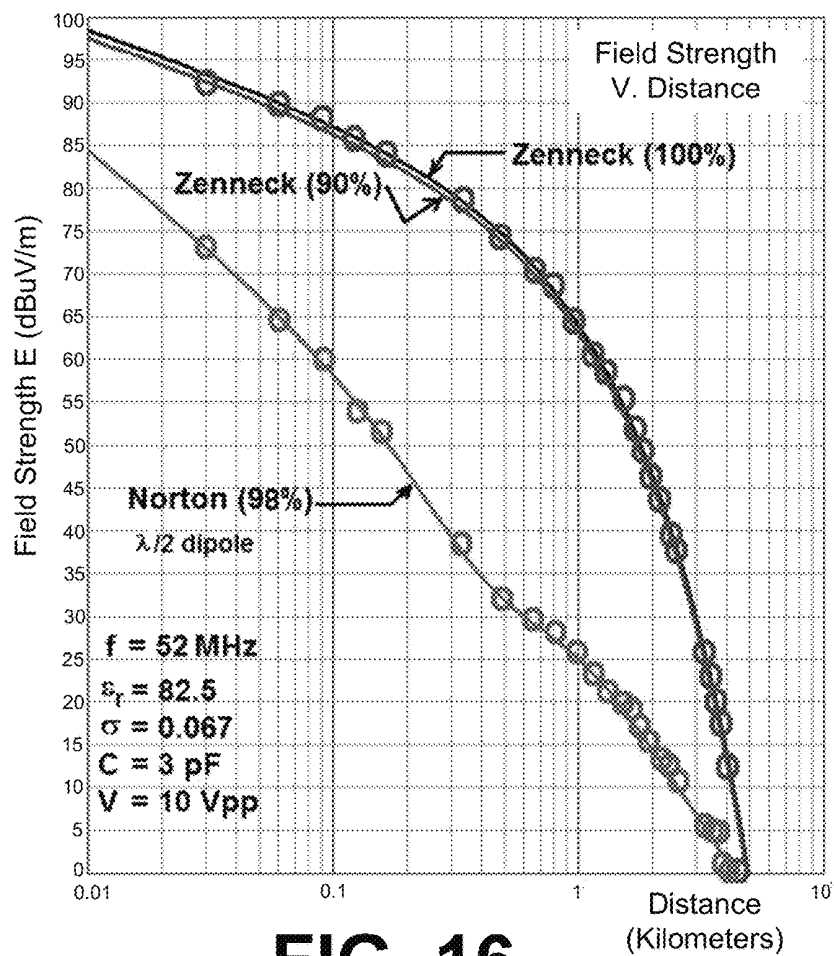
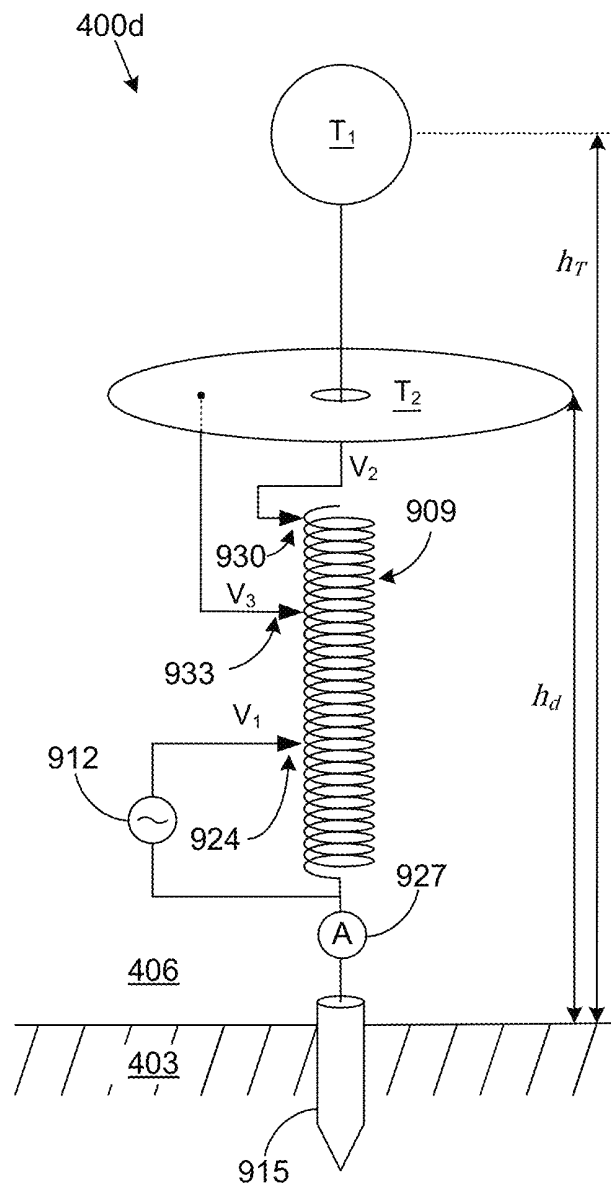
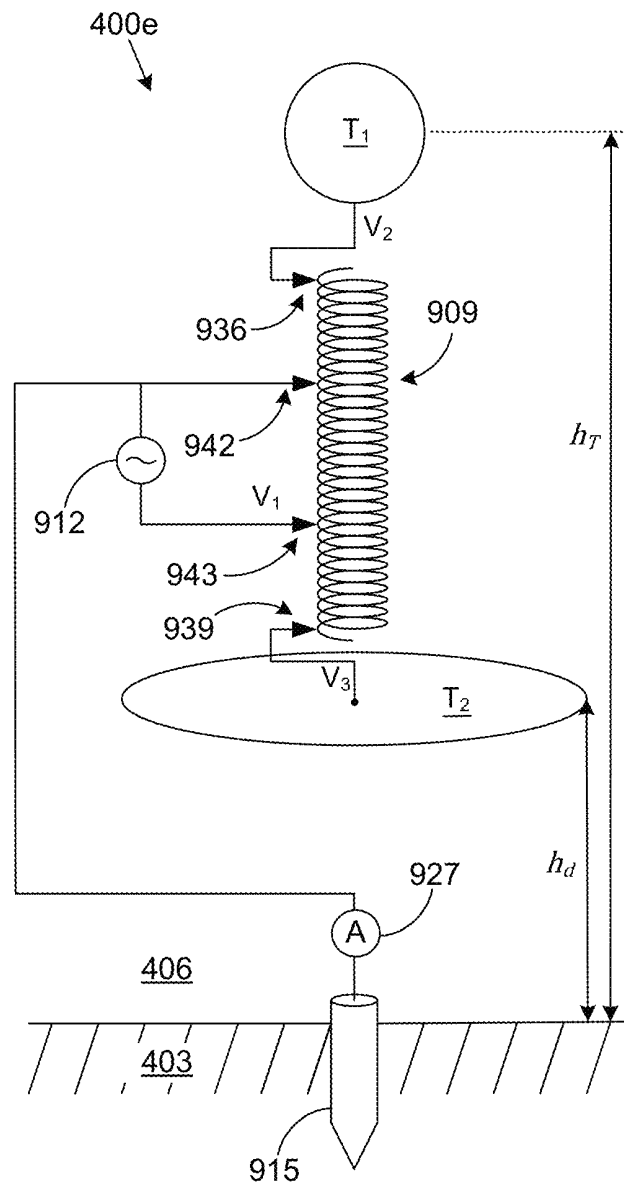
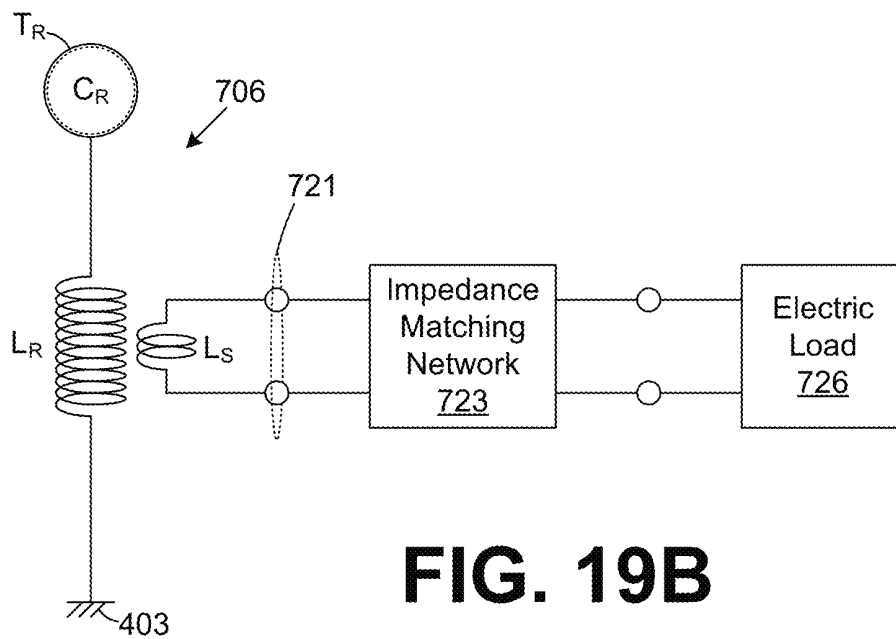
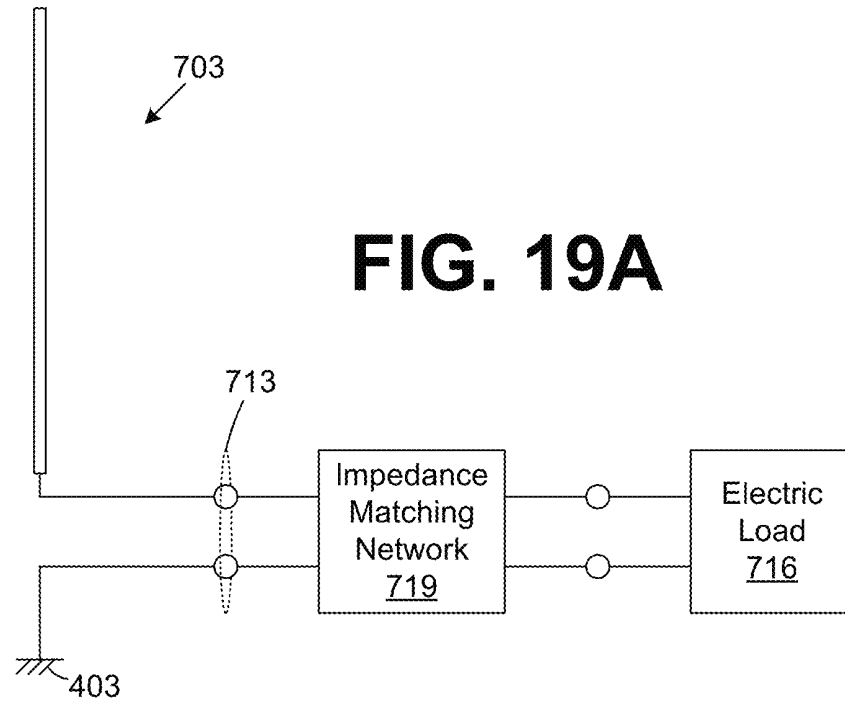


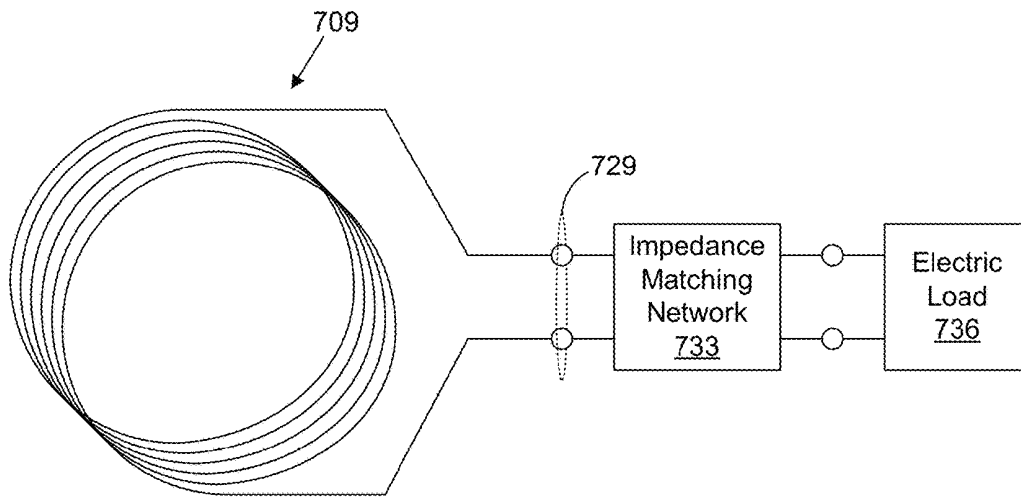
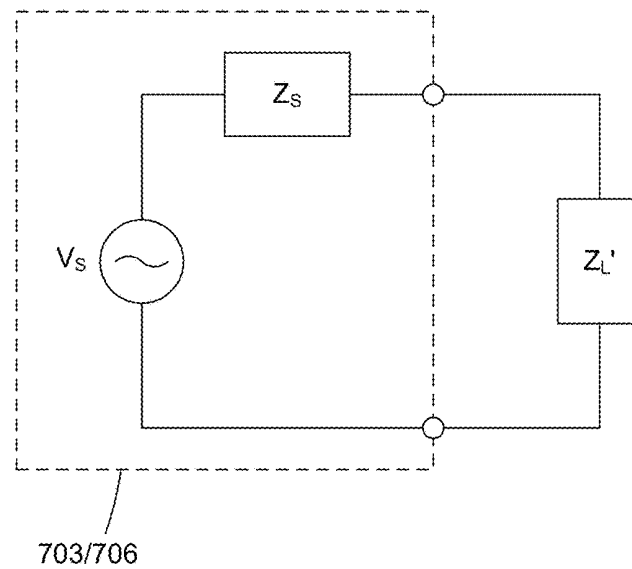
FIG. 14B

**FIG. 15****FIG. 16**

**FIG. 17**

**FIG. 18**



**FIG. 20****FIG. 21A**

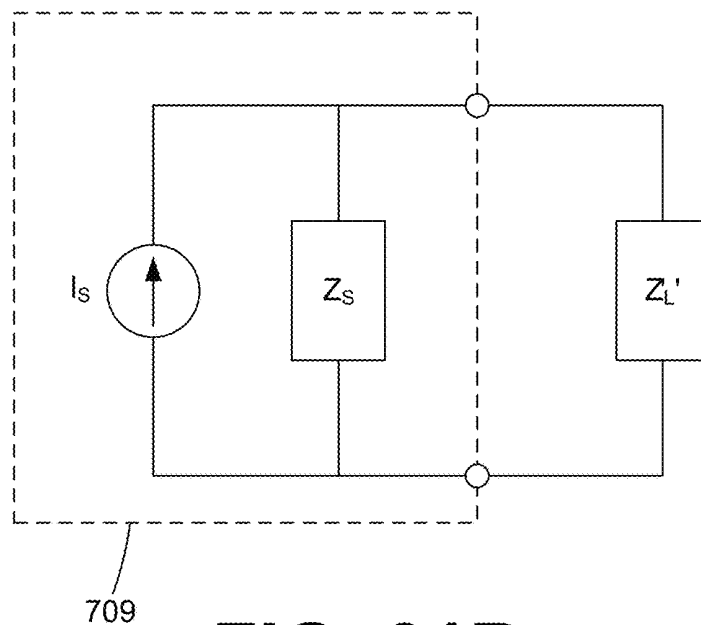


FIG. 21B

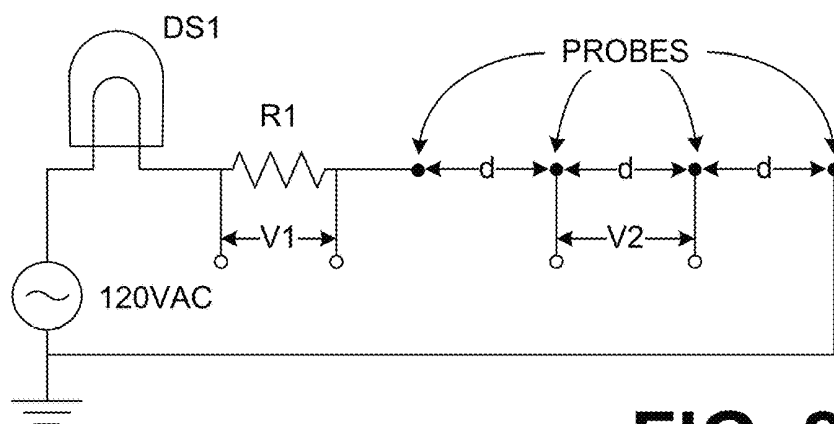


FIG. 22A

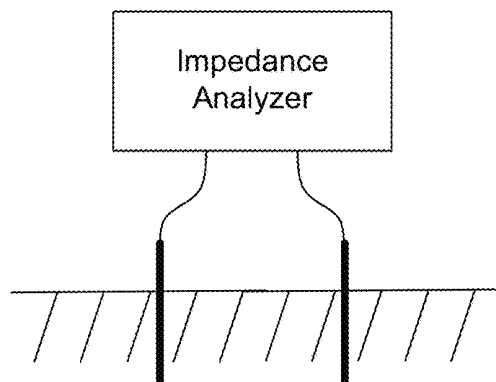
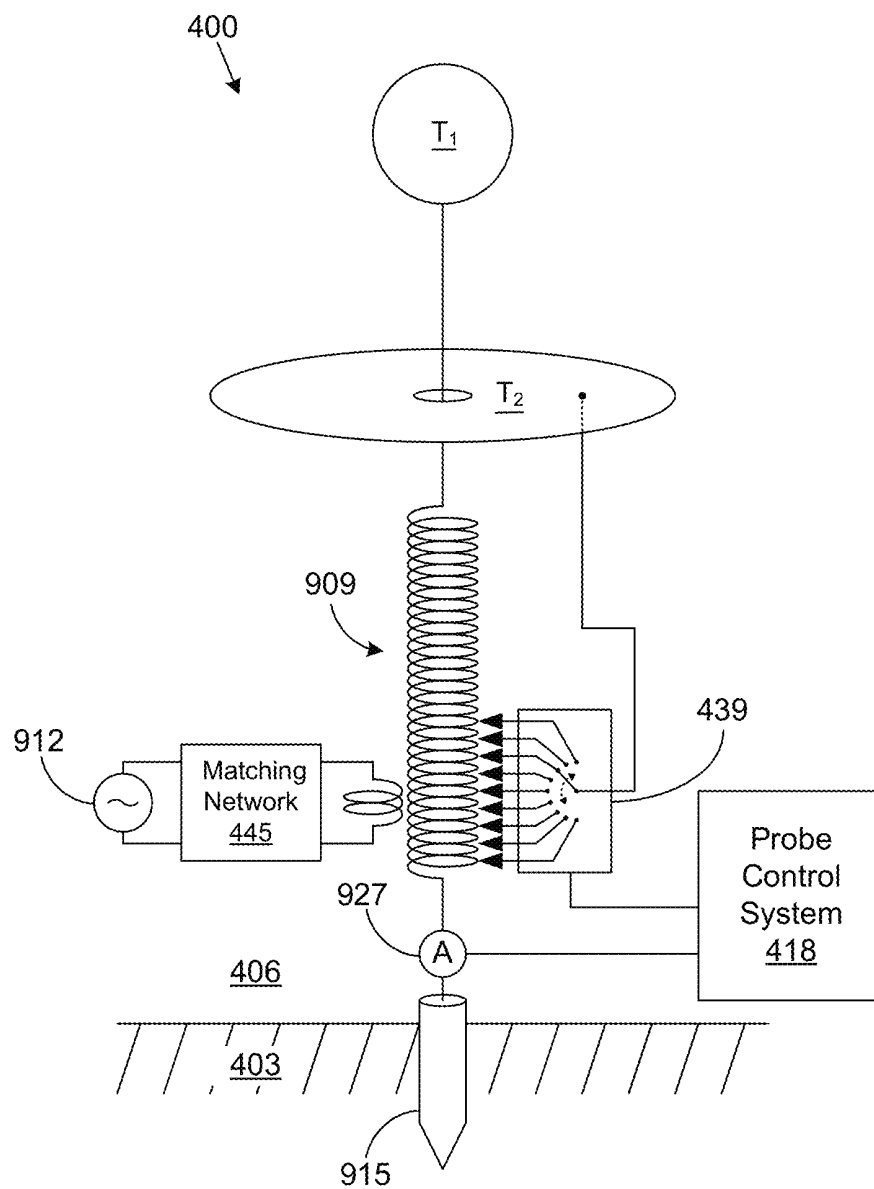
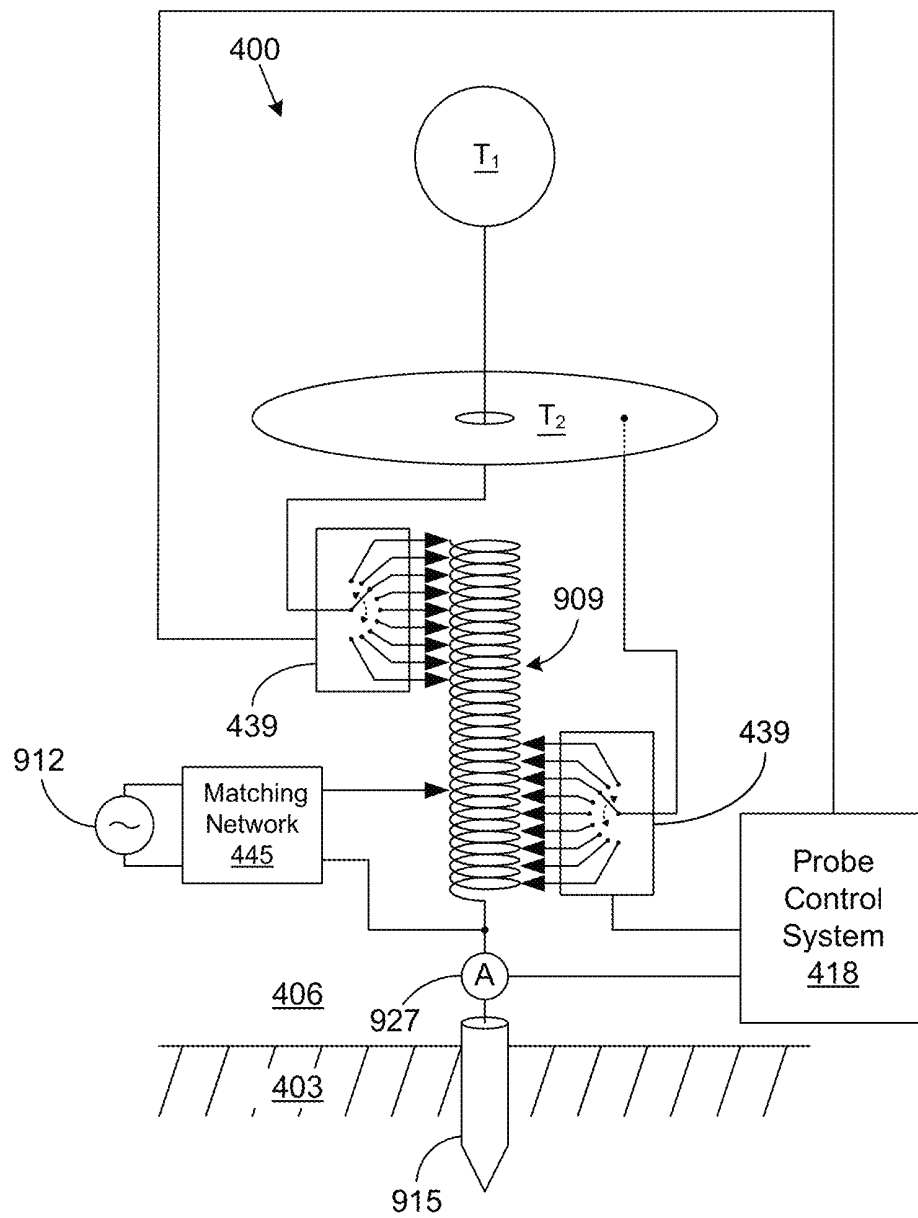
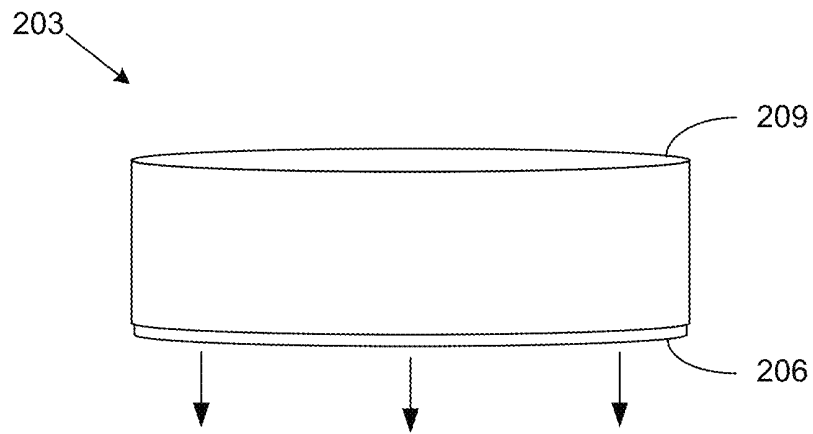
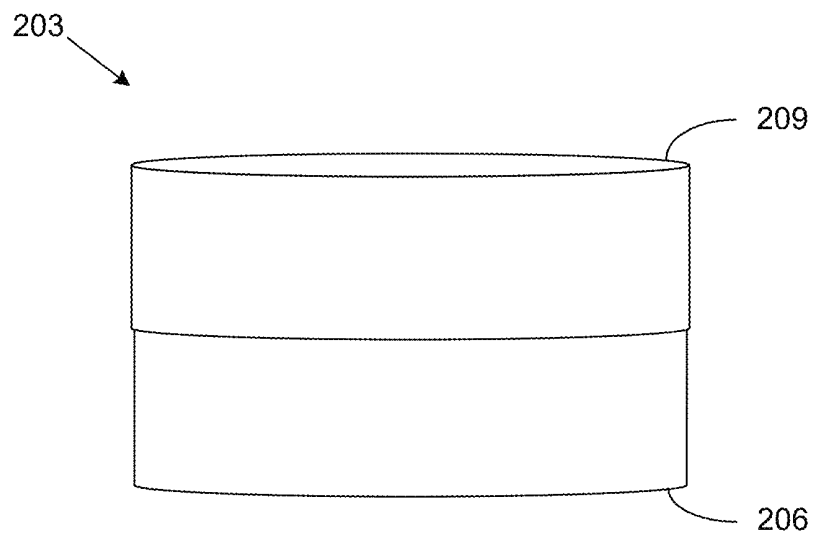


FIG. 22B

FIG. 23A

**FIG. 23B**

**FIG. 23C**

**FIG. 24A****FIG. 24B**

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EXCITATION AND USE OF GUIDED SURFACE WAVE MODES ON LOSSY MEDIA

CROSS REFERENCE TO RELATED APPLICATIONS

This application is related to U.S. application Ser. No. 13/789,538 entitled "EXCITATION AND USE OF GUIDED SURFACE WAVE MODES ON LOSSY MEDIA" filed on Mar. 7, 2013, and published on Sep. 11, 2014 (Patent Application Publication No. US-2014-0252886-A1), and U.S. application Ser. No. 13/789,525 entitled "EXCITATION AND USE OF GUIDED SURFACE WAVE MODES ON LOSSY MEDIA" filed on Mar. 7, 2013, and published on Sep. 11, 2014 (Patent Application Publication No. US-2014-0252865-A1).

BACKGROUND

For over a century, signals transmitted by radio waves involved radiation fields launched using conventional antenna structures. In contrast to radio science, electrical power distribution systems in the last century involved the transmission of energy guided along electrical conductors. This understanding of the distinction between radio frequency (RF) and power transmission has existed since the early 1900's.

BRIEF DESCRIPTION OF THE DRAWINGS

Many aspects of the present disclosure can be better understood with reference to the following drawings. The components in the drawings are not necessarily to scale, emphasis instead being placed upon clearly illustrating the principles of the disclosure. Moreover, in the drawings, like reference numerals designate corresponding parts throughout the several views.

FIG. 1 is a chart that depicts field strength as a function of distance for a guided electromagnetic field and a radiated electromagnetic field.

FIG. 2 is a drawing that illustrates a propagation interface with two regions employed for transmission of a guided surface wave according to various embodiments of the present disclosure.

FIGS. 3A and 3B are drawings that illustrate a complex angle of insertion of an electric field synthesized by guided surface waveguide probes according to the various embodiments of the present disclosure.

FIG. 4 is a drawing that illustrates a guided surface waveguide probe disposed with respect to a propagation interface of FIG. 2 according to an embodiment of the present disclosure.

FIG. 5 is a plot of an example of the magnitudes of close-in and far-out asymptotes of first order Hankel functions according to various embodiments of the present disclosure.

FIGS. 6A and 6B are plots illustrating bound charge on a sphere and the effect on capacitance according to various embodiments of the present disclosure.

FIG. 7 is a graphical representation illustrating the effect of elevation of a charge terminal on the location where a Brewster angle intersects with the lossy conductive medium according to various embodiments of the present disclosure.

FIGS. 8A and 8B are graphical representations illustrating the incidence of a synthesized electric field at a complex Brewster angle to match the guided surface waveguide mode

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at the Hankel crossover distance according to various embodiments of the present disclosure.

FIGS. 9A and 9B are graphical representations of examples of a guided surface waveguide probe according to an embodiment of the present disclosure.

FIG. 10 is a schematic diagram of the guided surface waveguide probe of FIG. 9A according to an embodiment of the present disclosure.

FIG. 11 includes plots of an example of the imaginary and real parts of a phase delay (Φ_{ϵ}) of a charge terminal T_1 of a guided surface waveguide probe of FIG. 9A according to an embodiment of the present disclosure.

FIG. 12 is an image of an example of an implemented guided surface waveguide probe of FIG. 9A according to an embodiment of the present disclosure.

FIG. 13 is a plot comparing measured and theoretical field strength of the guided surface waveguide probe of FIG. 12 according to an embodiment of the present disclosure.

FIGS. 14A and 14B are an image and graphical representation of a guided surface waveguide probe according to an embodiment of the present disclosure.

FIG. 15 is a plot of an example of the magnitudes of close-in and far-out asymptotes of first order Hankel functions according to various embodiments of the present disclosure.

FIG. 16 is a plot comparing measured and theoretical field strength of the guided surface waveguide probe of FIGS. 14A and 14B according to an embodiment of the present disclosure.

FIGS. 17 and 18 are graphical representations of examples of guided surface waveguide probes according to embodiments of the present disclosure.

FIGS. 19A and 19B depict examples of receivers that can be employed to receive energy transmitted in the form of a guided surface wave launched by a guided surface waveguide probe according to the various embodiments of the present disclosure.

FIG. 20 depicts an example of an additional receiver that can be employed to receive energy transmitted in the form of a guided surface wave launched by a guided surface waveguide probe according to the various embodiments of the present disclosure.

FIG. 21A depicts a schematic diagram representing the Thevenin-equivalent of the receivers depicted in FIGS. 19A and 19B according to an embodiment of the present disclosure.

FIG. 21B depicts a schematic diagram representing the Norton-equivalent of the receiver depicted in FIG. 17 according to an embodiment of the present disclosure.

FIGS. 22A and 22B are schematic diagrams representing examples of a conductivity measurement probe and an open wire line probe, respectively, according to an embodiment of the present disclosure.

FIGS. 23A through 23C are schematic drawings of examples of an adaptive control system employed by the probe control system of FIG. 4 according to embodiments of the present disclosure.

FIGS. 24A and 24B are drawings of an example of a variable terminal for use as a charging terminal according to an embodiment of the present disclosure.

DETAILED DESCRIPTION

To begin, some terminology shall be established to provide clarity in the discussion of concepts to follow. First, as

contemplated herein, a formal distinction is drawn between radiated electromagnetic fields and guided electromagnetic fields.

As contemplated herein, a radiated electromagnetic field comprises electromagnetic energy that is emitted from a source structure in the form of waves that are not bound to a waveguide. For example, a radiated electromagnetic field is generally a field that leaves an electric structure such as an antenna and propagates through the atmosphere or other medium and is not bound to any waveguide structure. Once radiated electromagnetic waves leave an electric structure such as an antenna, they continue to propagate in the medium of propagation (such as air) independent of their source until they dissipate regardless of whether the source continues to operate. Once electromagnetic waves are radiated, they are not recoverable unless intercepted, and, if not intercepted, the energy inherent in radiated electromagnetic waves is lost forever. Electrical structures such as antennas are designed to radiate electromagnetic fields by maximizing the ratio of the radiation resistance to the structure loss resistance. Radiated energy spreads out in space and is lost regardless of whether a receiver is present. The energy density of radiated fields is a function of distance due to geometric spreading. Accordingly, the term "radiate" in all its forms as used herein refers to this form of electromagnetic propagation.

A guided electromagnetic field is a propagating electromagnetic wave whose energy is concentrated within or near boundaries between media having different electromagnetic properties. In this sense, a guided electromagnetic field is one that is bound to a waveguide and may be characterized as being conveyed by the current flowing in the waveguide. If there is no load to receive and/or dissipate the energy conveyed in a guided electromagnetic wave, then no energy is lost except for that dissipated in the conductivity of the guiding medium. Stated another way, if there is no load for a guided electromagnetic wave, then no energy is consumed. Thus, a generator or other source generating a guided electromagnetic field does not deliver real power unless a resistive load is present. To this end, such a generator or other source essentially runs idle until a load is presented. This is akin to running a generator to generate a 60 Hertz electromagnetic wave that is transmitted over power lines where there is no electrical load. It should be noted that a guided electromagnetic field or wave is the equivalent to what is termed a "transmission line mode." This contrasts with radiated electromagnetic waves in which real power is supplied at all times in order to generate radiated waves. Unlike radiated electromagnetic waves, guided electromagnetic energy does not continue to propagate along a finite length waveguide after the energy source is turned off. Accordingly, the term "guide" in all its forms as used herein refers to this transmission mode (TM) of electromagnetic propagation.

Referring now to FIG. 1, shown is a graph 100 of field strength in decibels (dB) above an arbitrary reference in volts per meter as a function of distance in kilometers on a log-dB plot to further illustrate the distinction between radiated and guided electromagnetic fields. The graph 100 of FIG. 1 depicts a guided field strength curve 103 that shows the field strength of a guided electromagnetic field as a function of distance. This guided field strength curve 103 is essentially the same as a transmission line mode. Also, the graph 100 of FIG. 1 depicts a radiated field strength curve 106 that shows the field strength of a radiated electromagnetic field as a function of distance.

Of interest are the shapes of the curves 103 and 106 for guided wave and for radiation propagation, respectively. The radiated field strength curve 106 falls off geometrically ($1/d$, where d is distance), which is depicted as a straight line on the log-log scale. The guided field strength curve 103, on the other hand, has a characteristic exponential decay of $e^{-\alpha d}/\sqrt{d}$ and exhibits a distinctive knee 109 on the log-log scale. The guided field strength curve 103 and the radiated field strength curve 106 intersect at point 113, which occurs at a crossing distance. At distances less than the crossing distance at intersection point 113, the field strength of a guided electromagnetic field is significantly greater at most locations than the field strength of a radiated electromagnetic field. At distances greater than the crossing distance, the opposite is true. Thus, the guided and radiated field strength curves 103 and 106 further illustrate the fundamental propagation difference between guided and radiated electromagnetic fields. For an informal discussion of the difference between guided and radiated electromagnetic fields, reference is made to Milligan, T., *Modern Antenna Design*, McGraw-Hill, 1st Edition, 1985, pp. 8-9, which is incorporated herein by reference in its entirety.

The distinction between radiated and guided electromagnetic waves, made above, is readily expressed formally and placed on a rigorous basis. That two such diverse solutions could emerge from one and the same linear partial differential equation, the wave equation, analytically follows from the boundary conditions imposed on the problem. The Green function for the wave equation, itself, contains the distinction between the nature of radiation and guided waves.

In empty space, the wave equation is a differential operator whose eigenfunctions possess a continuous spectrum of eigenvalues on the complex wave-number plane. This transverse electro-magnetic (TEM) field is called the radiation field, and those propagating fields are called "Hertzian waves". However, in the presence of a conducting boundary, the wave equation plus boundary conditions mathematically lead to a spectral representation of wave-numbers composed of a continuous spectrum plus a sum of discrete spectra. To this end, reference is made to Sommerfeld, A., "Über die Ausbreitung der Wellen in der Drahtlosen Telegraphie," *Annalen der Physik*, Vol. 28, 1909, pp. 665-736. Also see Sommerfeld, A., "Problems of Radio," published as Chapter 6 in *Partial Differential Equations in Physics—Lectures on Theoretical Physics: Volume VI*, Academic Press, 1949, pp. 236-289, 295-296; Collin, R. E., "Hertzian Dipole Radiating Over a Lossy Earth or Sea: Some Early and Late 20th Century Controversies," *IEEE Antennas and Propagation Magazine*, Vol. 46, No. 2, April 2004, pp. 64-79; and Reich, H. J., Ordnung, P. F., Krauss, H. L., and Skalnik, J. G., *Microwave Theory and Techniques*, Van Nostrand, 1953, pp. 291-293, each of these references being incorporated herein by reference in their entirety.

To summarize the above, first, the continuous part of the wave-number eigenvalue spectrum, corresponding to branch-cut integrals, produces the radiation field, and second, the discrete spectra, and corresponding residue sum arising from the poles enclosed by the contour of integration, result in non-TEM traveling surface waves that are exponentially damped in the direction transverse to the propagation. Such surface waves are guided transmission line modes. For further explanation, reference is made to Friedman, B., *Principles and Techniques of Applied Mathematics*, Wiley, 1956, pp. 214, 283-286, 290, 298-300.

In free space, antennas excite the continuum eigenvalues of the wave equation, which is a radiation field, where the outwardly propagating RF energy with E_z and H_ϕ in-phase

is lost forever. On the other hand, waveguide probes excite discrete eigenvalues, which results in transmission line propagation. See Collin, R. E., *Field Theory of Guided Waves*, McGraw-Hill, 1960, pp. 453, 474-477. While such theoretical analyses have held out the hypothetical possibility of launching open surface guided waves over planar or spherical surfaces of lossy, homogeneous media, for more than a century no known structures in the engineering arts have existed for accomplishing this with any practical efficiency. Unfortunately, since it emerged in the early 1900's, the theoretical analysis set forth above has essentially remained a theory and there have been no known structures for practically accomplishing the launching of open surface guided waves over planar or spherical surfaces of lossy, homogeneous media.

According to the various embodiments of the present disclosure, various guided surface waveguide probes are described that are configured to excite electric fields that couple into a guided surface waveguide mode along the surface of a lossy conducting medium. Such guided electromagnetic fields are substantially mode-matched in magnitude and phase to a guided surface wave mode on the surface of the lossy conducting medium. Such a guided surface wave mode can also be termed a Zenneck waveguide mode. By virtue of the fact that the resultant fields excited by the guided surface waveguide probes described herein are substantially mode-matched to a guided surface waveguide mode on the surface of the lossy conducting medium, a guided electromagnetic field in the form of a guided surface wave is launched along the surface of the lossy conducting medium. According to one embodiment, the lossy conducting medium comprises a terrestrial medium such as the Earth.

Referring to FIG. 2, shown is a propagation interface that provides for an examination of the boundary value solution to Maxwell's equations derived in 1907 by Jonathan Zenneck as set forth in his paper Zenneck, J., "On the Propagation of Plane Electromagnetic Waves Along a Flat Conducting Surface and their Relation to Wireless Telegraphy," *Annalen der Physik*, Serial 4, Vol. 23, Sep. 20, 1907, pp. 846-866. FIG. 2 depicts cylindrical coordinates for radially propagating waves along the interface between a lossy conducting medium specified as Region 1 and an insulator specified as Region 2. Region 1 can comprise, for example, any lossy conducting medium. In one example, such a lossy conducting medium can comprise a terrestrial medium such as the Earth or other medium. Region 2 is a second medium that shares a boundary interface with Region 1 and has different constitutive parameters relative to Region 1. Region 2 can comprise, for example, any insulator such as the atmosphere or other medium. The reflection coefficient for such a boundary interface goes to zero only for incidence at a complex Brewster angle. See Stratton, J. A., *Electromagnetic Theory*, McGraw-Hill, 1941, p. 516.

According to various embodiments, the present disclosure sets forth various guided surface waveguide probes that generate electromagnetic fields that are substantially mode-matched to a guided surface waveguide mode on the surface of the lossy conducting medium comprising Region 1. According to various embodiments, such electromagnetic fields substantially synthesize a wave front incident at a complex Brewster angle of the lossy conducting medium that can result in zero reflection.

To explain further, in Region 2, where an $e^{j\omega t}$ field variation is assumed and where $\rho \neq 0$ and $z \geq 0$ (with z being the vertical coordinate normal to the surface of Region 1, and ρ being the radial dimension in cylindrical coordinates),

Zenneck's closed-form exact solution of Maxwell's equations satisfying the boundary conditions along the interface are expressed by the following electric field and magnetic field components:

$$H_{2\phi} = A e^{-u_2 z} H_1^{(2)}(-j\gamma\rho), \quad (1)$$

$$E_{2\rho} = A \left(\frac{u_2}{j\omega\epsilon_0} \right) e^{-u_2 z} H_1^{(2)}(-j\gamma\rho), \quad (2)$$

and

$$E_{2z} = A \left(\frac{-\gamma}{\omega\epsilon_0} \right) e^{-u_2 z} H_0^{(2)}(-j\gamma\rho). \quad (3)$$

In Region 1, where the $e^{j\omega t}$ field variation is assumed and where $\rho \neq 0$ and $z \leq 0$, Zenneck's closed-form exact solution of Maxwell's equations satisfying the boundary conditions along the interface are expressed by the following electric field and magnetic field components:

$$H_{1\phi} = A e^{u_1 z} H_1^{(2)}(-j\gamma\rho), \quad (4)$$

$$E_{1\rho} = A \left(\frac{-u_1}{\sigma_1 + j\omega\epsilon_1} \right) e^{u_1 z} H_1^{(2)}(-j\gamma\rho), \quad (5)$$

and

$$E_{1z} = A \left(\frac{-j\gamma}{\sigma_1 + j\omega\epsilon_1} \right) e^{u_1 z} H_0^{(2)}(-j\gamma\rho). \quad (6)$$

In these expressions, z is the vertical coordinate normal to the surface of Region 1 and ρ is the radial coordinate, $H_n^{(2)}(-j\gamma\rho)$ is a complex argument Hankel function of the second kind and order n , u_1 is the propagation constant in the positive vertical (z) direction in Region 1, u_2 is the propagation constant in the vertical (z) direction in Region 2, σ_1 is the conductivity of Region 1, ω is equal to $2\pi f$, where f is a frequency of excitation, ϵ_0 is the permittivity of free space, ϵ_1 is the permittivity of Region 1, A is a source constant imposed by the source, and γ is a surface wave radial propagation constant.

The propagation constants in the $\pm z$ directions are determined by separating the wave equation above and below the interface between Regions 1 and 2, and imposing the boundary conditions. This exercise gives, in Region 2,

$$u_2 = \frac{-jk_0}{\sqrt{1 + (\epsilon_r - j\chi)}} \quad (7)$$

and gives, in Region 1,

$$u_1 = -u_2(\epsilon_r - j\chi). \quad (8)$$

The radial propagation constant γ is given by

$$\gamma = j\sqrt{k_0^2 + u_2^2} = j\frac{k_0 n}{\sqrt{1 + n^2}}, \quad (9)$$

which is a complex expression where n is the complex index of refraction given by

$$n = \sqrt{\epsilon_r - j\chi}. \quad (10)$$

In all of the above Equations,

$$x = \frac{\sigma_1}{\omega \epsilon_o}, \quad (11)$$

and

$$k_o = \omega \sqrt{\mu_o \epsilon_o} = \frac{\lambda_o}{2\pi}, \quad (12)$$

where μ_o comprises the permeability of free space, ϵ_r comprises relative permittivity of Region 1. Thus, the generated surface wave propagates parallel to the interface and exponentially decays vertical to it. This is known as evanescence.

Thus, Equations (1)-(3) can be considered to be a cylindrically-symmetric, radially-propagating waveguide mode. See Barlow, H. M., and Brown, J., *Radio Surface Waves*, Oxford University Press, 1962, pp. 10-12, 29-33. The present disclosure details structures that excite this "open boundary" waveguide mode. Specifically, according to various embodiments, a guided surface waveguide probe is provided with a charge terminal of appropriate size that is fed with voltage and/or current and is positioned relative to the boundary interface between Region 2 and Region 1 to produce the complex Brewster angle at the boundary interface to excite the surface waveguide mode with no or minimal reflection. A compensation terminal of appropriate size can be positioned relative to the charge terminal, and fed with voltage and/or current, to refine the Brewster angle at the boundary interface.

To continue, the Leontovich impedance boundary condition between Region 1 and Region 2 is stated as

$$\hat{n} \times \vec{H}_2(\rho, \phi, 0) = \vec{J}_s, \quad (13)$$

where $\hat{n}$ is a unit normal in the positive vertical (+z) direction and $\vec{H}_2$ is the magnetic field strength in Region 2 expressed by Equation (1) above. Equation (13) implies that the electric and magnetic fields specified in Equations (1)-(3) may result in a radial surface current density along the boundary interface, such radial surface current density being specified by

$$J_p(\rho') = -A H_1^{(2)}(-j\gamma\rho') \quad (14)$$

where A is a constant. Further, it should be noted that close-in to the guided surface waveguide probe (for $p \ll \lambda$), Equation (14) above has the behavior

$$J_{\text{close}}(\rho') = \frac{-A(j2)}{\pi(-j\gamma\rho')} = -H_\phi = -\frac{I_o}{2\pi\rho'}. \quad (15)$$

The negative sign means that when source current (I_o) flows vertically upward, the required "close-in" ground current flows radially inward. By field matching on H_ϕ "close-in" we find that

$$A = -\frac{I_o\gamma}{4} \quad (16)$$

in Equations (1)-(6) and (14). Therefore, the radial surface current density of Equation (14) can be restated as

$$J_p(\rho') = \frac{I_o\gamma}{4} H_1^{(2)}(-j\gamma\rho'). \quad (17)$$

The fields expressed by Equations (1)-(6) and (17) have the nature of a transmission line mode bound to a lossy interface, not radiation fields such as are associated with ground-wave propagation. See Barlow, H. M. and Brown, J., *Radio Surface Waves*, Oxford University Press, 1962, pp. 1-5.

At this point, a review of the nature of the Hankel functions used in Equations (1)-(6) and (17) is provided for these solutions of the wave equation. One might observe that the Hankel functions of the first and second kind and order n are defined as complex combinations of the standard Bessel functions of the first and second kinds

$$H_n^{(1)}(x) = J_n(x) + jN_n(x), \text{ and} \quad (18)$$

$$H_n^{(2)}(x) = J_n(x) - jN_n(x), \quad (19)$$

These functions represent cylindrical waves propagating radially inward ($H_n^{(1)}$) and outward ($H_n^{(2)}$), respectively. The definition is analogous to the relationship $e^{\pm jx} = \cos x \pm j \sin x$. See, for example, Harrington, R. F., *Time-Harmonic Fields*, McGraw-Hill, 1961, pp. 460-463.

That $H_n^{(2)}(k_p\rho)$ is an outgoing wave can be recognized from its large argument asymptotic behavior that is obtained directly from the series definitions of $J_n(x)$ and $N_n(x)$. Far-out from the guided surface waveguide probe:

$$H_n^{(2)}(x) \xrightarrow{x \rightarrow \infty} \sqrt{\frac{2j}{\pi x}} j^n e^{-jx} = \sqrt{\frac{2}{\pi x}} j^n e^{-j(x - \frac{\pi}{4})}, \quad (20a)$$

which, when multiplied by $e^{j\omega t}$, is an outward propagating cylindrical wave of the form $e^{j(\omega t - k_p\rho)}$ with a $1/\sqrt{\rho}$ spatial variation. The first order (n=1) solution can be determined from Equation (20a) to be

$$H_1^{(2)}(x) \xrightarrow{x \rightarrow \infty} j \sqrt{\frac{2j}{\pi x}} e^{-jx} = \sqrt{\frac{2}{\pi x}} e^{-j(x - \frac{\pi}{2} - \frac{\pi}{4})}. \quad (20b)$$

Close-in to the guided surface waveguide probe (for $\rho \ll \lambda$), the Hankel function of first order and the second kind behaves as:

$$H_1^{(2)}(x) \xrightarrow{x \rightarrow 0} \frac{2j}{\pi x}. \quad (21)$$

Note that these asymptotic expressions are complex quantities. When x is a real quantity, Equations (20b) and (21) differ in phase by $\sqrt{j}$, which corresponds to an extra phase advance or "phase boost" of 45° or, equivalently, $\lambda/8$. The close-in and far-out asymptotes of the first order Hankel function of the second kind have a Hankel "crossover" or transition point where they are of equal magnitude at a distance of $\rho = R_x$. The distance to the Hankel crossover point can be found by equating Equations (20b) and (21), and solving for R_x . With $x = \sigma/\omega\epsilon_o$, it can be seen that the far-out and close-in Hankel function asymptotes are frequency dependent, with the Hankel crossover point moving out as the frequency is lowered. It should also be noted that the Hankel function asymptotes may also vary as the conductivity (σ) of the lossy conducting medium changes. For example, the conductivity of the soil can vary with changes in weather conditions.

Guided surface waveguide probes can be configured to establish an electric field having a wave tilt that corresponds

to a wave illuminating the surface of the lossy conducting medium at a complex angle, thereby exciting radial surface currents by substantially mode-matching to a guided surface wave mode at the Hankel crossover point at R_x .

Referring now to FIG. 3A, shown is a ray optic interpretation of an incident field (E) polarized parallel to a plane of incidence. The electric field vector E is to be synthesized as an incoming non-uniform plane wave, polarized parallel to the plane of incidence. The electric field vector E can be created from independent horizontal and vertical components as:

$$\vec{E}(\theta_0) = E_\rho \hat{\rho} + E_z \hat{z}. \quad (22)$$

Geometrically, the illustration in FIG. 3A suggests that the electric field vector E can be given by:

$$E_\rho(\rho, z) = E(\rho, z) \cos \theta_0, \quad (23a)$$

and

$$E_z(\rho, z) = E(\rho, z) \cos\left(\frac{\pi}{2} - \theta_0\right) = E(\rho, z) \sin \theta_0, \quad (23b)$$

which means that the field ratio is

$$\frac{E_\rho}{E_z} = \tan \theta_0. \quad (24)$$

Using the electric field and magnetic field components from the electric field and magnetic field component solutions, the surface waveguide impedances can be expressed. The radial surface waveguide impedance can be written as

$$Z_\rho = \frac{-E_z}{H_\phi} = \frac{\gamma}{j\omega\epsilon_0}, \quad (25)$$

and the surface-normal impedance can be written as

$$Z_z = \frac{-E_\rho}{H_\phi} = \frac{-u_2}{j\omega\epsilon_0}. \quad (26)$$

A generalized parameter W, called “wave tilt,” is noted herein as the ratio of the horizontal electric field component to the vertical electric field component given by

$$W = \frac{E_\rho}{E_z} = |W|e^{j\theta}, \quad (27)$$

which is complex and has both magnitude and phase.

For a TEM wave in Region 2, the wave tilt angle is equal to the angle between the normal of the wave-front at the boundary interface with Region 1 and the tangent to the boundary interface. This may be easier to see in FIG. 3B, which illustrates equi-phase surfaces of a TEM wave and their normals for a radial cylindrical guided surface wave. At the boundary interface ($z=0$) with a perfect conductor, the wave-front normal is parallel to the tangent of the boundary interface, resulting in $W=0$. However, in the case of a lossy dielectric, a wave tilt W exists because the wave-front normal is not parallel with the tangent of the boundary interface at $z=0$.

This may be better understood with reference to FIG. 4, which shows an example of a guided surface waveguide probe 400a that includes an elevated charge terminal T_1 and a lower compensation terminal T_2 that are arranged along a vertical axis z that is normal to a plane presented by the lossy conducting medium 403. In this respect, the charge terminal T_1 is placed directly above the compensation terminal T_2 although it is possible that some other arrangement of two or more charge and/or compensation terminals T_N can be used. The guided surface waveguide probe 400a is disposed above a lossy conducting medium 403 according to an embodiment of the present disclosure. The lossy conducting medium 403 makes up Region 1 (FIGS. 2, 3A and 3B) and a second medium 406 shares a boundary interface with the lossy conducting medium 403 and makes up Region 2 (FIGS. 2, 3A and 3B).

The guided surface waveguide probe 400a includes a coupling circuit 409 that couples an excitation source 412 to the charge and compensation terminals T_1 and T_2 . According to various embodiments, charges Q_1 and Q_2 can be imposed on the respective charge and compensation terminals T_1 and T_2 , depending on the voltages applied to terminals T_1 and T_2 at any given instant. I_1 is the conduction current feeding the charge Q_1 on the charge terminal T_1 , and I_2 is the conduction current feeding the charge Q_2 on the compensation terminal T_2 .

The concept of an electrical effective height can be used to provide insight into the construction and operation of the guided surface waveguide probe 400a. The electrical effective height (h_{eff}) has been defined as

$$h_{eff} = \frac{1}{I_0} \int_0^{h_p} I(z) dz \quad (28a)$$

for a monopole with a physical height (or length) of h_p , and as

$$h_{eff} = \frac{1}{I_0} \int_{-h_p}^{h_p} I(z) dz \quad (28b)$$

for a doublet or dipole. These expressions differ by a factor of 2 since the physical length of a dipole, $2h_p$, is twice the physical height of the monopole, h_p . Since the expressions depend upon the magnitude and phase of the source distribution, effective height (or length) is complex in general. The integration of the distributed current $I(z)$ of the monopole antenna structure is performed over the physical height of the structure (h_p), and normalized to the ground current (I_0) flowing upward through the base (or input) of the structure. The distributed current along the structure can be expressed by

$$I(z) = I_C \cos(\beta_0 z), \quad (29)$$

where β_0 is the propagation factor for free space. In the case of the guided surface waveguide probe 400a of FIG. 4, I_C is the current distributed along the vertical structure.

This may be understood using a coupling circuit 409 that includes a low loss coil (e.g., a helical coil) at the bottom of the structure and a supply conductor connected to the charge terminal T_1 . With a coil or a helical delay line of physical length l_c and a propagation factor of

$$\beta_p = \frac{2\pi}{\lambda_p} = \frac{2\pi}{V_f \lambda_0}, \quad (30)$$

where V_f is the velocity factor on the structure, λ_0 is the wavelength at the supplied frequency, and λ_p is the propagation wavelength resulting from any velocity factor V_f , the phase delay on the structure is $\Phi = \beta_p l_c$, and the current fed to the top of the coil from the bottom of the physical structure is

$$I_C(\beta_p l_c) = I_0 e^{j\Phi}, \quad (31)$$

with the phase Φ measured relative to the ground (stake) current I_0 . Consequently, the electrical effective height of the guided surface waveguide probe **400a** in FIG. 4 can be approximated by

$$h_{eff} = \frac{1}{I_0} \int_0^{h_p} I_0 e^{j\Phi} \cos(\beta_0 z) dz \cong h_p e^{j\Phi}, \quad (32)$$

for the case where the physical height $h_p \ll \lambda_0$, the wavelength at the supplied frequency. A dipole antenna structure may be evaluated in a similar fashion. The complex effective height of a monopole, $h_{eff} = h_p$, at an angle Φ (or the complex effective length for a dipole $h_{eff} = 2h_p e^{j\Phi}$), may be adjusted to cause the source fields to match a guided surface waveguide mode and cause a guided surface wave to be launched on the lossy conducting medium **403**.

According to the embodiment of FIG. 4, the charge terminal T_1 is positioned over the lossy conducting medium **403** at a physical height H_1 , and the compensation terminal T_2 is positioned directly below T_1 along the vertical axis z at a physical height H_2 , where H_2 is less than H_1 . The height h of the transmission structure may be calculated as $h = H_1 - H_2$. The charge terminal T_1 has an isolated capacitance C_1 , and the compensation terminal T_2 has an isolated capacitance C_2 . A mutual capacitance C_M can also exist between the terminals T_1 and T_2 depending on the distance therebetween. During operation, charges Q_1 and Q_2 are imposed on the charge terminal T_1 and compensation terminal T_2 , respectively, depending on the voltages applied to the charge terminal T_1 and compensation terminal T_2 at any given instant.

According to one embodiment, the lossy conducting medium **403** comprises a terrestrial medium such as the planet Earth. To this end, such a terrestrial medium comprises all structures or formations included thereon whether natural or man-made. For example, such a terrestrial medium can comprise natural elements such as rock, soil, sand, fresh water, sea water, trees, vegetation, and all other natural elements that make up our planet. In addition, such a terrestrial medium can comprise man-made elements such as concrete, asphalt, building materials, and other man-made materials. In other embodiments, the lossy conducting medium **403** can comprise some medium other than the Earth, whether naturally occurring or man-made. In other embodiments, the lossy conducting medium **403** can comprise other media such as man-made surfaces and structures such as automobiles, aircraft, man-made materials (such as plywood, plastic sheeting, or other materials) or other media.

In the case that the lossy conducting medium **403** comprises a terrestrial medium or Earth, the second medium **406** can comprise the atmosphere above the ground. As such, the atmosphere can be termed an "atmospheric medium" that

comprises air and other elements that make up the atmosphere of the Earth. In addition, it is possible that the second medium **406** can comprise other media relative to the lossy conducting medium **403**.

Referring back to FIG. 4, the effect of the lossy conducting medium **403** in Region 1 can be examined using image theory analysis. This analysis with respect to the lossy conducting medium assumes the presence of induced effective image charges Q_1' and Q_2' beneath the guided surface waveguide probes coinciding with the charges Q_1 and Q_2 on the charge and compensation terminals T_1 and T_2 as illustrated in FIG. 4. Such image charges Q_1' and Q_2' are not merely 180° out of phase with the primary source charges Q_1 and Q_2 on the charge and compensation terminals T_1 and T_2 , as they would be in the case of a perfect conductor. A lossy conducting medium such as, for example, a terrestrial medium presents phase shifted images. That is to say, the image charges Q_1' and Q_2' are at complex depths. For a discussion of complex images, reference is made to Wait, J. R., "Complex Image Theory—Revisited," *IEEE Antennas and Propagation Magazine*, Vol. 33, No. 4, August 1991, pp. 27-29, which is incorporated herein by reference in its entirety.

Instead of the image charges Q_1' and Q_2' being at a depth that is equal to the physical height (H_n) of the charges Q_1 and Q_2 , a conducting image ground plane **415** (representing a perfect conductor) is placed at a complex depth of $z = -d/2$ and the image charges appear at complex depths (i.e., the "depth" has both magnitude and phase), given by $-D_n = -(d/2 + d/2 + H_n) = -H_n$, where $n=1, 2, \dots$, and for vertically polarized sources,

$$d = \frac{2\sqrt{\gamma_e^2 + k_0^2}}{\gamma_e^2} \approx \frac{2}{\gamma_e} = d_r + jd_i = |d| \angle \zeta, \quad (33)$$

where

$$\gamma_e^2 = j\omega u_1 \sigma_1 - \omega^2 u_1 \epsilon_1, \quad (34)$$

and

$$k_0 = \omega \sqrt{u_0 \epsilon_0}. \quad (35)$$

as indicated in Equation (12). In the lossy conducting medium, the wave front normal is parallel to the tangent of the conducting image ground plane **415** at $z = -d/2$, and not at the boundary interface between Regions 1 and 2.

The complex spacing of image charges Q_1' and Q_2' , in turn, implies that the external fields will experience extra phase shifts not encountered when the interface is either a lossless dielectric or a perfect conductor. The essence of the lossy dielectric image-theory technique is to replace the finitely conducting Earth (or lossy dielectric) by a perfect conductor located at the complex depth, $z = -d/2$ with source images located at complex depths of $D_n = d + H_n$. Thereafter, the fields above ground ($z \geq 0$) can be calculated using a superposition of the physical charge Q_n (at $z = +H_n$) plus its image Q_n' (at $z' = -D_n$).

Given the foregoing discussion, the asymptotes of the radial surface waveguide current at the surface of the lossy conducting medium $J_\rho(\rho)$ can be determined to be $J_1(\rho)$ when close-in and $J_2(\rho)$ when far-out, where

$$\text{Close-in } (\rho < \lambda/8): J_\rho(\rho) \sim J_1 = \frac{I_1 + I_2}{2\pi\rho} + \frac{E_\rho^{QS}(Q_1) + E_\rho^{QS}(Q_2)}{Z_\rho}, \quad (36)$$

and

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-continued

$$\text{Far-out } (\rho \gg \lambda/8): J_\rho(\rho) \sim J_2 = \frac{j\gamma\omega Q_1}{4} \times \sqrt{\frac{2\gamma}{\pi}} \times \frac{e^{-(\alpha+j\beta)\rho}}{\sqrt{\rho}}, \quad (37)$$

where α and β are constants related to the decay and propagation phase of the far-out radial surface current density, respectively. As shown in FIG. 4, I_1 is the conduction current feeding the charge Q_1 on the elevated charge terminal T_1 , and I_2 is the conduction current feeding the charge Q_2 on the lower compensation terminal T_2 .

According to one embodiment, the shape of the charge terminal T_1 is specified to hold as much charge as practically possible. Ultimately, the field strength of a guided surface wave launched by a guided surface waveguide probe 400a is directly proportional to the quantity of charge on the terminal T_1 . In addition, bound capacitances may exist between the respective charge terminal T_1 and compensation terminal T_2 and the lossy conducting medium 403 depending on the heights of the respective charge terminal T_1 and compensation terminal T_2 with respect to the lossy conducting medium 403.

The charge Q_1 on the upper charge terminal T_1 may be determined by $Q_1 = C_1 V_1$, where C_1 is the isolated capacitance of the charge terminal T_1 and V_1 is the voltage applied to the charge terminal T_1 . In the example of FIG. 4, the spherical charge terminal T_1 can be considered a capacitor, and the compensation terminal T_2 can comprise a disk or lower capacitor. However, in other embodiments the terminals T_1 and/or T_2 can comprise any conductive mass that can hold the electrical charge. For example, the terminals T_1 and/or T_2 can include any shape such as a sphere, a disk, a cylinder, a cone, a torus, a hood, one or more rings, or any other randomized shape or combination of shapes. If the terminals T_1 and/or T_2 are spheres or disks, the respective self-capacitance C_1 and C_2 can be calculated. The capacitance of a sphere at a physical height of h above a perfect ground is given by

$$C_{\text{elevated sphere}} = 4\pi\epsilon_0 a (1 + M + M^2 + M^3 + 2M^4 + 3M^5 + \dots), \quad (38)$$

where the diameter of the sphere is $2a$ and $M = a/2h$.

In the case of a sufficiently isolated terminal, the self-capacitance of a conductive sphere can be approximated by $C = 4\pi\epsilon_0 a$, where a comprises the radius of the sphere in meters, and the self-capacitance of a disk can be approximated by $C = 8\epsilon_0 a$, where a comprises the radius of the disk in meters. Also note that the charge terminal T_1 and compensation terminal T_2 need not be identical as illustrated in FIG. 4. Each terminal can have a separate size and shape, and include different conducting materials. A probe control system 418 is configured to control the operation of the guided surface waveguide probe 400a.

Consider the geometry at the interface with the lossy conducting medium 403, with respect to the charge Q_1 on the elevated charge terminal T_1 . As illustrated in FIG. 3A, the relationship between the field ratio and the wave tilt is

$$\frac{E_\rho}{E_z} = \frac{E \sin\psi}{E \cos\psi} = \tan\psi = W = |W|e^{j\psi}, \text{ and} \quad (39)$$

$$\frac{E_z}{E_\rho} = \frac{E \sin\theta}{E \cos\theta} = \tan\theta = \frac{1}{W} = \frac{1}{|W|}e^{-j\psi}. \quad (40)$$

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For the specific case of a guided surface wave launched in a transmission mode (TM), the wave tilt field ratio is given by

$$W = \frac{E_\rho}{E_z} = \frac{u_1}{-j\gamma} \frac{H_1^{(2)}(-j\gamma\rho)}{H_0^{(2)}(-j\gamma\rho)} \cong \frac{1}{n}, \quad (41)$$

when

$$H_n^{(2)}(x) \xrightarrow{x \rightarrow \infty} j^n H_0^{(2)}(x).$$

Applying Equation (40) to a guided surface wave gives

$$\tan\theta_{i,B} = \frac{E_z}{E_\rho} = \frac{u_2}{\gamma} = \sqrt{\epsilon_r - jx} = n = \frac{1}{W} = \frac{1}{|W|}e^{-j\psi}. \quad (42)$$

With the angle of incidence equal to the complex Brewster angle ($\theta_{i,B}$), the reflection coefficient vanishes, as shown by

$$\Gamma_{||}(\theta_{i,B}) = \frac{\sqrt{(\epsilon_r - jx) - \sin^2\theta_i} - (\epsilon_r - jx)\cos\theta_i}{\sqrt{(\epsilon_r - jx) - \sin^2\theta_i} + (\epsilon_r - jx)\cos\theta_i} \Big|_{\theta_i=\theta_{i,B}} = 0. \quad (43)$$

By adjusting the complex field ratio, an incident field can be synthesized to be incident at a complex angle at which the reflection is reduced or eliminated. As in optics, minimizing the reflection of the incident electric field can improve and/or maximize the energy coupled into the guided surface waveguide mode of the lossy conducting medium 403. A larger reflection can hinder and/or prevent a guided surface wave from being launched. Establishing this ratio as $n = \sqrt{\epsilon_r - jx}$ gives an incidence at the complex Brewster angle, making the reflections vanish.

Referring to FIG. 5, shown is an example of a plot of the magnitudes of the first order Hankel functions of Equations (20b) and (21) for a Region 1 conductivity of $\sigma = 0.010$ mhos/m and relative permittivity $\epsilon_r = 15$, at an operating frequency of 1850 kHz. Curve 503 is the magnitude of the far-out asymptote of Equation (20b) and curve 506 is the magnitude of the close-in asymptote of Equation (21), with the Hankel crossover point 509 occurring at a distance of $R_x = 54$ feet. While the magnitudes are equal, a phase offset exists between the two asymptotes at the Hankel crossover point 509. According to various embodiments, a guided electromagnetic field can be launched in the form of a guided surface wave along the surface of the lossy conducting medium with little or no reflection by matching the complex Brewster angle ($\theta_{i,B}$) at the Hankel crossover point 509.

Out beyond the Hankel crossover point 509, the large argument asymptote predominates over the "close-in" representation of the Hankel function, and the vertical component of the mode-matched electric field of Equation (3) asymptotically passes to

$$E_{2z} \xrightarrow{\rho \rightarrow \infty} \left(\frac{q_{free}}{\epsilon_0} \right) \sqrt{\frac{\gamma^3}{8\pi}} e^{-u_2 z} \frac{e^{-j(\gamma\rho - \pi/4)}}{\sqrt{\rho}}, \quad (44)$$

which is linearly proportional to free charge on the isolated component of the elevated charge terminal's capacitance at the terminal voltage, $q_{free} = C_{free} \times V_T$. The height H_1 of the elevated charge terminal T_1 (FIG. 4) affects the amount of free charge on the charge terminal T_1 . When the charge terminal T_1 is near the image ground plane 415 (FIG. 4), most of the charge Q_1 on the terminal is "bound" to its image charge. As the charge terminal T_1 is elevated, the bound charge is lessened until the charge terminal T_1 reaches a height at which substantially all of the isolated charge is free.

The advantage of an increased capacitive elevation for the charge terminal T_1 is that the charge on the elevated charge terminal T_1 is further removed from the image ground plane 415, resulting in an increased amount of free charge q_{free} to couple energy into the guided surface waveguide mode.

FIGS. 6A and 6B are plots illustrating the effect of elevation (h) on the free charge distribution on a spherical charge terminal with a diameter of $D=32$ inches. FIG. 6A shows the angular distribution of the charge around the spherical terminal for physical heights of 6 feet (curve 603), 10 feet (curve 606) and 34 feet (curve 609) above a perfect ground plane. As the charge terminal is moved away from the ground plane, the charge distribution becomes more uniformly distributed about the spherical terminal. In FIG. 6B, curve 612 is a plot of the capacitance of the spherical terminal as a function of physical height (h) in feet based upon Equation (38). For a sphere with a diameter of 32 inches, the isolated capacitance (C_{iso}) is 45.2 pF, which is illustrated in FIG. 6B as line 615. From FIGS. 6A and 6B, it can be seen that for elevations of the charge terminal T_1 that are about four diameters (4D) or greater, the charge distribution is approximately uniform about the spherical terminal, which can improve the coupling into the guided surface waveguide mode. The amount of coupling may be expressed as the efficiency at which a guided surface wave is launched (or "launching efficiency") in the guided surface waveguide mode. A launching efficiency of close to 100% is possible. For example, launching efficiencies of greater than 99%, greater than 98%, greater than 95%, greater than 90%, greater than 85%, greater than 80%, and greater than 75% can be achieved.

However, with the ray optic interpretation of the incident field (E), at greater charge terminal heights, the rays intersecting the lossy conducting medium at the Brewster angle do so at substantially greater distances from the respective guided surface waveguide probe. FIG. 7 graphically illustrates the effect of increasing the physical height of the sphere on the distance where the electric field is incident at the Brewster angle. As the height is increased from h_1 through h_2 to h_3 , the point where the electric field intersects with the lossy conducting medium (e.g., the earth) at the Brewster angle moves further away from the charge. The weaker electric field strength resulting from geometric spreading at these greater distances reduces the effectiveness of coupling into the guided surface waveguide mode. Stated another way, the efficiency at which a guided surface wave is launched (or the "launching efficiency") is reduced. However, compensation can be provided that reduces the distance at which the electric field is incident with the lossy conducting medium at the Brewster angle as will be described.

Referring now to FIG. 8A, an example of the complex angle trigonometry is shown for the ray optic interpretation of the incident electric field (E) of the charge terminal T_1 with a complex Brewster angle ($\theta_{i,B}$) at the Hankel crossover

distance (R_x). Recall from Equation (42) that, for a lossy conducting medium, the Brewster angle is complex and specified by

$$\tan \theta_{i,B} = \sqrt{\epsilon_r - j \frac{\sigma}{\omega \epsilon_0}} = n. \quad (45)$$

Electrically, the geometric parameters are related by the electrical effective height (h_{eff}) of the charge terminal T_1 by

$$R_x \tan \psi_{i,B} = R_x \times W = h_{eff} = h_p e^{j\Phi}, \quad (46)$$

where $\psi_{i,B} = (\pi/2) - \theta_{i,B}$ is the Brewster angle measured from the surface of the lossy conducting medium. To couple into the guided surface waveguide mode, the wave tilt of the electric field at the Hankel crossover distance can be expressed as the ratio of the electrical effective height and the Hankel crossover distance

$$\frac{h_{eff}}{R_x} = \tan \psi_{i,B} = W_{R_x}. \quad (47)$$

Since both the physical height (h_p) and the Hankel crossover distance (R_x) are real quantities, the angle of the desired guided surface wave tilt at the Hankel crossover distance (W_{R_x}) is equal to the phase (Φ) of the complex effective height (h_{eff}). This implies that by varying the phase at the supply point of the coil, and thus the phase shift in Equation (32), the complex effective height can be manipulated and the wave tilt adjusted to synthetically match the guided surface waveguide mode at the Hankel crossover point 509.

In FIG. 8A, a right triangle is depicted having an adjacent side of length R_x along the lossy conducting medium surface and a complex Brewster angle $\psi_{i,B}$ measured between a ray extending between the Hankel crossover point at R_x and the center of the charge terminal T_1 , and the lossy conducting medium surface between the Hankel crossover point and the charge terminal T_1 . With the charge terminal T_1 positioned at physical height h_p and excited with a charge having the appropriate phase Φ , the resulting electric field is incident with the lossy conducting medium boundary interface at the Hankel crossover distance R_x , and at the Brewster angle. Under these conditions, the guided surface waveguide mode can be excited without reflection or substantially negligible reflection.

However, Equation (46) means that the physical height of the guided surface waveguide probe 400a (FIG. 4) can be relatively small. While this will excite the guided surface waveguide mode, the proximity of the elevated charge Q_1 to its mirror image Q_1' (see FIG. 4) can result in an unduly large bound charge with little free charge. To compensate, the charge terminal T_1 can be raised to an appropriate elevation to increase the amount of free charge. As one example rule of thumb, the charge terminal T_1 can be positioned at an elevation of about 4-5 times (or more) the effective diameter of the charge terminal T_1 . The challenge is that as the charge terminal height increases, the rays intersecting the lossy conductive medium at the Brewster angle do so at greater distances as shown in FIG. 7, where the electric field is weaker by a factor of $\sqrt{R_x/R_{xm}}$.

FIG. 8B illustrates the effect of raising the charge terminal T_1 above the height of FIG. 8A. The increased elevation causes the distance at which the wave tilt is incident with the lossy conductive medium to move beyond the Hankel cross-

over point **509**. To improve coupling in the guide surface waveguide mode, and thus provide for a greater launching efficiency of the guided surface wave, a lower compensation terminal T_2 can be used to adjust the total effective height (h_{TE}) of the charge terminal T_1 such that the wave tilt at the Hankel crossover distance is at the Brewster angle. For example, if the charge terminal T_1 has been elevated to a height where the electric field intersects with the lossy conductive medium at the Brewster angle at a distance greater than the Hankel crossover point **509**, as illustrated by line **803**, then the compensation terminal T_2 can be used to adjust h_{TE} by compensating for the increased height. The effect of the compensation terminal T_2 is to reduce the electrical effective height of the guided surface waveguide probe (or effectively raise the lossy medium interface) such that the wave tilt at the Hankel crossover distance is at the Brewster angle, as illustrated by line **806**.

The total effective height can be written as the superposition of an upper effective height (h_{UE}) associated with the charge terminal T_1 and a lower effective height (h_{LE}) associated with the compensation terminal T_2 such that

$$h_{TE} = h_{UE} + h_{LE} = h_p e^{j(\beta h_p + \Phi_U)} + h_d e^{j(\beta h_d + \Phi_L)} = R_x \times W, \quad (48)$$

where Φ_U is the phase delay applied to the upper charge terminal T_1 , Φ_L is the phase delay applied to the lower compensation terminal T_2 , and $\beta = 2\pi/\lambda_p$ is the propagation factor from Equation (30). If extra lead lengths are taken into consideration, they can be accounted for by adding the charge terminal lead length z to the physical height h_p of the charge terminal T_1 and the compensation terminal lead length y to the physical height h_d of the compensation terminal T_2 as shown in

$$h_{TE} = (h_p + z) e^{j(\beta(h_p + z) + \Phi_U)} + (h_d + y) e^{j(\beta(h_d + y) + \Phi_L)} = R_x \times W. \quad (49)$$

The lower effective height can be used to adjust the total effective height (h_{TE}) to equal the complex effective height (h_{eff}) of FIG. **8A**.

Equations (48) or (49) can be used to determine the physical height of the lower disk of the compensation terminal T_2 and the phase angles to feed the terminals in order to obtain the desired wave tilt at the Hankel crossover distance. For example, Equation (49) can be rewritten as the phase shift applied to the charge terminal T_1 as a function of the compensation terminal height (h_d) to give

$$\Phi_U(h_d) = -\beta(h_p + z) - j \ln \left(\frac{R_x \times W - (h_d + y) e^{j(\beta h_d + \Phi_L)}}{(h_p + z)} \right). \quad (50)$$

To determine the positioning of the compensation terminal T_2 , the relationships discussed above can be utilized. First, the total effective height (h_{TE}) is the superposition of the complex effective height (h_{UE}) of the upper charge terminal T_1 and the complex effective height (h_{LE}) of the lower compensation terminal T_2 as expressed in Equation (49). Next, the tangent of the angle of incidence can be expressed geometrically as

$$\tan \psi_E = \frac{h_{TE}}{R_x}, \quad (51)$$

which is the definition of the wave tilt, W . Finally, given the desired Hankel crossover distance R_x , the h_{TE} can be adjusted to make the wave tilt of the incident electric field

match the complex Brewster angle at the Hankel crossover point **509**. This can be accomplished by adjusting h_p , Φ_U , and/or h_d .

These concepts may be better understood when discussed in the context of an example of a guided surface waveguide probe. Referring to FIGS. **9A** and **9B**, shown are graphical representations of examples of guided surface waveguide probes **400b** and **400c** that include a charge terminal T_1 . An AC source **912** acts as the excitation source (**412** of FIG. **4**) for the charge terminal T_1 , which is coupled to the guided surface waveguide probe **400b** through a coupling circuit (**409** of FIG. **4**) comprising a coil **909** such as, e.g., a helical coil. As shown in FIG. **9A**, the guided surface waveguide probe **400b** can include the upper charge terminal T_1 (e.g., a sphere at height h_T) and a lower compensation terminal T_2 (e.g., a disk at height h_d) that are positioned along a vertical axis z that is substantially normal to the plane presented by the lossy conducting medium **403**. A second medium **406** is located above the lossy conducting medium **403**. The charge terminal T_1 has a self-capacitance C_p , and the compensation terminal T_2 has a self-capacitance C_d . During operation, charges Q_1 and Q_2 are imposed on the terminals T_1 and T_2 , respectively, depending on the voltages applied to the terminals T_1 and T_2 at any given instant.

In the example of FIG. **9A**, the coil **909** is coupled to a ground stake **915** at a first end and the compensation terminal T_2 at a second end. In some implementations, the connection to the compensation terminal T_2 can be adjusted using a tap **921** at the second end of the coil **909** as shown in FIG. **9A**. The coil **909** can be energized at an operating frequency by the AC source **912** through a tap **924** at a lower portion of the coil **909**. In other implementations, the AC source **912** can be inductively coupled to the coil **909** through a primary coil. The charge terminal T_1 is energized through a tap **918** coupled to the coil **909**. An ammeter **927** located between the coil **909** and ground stake **915** can be used to provide an indication of the magnitude of the current flow at the base of the guided surface waveguide probe. Alternatively, a current clamp may be used around the conductor coupled to the ground stake **915** to obtain an indication of the magnitude of the current flow. The compensation terminal T_2 is positioned above and substantially parallel with the lossy conducting medium **403** (e.g., the ground).

The construction and adjustment of the guided surface waveguide probe **400** is based upon various operating conditions, such as the transmission frequency, conditions of the lossy conductive medium (e.g., soil conductivity σ and relative permittivity ϵ_r), and size of the charge terminal T_1 . The index of refraction can be calculated from Equations (10) and (11) as

$$n = \sqrt{\epsilon_r - j\sigma/\omega}, \quad (52)$$

where $x = \sigma/\omega\epsilon_0$ with $\omega = 2\pi f$, and complex Brewster angle ($\theta_{i,B}$) measured from the surface normal can be determined from Equation (42) as

$$\theta_{i,B} = \arctan(\sqrt{\epsilon_r - j\sigma/\omega}), \quad (53)$$

or measured from the surface as shown in FIG. **8A** as

$$\psi_{i,B} = \frac{\pi}{2} - \theta_{i,B}. \quad (54)$$

The wave tilt at the Hankel crossover distance can also be found using Equation (47).

The Hankel crossover distance can also be found by equating Equations (20b) and (21), and solving for R_x . The electrical effective height can then be determined from Equation (46) using the Hankel crossover distance and the complex Brewster angle as

$$h_{eff} = R_x \tan \Psi_{i,B} = h_p e^{i\Phi}. \quad (55)$$

As can be seen from Equation (55), the complex effective height (h_{eff}) includes a magnitude that is associated with the physical height (h_p) of charge terminal T_1 and a phase (Φ) that is to be associated with the angle of the wave tilt at the Hankel crossover distance (Ψ). With these variables and the selected charge terminal T_1 configuration, it is possible to determine the configuration of a guided surface waveguide probe 400.

With the selected charge terminal T_1 configuration, a spherical diameter (or the effective spherical diameter) can be determined. For example, if the charge terminal T_1 is not configured as a sphere, then the terminal configuration may be modeled as a spherical capacitance having an effective spherical diameter. The size of the charge terminal T_1 can be chosen to provide a sufficiently large surface for the charge Q_1 imposed on the terminals. In general, it is desirable to make the charge terminal T_1 as large as practical. The size of the charge terminal T_1 should be large enough to avoid ionization of the surrounding air, which can result in electrical discharge or sparking around the charge terminal. As previously discussed with respect to FIGS. 6A and 6B, to reduce the amount of bound charge on the charge terminal T_1 , the desired elevation of the charge terminal T_1 should be 4-5 times the effective spherical diameter (or more). If the elevation of the charge terminal T_1 is less than the physical height (h_p) indicated by the complex effective height (h_{eff}) determined using Equation (55), then the charge terminal T_1 should be positioned at a physical height of $h_T = h_p$ above the lossy conductive medium (e.g., the earth). If the charge terminal T_1 is located at h_p , then a guided surface wave tilt can be produced at the Hankel crossover distance (R_x) without the use of a compensation terminal T_2 . FIG. 9B illustrates an example of the guided surface waveguide probe 400c without a compensation terminal T_2 .

Referring back to FIG. 9A, a compensation terminal T_2 can be included when the elevation of the charge terminal T_1 is greater than the physical height (h_p) indicated by the determined complex effective height (h_{eff}). As discussed with respect to FIG. 8B, the compensation terminal T_2 can be used to adjust the total effective height (h_{TE}) of the guided surface waveguide probe 400 to excite an electric field having a guided surface wave tilt at R_x . The compensation terminal T_2 can be positioned below the charge terminal T_1 at a physical height of $h_d = h_T - h_p$, where h_T is the total physical height of the charge terminal T_1 . With the position of the compensation terminal T_2 fixed and the phase delay Φ_L applied to the lower compensation terminal T_2 , the phase delay Φ_U applied to the upper charge terminal T_1 can be determined using Equation (50).

When installing a guided surface waveguide probe 400, the phase delays Φ_U and Φ_L of Equations (48)-(50) may be adjusted as follows. Initially, the complex effective height (h_{eff}) and the Hankel crossover distance (R_x) are determined for the operational frequency (f_0). To minimize bound capacitance and corresponding bound charge, the upper charge terminal T_1 is positioned at a total physical height (h_T) that is at least four times the spherical diameter (or equivalent spherical diameter) of the charge terminal T_1 . Note that, at the same time, the upper charge terminal T_1 should also be positioned at a height that is at least the

magnitude (h_p) of the complex effective height (h_{eff}). If $h_T > h_p$, then the lower compensation terminal T_2 can be positioned at a physical height of $h_d = h_T - h_p$ as shown in FIG. 9A. The compensation terminal T_2 can then be coupled to the coil 909, where the upper charge terminal T_1 is not yet coupled to the coil 909. The AC source 912 is coupled to the coil 909 in such a manner so as to minimize reflection and maximize coupling into the coil 909. To this end, the AC source 912 may be coupled to the coil 909 at an appropriate point such as at the 50Ω point to maximize coupling. In some embodiments, the AC source 912 may be coupled to the coil 909 via an impedance matching network. For example, a simple L-network comprising capacitors (e.g., tapped or variable) and/or a capacitor/inductor combination (e.g., tapped or variable) can be matched to the operational frequency so that the AC source 912 sees a 50Ω load when coupled to the coil 909. The compensation terminal T_2 can then be adjusted for parallel resonance with at least a portion of the coil at the frequency of operation. For example, the tap 921 at the second end of the coil 909 may be repositioned. While adjusting the compensation terminal circuit for resonance aids the subsequent adjustment of the charge terminal connection, it is not necessary to establish the guided surface wave tilt (W_{Rx}) at the Hankel crossover distance (R_x). The upper charge terminal T_1 may then be coupled to the coil 909.

In this context, FIG. 10 shows a schematic diagram of the general electrical hookup of FIG. 9A in which V_1 is the voltage applied to the lower portion of the coil 909 from the AC source 912 through tap 924, V_2 is the voltage at tap 918 that is supplied to the upper charge terminal T_1 , and V_3 is the voltage applied to the lower compensation terminal T_2 through tap 921. The resistances R_p and R_d represent the ground return resistances of the charge terminal T_1 and compensation terminal T_2 , respectively. The charge and compensation terminals T_1 and T_2 may be configured as spheres, cylinders, toroids, rings, hoods, or any other combination of capacitive structures. The size of the charge and compensation terminals T_1 and T_2 can be chosen to provide a sufficiently large surface for the charges Q_1 and Q_2 imposed on the terminals. In general, it is desirable to make the charge terminal T_1 as large as practical. The size of the charge terminal T_1 should be large enough to avoid ionization of the surrounding air, which can result in electrical discharge or sparking around the charge terminal. The self-capacitance C_p and C_d can be determined for the sphere and disk as disclosed, for example, with respect to Equation (38).

As can be seen in FIG. 10, a resonant circuit is formed by at least a portion of the inductance of the coil 909, the self-capacitance C_d of the compensation terminal T_2 , and the ground return resistance R_d associated with the compensation terminal T_2 . The parallel resonance can be established by adjusting the voltage V_3 applied to the compensation terminal T_2 (e.g., by adjusting a tap 921 position on the coil 909) or by adjusting the height and/or size of the compensation terminal T_2 to adjust C_d . The position of the coil tap 921 can be adjusted for parallel resonance, which will result in the ground current through the ground stake 915 and through the ammeter 927 reaching a maximum point. After parallel resonance of the compensation terminal T_2 has been established, the position of the tap 924 for the AC source 912 can be adjusted to the 50Ω point on the coil 909.

Voltage V_2 from the coil 909 may then be applied to the charge terminal T_1 through the tap 918. The position of tap 918 can be adjusted such that the phase (Φ) of the total effective height (h_{TE}) approximately equals the angle of the

guided surface wave tilt (Ψ) at the Hankel crossover distance (R_x). The position of the coil tap **918** is adjusted until this operating point is reached, which results in the ground current through the ammeter **927** increasing to a maximum. At this point, the resultant fields excited by the guided surface waveguide probe **400b** (FIG. 9A) are substantially mode-matched to a guided surface waveguide mode on the surface of the lossy conducting medium **403**, resulting in the launching of a guided surface wave along the surface of the lossy conducting medium **403** (FIGS. 4, 9A, 9B). This can be verified by measuring field strength along a radial extending from the guided surface waveguide probe **400** (FIGS. 4, 9A, 9B). Resonance of the circuit including the compensation terminal T_2 may change with the attachment of the charge terminal T_1 and/or with adjustment of the voltage applied to the charge terminal T_1 through tap **921**. While adjusting the compensation terminal circuit for resonance aids the subsequent adjustment of the charge terminal connection, it is not necessary to establish the guided surface wave tilt (W_{Rx}) at the Hankel crossover distance (R_x). The system may be further adjusted to improve coupling by iteratively adjusting the position of the tap **924** for the AC source **912** to be at the 50Ω point on the coil **909** and adjusting the position of tap **918** to maximize the ground current through the ammeter **927**. Resonance of the circuit including the compensation terminal T_2 may drift as the positions of taps **918** and **924** are adjusted, or when other components are attached to the coil **909**.

If $h_T \leq h_p$, then a compensation terminal T_2 is not needed to adjust the total effective height (h_{TE}) of the guided surface waveguide probe **400c** as shown in FIG. 9B. With the charge terminal positioned at h_p , the voltage V_2 can be applied to the charge terminal T_1 from the coil **909** through the tap **918**. The position of tap **918** that results in the phase (Φ) of the total effective height (h_{TE}) approximately equal to the angle of the guided surface wave tilt (Ψ) at the Hankel crossover distance (R_x) can then be determined. The position of the coil tap **918** is adjusted until this operating point is reached, which results in the ground current through the ammeter **927** increasing to a maximum. At that point, the resultant fields are substantially mode-matched to the guided surface waveguide mode on the surface of the lossy conducting medium **403**, thereby launching the guided surface wave along the surface of the lossy conducting medium **403**. This can be verified by measuring field strength along a radial extending from the guided surface waveguide probe **400**. The system may be further adjusted to improve coupling by iteratively adjusting the position of the tap **924** for the AC source **912** to be at the 50Ω point on the coil **909** and adjusting the position of tap **918** to maximize the ground current through the ammeter **927**.

In one experimental example, a guided surface waveguide probe **400b** was constructed to verify the operation of the proposed structure at 1.879 MHz. The soil conductivity at the site of the guided surface waveguide probe **400b** was determined to be $\sigma=0.0053$ mhos/m and the relative permittivity was $\epsilon_r=28$. Using these values, the index of refraction given by Equation (52) was determined to be $n=6.555-j3.869$. Based upon Equations (53) and (54), the complex Brewster angle was found to be $\theta_{i,B}=83.517-j3.783$ degrees, or $\psi_{i,B}=6.483+j3.783$ degrees.

Using Equation (47), the guided surface wave tilt was calculated as $W_{Rx}=0.113+j0.067=0.131 e^{j(30.551^\circ)}$. A Hankel crossover distance of $R_x=54$ feet was found by equating Equations (20b) and (21), and solving for R_x . Using Equation (55), the complex effective height ($h_{eff}=h_p e^{j\Phi}$) was determined to be $h_p=7.094$ feet (relative to the lossy con-

ducting medium) and $\Phi=30.551$ degrees (relative to the ground current). Note that the phase Φ is equal to the argument of the guided surface wave tilt Ψ . However, the physical height of $h_p=7.094$ feet is relatively small. While this will excite a guided surface waveguide mode, the proximity of the elevated charge terminal T_1 to the earth (and its mirror image) will result in a large amount of bound charge and very little free charge. Since the guided surface wave field strength is proportional to the free charge on the charge terminal, an increased elevation was desirable.

To increase the amount of free charge, the physical height of the charge terminal T_1 was set to be $h_p=17$ feet, with the compensation terminal T_2 positioned below the charge terminal T_1 . The extra lead lengths for connections were approximately $y=2.7$ feet and $z=1$ foot. Using these values, the height of the compensation terminal T_2 (h_d) was determined using Equation (50). This is graphically illustrated in FIG. 11, which shows plots **130** and **160** of the imaginary and real parts of Φ_U , respectively. The compensation terminal T_2 is positioned at a height h_d where $\text{Im}\{\Phi_U\}=0$, as graphically illustrated in plot **130**. In this case, setting the imaginary part to zero gives a height of $h_d=8.25$ feet. At this fixed height, the coil phase Φ_U can be determined from $\text{Re}\{\Phi_U\}$ as $+22.84$ degrees, as graphically illustrated in plot **160**.

As previously discussed, the total effective height is the superposition of the upper effective height (h_{UE}) associated with the charge terminal T_1 and the lower effective height (h_{LE}) associated with the compensation terminal T_2 as expressed in Equation (49). With the coil tap adjusted to 22.84 degrees, the complex upper effective height is given as

$$h_{UE}=(h_p+z)e^{j(\beta(h_p+z)+\Phi_U)}=14.711+j10.832 \quad (56)$$

(or 18.006 at 35.21°) and the complex lower effective height is given as

$$h_{LE}=(h_d+y)e^{j(\beta(h_d+y)+\Phi_L)}=-8.602-j6.776 \quad (57)$$

(or 10.950 at -141.773°). The total effective height (h_{TE}) is the superposition of these two values, which gives

$$h_{TE}=h_{UE}+h_{LE}=6.109-j3.606=7.094e^{j(30.551^\circ)}. \quad (58)$$

As can be seen, the coil phase matches the calculated angle of the guided surface wave tilt, W_{Rx} . The guided surface waveguide probe can then be adjusted to maximize the ground current. As previously discussed with respect to FIG. 9A, the guided surface waveguide mode coupling can be improved by iteratively adjusting the position of the tap **924** for the AC source **912** to be at the 50Ω point on the coil **909** and adjusting the position of tap **918** to maximize the ground current through the ammeter **927**.

Field strength measurements were carried out to verify the ability of the guided surface waveguide probe **400b** (FIG. 9A) to couple into a guided surface wave or a transmission line mode. Referring to FIG. 12, shown is an image of the guided surface waveguide probe used for the field strength measurements. FIG. 12 shows the guided surface waveguide probe **400b** including an upper charge terminal T_1 and a lower compensation terminal T_2 , which were both fabricated as rings. An insulating structure supports the charge terminal T_1 above the compensation terminal T_2 . For example, an RF insulating fiberglass mast can be used to support the charge and compensation terminals T_1 and T_2 . The insulating support structure can be configured to adjust the position of the charge and compensation terminals T_1 and T_2 using, e.g., insulated guy wires and pulleys, screw gears, or other appropriate mechanism as can be understood. A coil was used in the coupling circuit with one end of the coil

grounded to an 8 foot ground rod near the base of the RF insulating fiberglass mast. The AC source was coupled to the right side of the coil by a tap connection (V_1), and taps for the charge terminal T_1 and compensation terminal T_2 were located at the center (V_2) and the left of the coil (V_3). FIG. 9A graphically illustrates the tap locations on the coil 909.

The guided surface waveguide probe 400b was supplied with power at a frequency of 1879 kHz. The voltage on the upper charge terminal T_1 was $15.6V_{peak-peak}$ ($5.515V_{RMS}$) with a capacitance of 64 pF. Field strength (FS) measurements were taken at predetermined distances along a radial extending from the guided surface waveguide probe 400b using a FIM-41 FS meter (Potomac Instruments, Inc., Silver Spring, Md.). The measured data and predicted values for a guided surface wave transmission mode with an electrical launching efficiency of 35% are indicated in TABLE 1 below. Beyond the Hankel crossover distance (R_x), the large argument asymptote predominates over the “close-in” representation of the Hankel function, and the vertical component of the mode-matched electric asymptotically passes to Equation (44), which is linearly proportional to free charge on the charge terminal. TABLE 1 shows the measured values and predicted data. When plotted using an accurate plotting application (Mathcad), the measured values were found to fit an electrical launching efficiency curve corresponding to 38%, as illustrated in FIG. 13. For $15.6V_{pp}$ on the charge terminal T_1 , the field strength curve (Zenneck @ 38%) passes through $363 \mu V/m$ at 1 mile (and $553 \mu V/m$ at 1 km) and scales linearly with the capacitance (C_p) and applied terminal voltage.

TABLE 1

Range (miles)	Measured FS w/FIM-41 ($\mu V/m$)	Predicted FS ($\mu V/m$)
0.64	550	546
1.25	265	263
3.15	67	74
4.48	30	35
6.19	14	13

The lower electrical launching efficiency may be attributed to the height of the upper charge terminal T_1 . Even with the charge terminal T_1 elevated to a physical height of 17 feet, the bound charge reduces the efficiency of the guided surface waveguide probe 400b. While increasing the height of the charge terminal T_1 would improve the launching efficiency of the guided surface waveguide probe 400b, even at such a low height ($h_d/\lambda=0.032$) the coupled wave was found to match a 38% electric launching efficiency curve. In addition, it can be seen in FIG. 13 that the modest 17 foot guided surface waveguide probe 400b of FIG. 9A (with no ground system other than an 8 foot ground rod) exhibits better field strength than a full quarter-wave tower ($\lambda/4$ Norton=131 feet tall) with an extensive ground system by more than 10 dB in the range of 1-6 miles at 1879 kHz. Increasing the elevation of the charge terminal T_1 , and adjusting the height of the compensation terminal T_2 and the coil phase Φ_{ν} , can improve the guided surface waveguide mode coupling, and thus the resulting electric field strength.

In another experimental example, a guided surface waveguide probe 400 was constructed to verify the operation of the proposed structure at 52 MHz (corresponding to $\omega=2\pi f=3.267\times 10^8$ radians/sec). FIG. 14A shows an image of the guided surface waveguide probe 400. FIG. 14B is a schematic diagram of the guided surface waveguide probe 400 of FIG. 14A. The complex effective height between the

charge and compensation terminals T_1 and T_2 of the doublet probe was adjusted to match R_x times the guided surface wave tilt, W_{R_x} , at the Hankel crossover distance to launch a guided surface wave. This can be accomplished by changing the physical spacing between terminals, the magnetic link coupling and its position between the AC source 912 and the coil 909, the relative phase of the voltage between the terminals T_1 and T_2 , the height of the charge and compensation terminal T_1 and T_2 relative to ground or the lossy conducting medium, or a combination thereof. The conductivity of the lossy conducting medium at the site of the guided surface waveguide probe 400 was determined to be $\sigma=0.067$ mhos/m and the relative permittivity was $\epsilon_r=82.5$. Using these values, the index of refraction was determined to be $n=9.170-j1.263$. The complex Brewster angle was found to be $\psi_{i,B}=6.110+j0.8835$ degrees.

A Hankel crossover distance of $R_x=2$ feet was found by equating Equations (20b) and (21), and solving for R_x . FIG. 15 shows a graphical representation of the crossover distance R_x at 52 Hz. Curve 533 is a plot of the “far-out” asymptote. Curve 536 is a plot of the “close-in” asymptote. The magnitudes of the two sets of mathematical asymptotes in this example are equal at a Hankel crossover point 539 of two feet. The graph was calculated for water with a conductivity of 0.067 mhos/m and a relative dielectric constant (permittivity) of $\epsilon_r=82.5$, at an operating frequency of 52 MHz. At lower frequencies, the Hankel crossover point 539 moves farther out. The guided surface wave tilt was calculated as $W_{R_x}=0.108 e^{j(7.851^\circ)}$. For the doublet configuration with a total height of 6 feet, the complex effective height ($h_{eff}=2h_p e^{j\Phi}=R_x \tan \psi_{i,B}$) was determined to be $2h_p=6$ inches with $\Phi=-172$ degrees. When adjusting the phase delay of the compensation terminal T_2 to the actual conditions, it was found that $\Phi=-174$ degrees maximized the mode matching of the guided surface wave, which was within experimental error.

Field strength measurements were carried out to verify the ability of the guided surface waveguide probe 400 of FIGS. 14A and 14B to couple into a guided surface wave or a transmission line mode. With 10V peak-to-peak applied to the 3.5 pF terminals T_1 and T_2 , the electric fields excited by the guided surface waveguide probe 400 were measured and plotted in FIG. 16. As can be seen, the measured field strengths fell between the Zenneck curves for 90% and 100%. The measured values for a Norton half wave dipole antenna were significantly less.

Referring next to FIG. 17, shown is a graphical representation of another example of a guided surface waveguide probe 400d including an upper charge terminal T_1 (e.g., a sphere at height h_T) and a lower compensation terminal T_2 (e.g., a disk at height h_d) that are positioned along a vertical axis z that is substantially normal to the plane presented by the lossy conducting medium 403. During operation, charges Q_1 and Q_2 are imposed on the charge and compensation terminals T_1 and T_2 , respectively, depending on the voltages applied to the terminals T_1 and T_2 at any given instant.

As in FIGS. 9A and 9B, an AC source 912 acts as the excitation source (412 of FIG. 4) for the charge terminal T_1 . The AC source 912 is coupled to the guided surface waveguide probe 400d through a coupling circuit (409 of FIG. 4) comprising a coil 909. The AC source 912 can be connected across a lower portion of the coil 909 through a tap 924, as shown in FIG. 17, or can be inductively coupled to the coil 909 by way of a primary coil. The coil 909 can be coupled to a ground stake 915 at a first end and the charge terminal T_1 at a second end. In some implementations, the connection

to the charge terminal T_1 can be adjusted using a tap **930** at the second end of the coil **909**. The compensation terminal T_2 is positioned above and substantially parallel with the lossy conducting medium **403** (e.g., the ground or earth), and energized through a tap **933** coupled to the coil **909**. An ammeter **927** located between the coil **909** and ground stake **915** can be used to provide an indication of the magnitude of the current flow (I_0) at the base of the guided surface waveguide probe. Alternatively, a current clamp may be used around the conductor coupled to the ground stake **915** to obtain an indication of the magnitude of the current flow (I_0).

In the embodiment of FIG. 17, the connection to the charge terminal T_1 (tap **930**) has been moved up above the connection point of tap **933** for the compensation terminal T_2 as compared to the configuration of FIG. 9A. Such an adjustment allows an increased voltage (and thus a higher charge Q_1) to be applied to the upper charge terminal T_1 . As with the guided surface waveguide probe **400b** of FIG. 9A, it is possible to adjust the total effective height (h_{TE}) of the guided surface waveguide probe **400d** to excite an electric field having a guided surface wave tilt at the Hankel crossover distance R_x . The Hankel crossover distance can also be found by equating Equations (20b) and (21), and solving for R_x . The index of refraction (n), the complex Brewster angle ($\theta_{i,B}$ and $\psi_{i,B}$), the wave tilt ($|W|e^{j\psi}$) and the complex effective height ($h_{eff}=h_p e^{j\Phi}$) can be determined as described with respect to Equations (52)-(55) above.

With the selected charge terminal T_1 configuration, a spherical diameter (or the effective spherical diameter) can be determined. For example, if the charge terminal T_1 is not configured as a sphere, then the terminal configuration may be modeled as a spherical capacitance having an effective spherical diameter. The size of the charge terminal T_1 can be chosen to provide a sufficiently large surface for the charge Q_1 imposed on the terminals. In general, it is desirable to make the charge terminal T_1 as large as practical. The size of the charge terminal T_1 should be large enough to avoid ionization of the surrounding air, which can result in electrical discharge or sparking around the charge terminal. To reduce the amount of bound charge on the charge terminal T_1 , the desired elevation to provide free charge on the charge terminal T_1 for launching a guided surface wave should be at least 4-5 times the effective spherical diameter above the lossy conductive medium (e.g., the earth). The compensation terminal T_2 can be used to adjust the total effective height (h_{TE}) of the guided surface waveguide probe **400d** to excite an electric field having a guided surface wave tilt at R_x . The compensation terminal T_2 can be positioned below the charge terminal T_1 at $h_d=h_T-h_p$, where h_T is the total physical height of the charge terminal T_1 . With the position of the compensation terminal T_2 fixed and the phase delay Φ_U applied to the upper charge terminal T_1 , the phase delay Φ_L applied to the lower compensation terminal T_2 can be determined using the relationships of Equation (49).

$$\Phi_U(h_d) = -\beta(h_d + y) - j \ln \left(\frac{R_x \times W - (h_p + z)e^{j(\beta h_p + \beta z + \Phi_L)}}{(h_d + y)} \right) \quad (59)$$

In alternative embodiments, the compensation terminal T_2 can be positioned at a height h_d where $\text{Im}\{\Phi_L\}=0$.

With the AC source **912** coupled to the coil **909** (e.g., at the 50Ω point to maximize coupling), the position of tap **933** may be adjusted for parallel resonance of the compensation terminal T_2 with at least a portion of the coil at the frequency

of operation. Voltage V_2 from the coil **909** can be applied to the charge terminal T_1 , and the position of tap **930** can be adjusted such that the phase (Ψ) of the total effective height (h_{TE}) approximately equals the angle of the guided surface wave tilt (W_{Rx}) at the Hankel crossover distance (R_x). The position of the coil tap **930** can be adjusted until this operating point is reached, which results in the ground current through the ammeter **927** increasing to a maximum. At this point, the resultant fields excited by the guided surface waveguide probe **400d** are substantially mode-matched to a guided surface waveguide mode on the surface of the lossy conducting medium **403**, resulting in the launching of a guided surface wave along the surface of the lossy conducting medium **403**. This can be verified by measuring field strength along a radial extending from the guided surface waveguide probe **400**.

In other implementations, the voltage V_2 from the coil **909** can be applied to the charge terminal T_1 , and the position of tap **933** can be adjusted such that the phase (Φ) of the total effective height (h_{TE}) approximately equals the angle of the guided surface wave tilt (Ψ) at R_x . The position of the coil tap **930** can be adjusted until the operating point is reached, resulting in the ground current through the ammeter **927** substantially reaching a maximum. The resultant fields are substantially mode-matched to a guided surface waveguide mode on the surface of the lossy conducting medium **403**, and a guided surface wave is launched along the surface of the lossy conducting medium **403**. This can be verified by measuring field strength along a radial extending from the guided surface waveguide probe **400**. The system may be further adjusted to improve coupling by iteratively adjusting the position of the tap **924** for the AC source **912** to be at the 50Ω point on the coil **909** and adjusting the position of tap **930** and/or **933** to maximize the ground current through the ammeter **927**.

FIG. 18 is a graphical representation illustrating another example of a guided surface waveguide probe **400e** including an upper charge terminal T_1 (e.g., a sphere at height h_T) and a lower compensation terminal T_2 (e.g., a disk at height h_d) that are positioned along a vertical axis z that is substantially normal to the plane presented by the lossy conducting medium **403**. In the example of FIG. 18, the charge terminal T_1 (e.g., a sphere at height h_T) and compensation terminal T_2 (e.g., a disk at height h_d) are coupled to opposite ends of the coil **909**. For example, charge terminal T_1 can be connected via tap **936** at a first end of coil **909** and compensation terminal T_2 can be connected via tap **939** at a second end of coil **909** as shown in FIG. 18. The compensation terminal T_2 is positioned above and substantially parallel with the lossy conducting medium **403** (e.g., the ground or earth). During operation, charges Q_1 and Q_2 are imposed on the charge and compensation terminals T_1 and T_2 , respectively, depending on the voltages applied to the terminals T_1 and T_2 at any given instant.

An AC source **912** acts as the excitation source (**412** of FIG. 4) for the charge terminal T_1 . The AC source **912** is coupled to the guided surface waveguide probe **400e** through a coupling circuit (**409** of FIG. 4) comprising a coil **909**. In the example of FIG. 18, the AC source **912** is connected across a middle portion of the coil **909** through tapped connections **942** and **943**. In other embodiments, the AC source **912** can be inductively coupled to the coil **909** through a primary coil. One side of the AC source **912** is also coupled to a ground stake **915**, which provides a ground point on the coil **909**. An ammeter **927** located between the coil **909** and ground stake **915** can be used to provide an indication of the magnitude of the current flow at the base of

the guided surface waveguide probe **400e**. Alternatively, a current clamp may be used around the conductor coupled to the ground stake **915** to obtain an indication of the magnitude of the current flow.

It is possible to adjust the total effective height (h_{TE}) of the guided surface waveguide probe **400e** to excite an electric field having a guided surface wave tilt at the Hankel crossover distance R_x , as has been previously discussed. The Hankel crossover distance can also be found by equating Equations (20b) and (21), and solving for R_x . The index of refraction (n), the complex Brewster angle ($\theta_{i,B}$ and $\psi_{i,B}$) and the complex effective height ($h_{eff}=h_p e^{j\Phi}$) can be determined as described with respect to Equations (52)-(55) above.

A spherical diameter (or the effective spherical diameter) can be determined for the selected charge terminal T_1 configuration. For example, if the charge terminal T_1 is not configured as a sphere, then the terminal configuration may be modeled as a spherical capacitance having an effective spherical diameter. To reduce the amount of bound charge on the charge terminal T_1 , the desired elevation to provide free charge on the charge terminal T_1 for launching a guided surface wave should be at least 4-5 times the effective spherical diameter above the lossy conductive medium (e.g., the earth). The compensation terminal T_2 can be positioned below the charge terminal T_1 at $h_d=h_T-h_p$, where h_T is the total physical height of the charge terminal T_1 . With the positions of the charge terminal T_1 and the compensation terminal T_2 fixed and the AC source **912** coupled to the coil **909** (e.g., at the 50 Ω point to maximize coupling), the position of tap **939** may be adjusted for parallel resonance of the compensation terminal T_2 with at least a portion of the coil at the frequency of operation. While adjusting the compensation terminal circuit for resonance aids the subsequent adjustment of the charge terminal connection, it is not necessary to establish the guided surface wave tilt (W_{Rx}) at the Hankel crossover distance (R_x). One or both of the phase delays Φ_L and Φ_U applied to the upper charge terminal T_1 and lower compensation terminal T_2 can be adjusted by repositioning one or both of the taps **936** and/or **939** on the coil **909**. In addition, the phase delays Φ_L and Φ_U may be adjusted by repositioning one or both of the taps **942** of the AC source **912**. The position of the coil tap(s) **936**, **939** and/or **942** can be adjusted until this operating point is reached, which results in the ground current through the ammeter **927** increasing to a maximum. This can be verified by measuring field strength along a radial extending from the guided surface waveguide probe **400**. The phase delays may then be adjusted by repositioning these tap(s) to increase (or maximize) the ground current.

When the electric fields produced by a guided surface waveguide probe **400** has a guided surface wave tilt at the Hankel crossover distance R_x , they are substantially mode-matched to a guided surface waveguide mode on the surface of the lossy conducting medium, and a guided electromagnetic field in the form of a guided surface wave is launched along the surface of the lossy conducting medium. As illustrated in FIG. 1, the guided field strength curve **103** of the guided electromagnetic field has a characteristic exponential decay of $e^{-\alpha d/\sqrt{d}}$ and exhibits a distinctive knee **109** on the log-log scale. Receive circuits can be utilized with one or more guided surface waveguide probe to facilitate wireless transmission and/or power delivery systems.

Referring next to FIGS. **19A**, **19B**, and **20**, shown are examples of generalized receive circuits for using the surface-guided waves in wireless power delivery systems. FIGS. **19A** and **19B** include a linear probe **703** and a tuned

resonator **706**, respectively. FIG. **20** is a magnetic coil **709** according to various embodiments of the present disclosure. According to various embodiments, each one of the linear probe **703**, the tuned resonator **706**, and the magnetic coil **709** may be employed to receive power transmitted in the form of a guided surface wave on the surface of a lossy conducting medium **403** (FIG. **4**) according to various embodiments. As mentioned above, in one embodiment the lossy conducting medium **403** comprises a terrestrial medium (or earth).

With specific reference to FIG. **19A**, the open-circuit terminal voltage at the output terminals **713** of the linear probe **703** depends upon the effective height of the linear probe **703**. To this end, the terminal point voltage may be calculated as

$$V_T = \int_0^{h_e} E_{inc} dl, \quad (60)$$

where E_{inc} is the strength of the electric field on the linear probe **703** in Volts per meter, dl is an element of integration along the direction of the linear probe **703**, and h_e is the effective height of the linear probe **703**. An electrical load **716** is coupled to the output terminals **713** through an impedance matching network **719**.

When the linear probe **703** is subjected to a guided surface wave as described above, a voltage is developed across the output terminals **713** that may be applied to the electrical load **716** through a conjugate impedance matching network **719** as the case may be. In order to facilitate the flow of power to the electrical load **716**, the electrical load **716** should be substantially impedance matched to the linear probe **703** as will be described below.

Referring to FIG. **19B**, the tuned resonator **706** includes a charge terminal T_R that is elevated above the lossy conducting medium **403**. The charge terminal T_R has a self-capacitance C_R . In addition, there may also be a bound capacitance (not shown) between the charge terminal T_R and the lossy conducting medium **403** depending on the height of the charge terminal T_R above the lossy conducting medium **403**. The bound capacitance should preferably be minimized as much as is practicable, although this may not be entirely necessary in every instance of a guided surface waveguide probe **400**.

The tuned resonator **706** also includes a coil L_R . One end of the coil L_R is coupled to the charge terminal T_R , and the other end of the coil L_R is coupled to the lossy conducting medium **403**. To this end, the tuned resonator **706** (which may also be referred to as tuned resonator L_R - C_R) comprises a series-tuned resonator as the charge terminal C_R and the coil L_R are situated in series. The tuned resonator **706** is tuned by adjusting the size and/or height of the charge terminal T_R , and/or adjusting the size of the coil L_R so that the reactive impedance of the structure is substantially eliminated.

For example, the reactance presented by the self-capacitance C_R is calculated as $1/j\omega C_R$. Note that the total capacitance of the tuned resonator **706** may also include capacitance between the charge terminal T_R and the lossy conducting medium **403**, where the total capacitance of the tuned resonator **706** may be calculated from both the self-capacitance C_R and any bound capacitance as can be appreciated. According to one embodiment, the charge terminal T_R may be raised to a height so as to substantially reduce or eliminate any bound capacitance. The existence of a bound capacitance may be determined from capacitance measurements between the charge terminal T_R and the lossy conducting medium **403**.

The inductive reactance presented by a discrete-element coil L_R may be calculated as $j\omega L$, where L is the lumped-element inductance of the coil L_R . If the coil L_R is a distributed element, its equivalent terminal-point inductive reactance may be determined by conventional approaches. To tune the tuned resonator **706**, one would make adjustments so that the inductive reactance presented by the coil L_R equals the capacitive reactance presented by the tuned resonator **706** so that the resulting net reactance of the tuned resonator **706** is substantially zero at the frequency of operation. An impedance matching network **723** may be inserted between the probe terminals **721** and the electrical load **726** in order to effect a conjugate-match condition for maxim power transfer to the electrical load **726**.

When placed in the presence of a guided surface wave, generated at the frequency of the tuned resonator **706** and the conjugate matching network **723**, as described above, maximum power will be delivered from the surface guided wave to the electrical load **726**. That is, once conjugate impedance matching is established between the tuned resonator **706** and the electrical load **726**, power will be delivered from the structure to the electrical load **726**. To this end, an electrical load **726** may be coupled to the tuned resonator **706** by way of magnetic coupling, capacitive coupling, or conductive (direct tap) coupling. The elements of the coupling network may be lumped components or distributed elements as can be appreciated. In the embodiment shown in FIG. **19B**, magnetic coupling is employed where a coil L_S is positioned as a secondary relative to the coil L_R that acts as a transformer primary. The coil L_S may be link coupled to the coil L_R by geometrically winding it around the same core structure and adjusting the coupled magnetic flux as can be appreciated. In addition, while the tuned resonator **706** comprises a series-tuned resonator, a parallel-tuned resonator or even a distributed-element resonator may also be used.

Referring to FIG. **20**, the magnetic coil **709** comprises a receive circuit that is coupled through an impedance matching network **733** to an electrical load **736**. In order to facilitate reception and/or extraction of electrical power from a guided surface wave, the magnetic coil **709** may be positioned so that the magnetic flux of the guided surface wave, H_{gs} , passes through the magnetic coil **709**, thereby inducing a current in the magnetic coil **709** and producing a terminal point voltage at its output terminals **729**. The magnetic flux of the guided surface wave coupled to a single turn coil is expressed by

$$\Psi = \iint_{A_{CS}} \mu_r \mu_0 \vec{H} \cdot \hat{n} dA \quad (61)$$

where Ψ is the coupled magnetic flux, μ_r is the effective relative permeability of the core of the magnetic coil **709**, μ_0 is the permeability of free space, $\vec{H}$ is the incident magnetic field strength vector, $\hat{n}$ is a unit vector normal to the cross-sectional area of the turns, and A_{CS} is the area enclosed by each loop. For an N -turn magnetic coil **709** oriented for maximum coupling to an incident magnetic field that is uniform over the cross-sectional area of the magnetic coil **709**, the open-circuit induced voltage appearing at the output terminals **729** of the magnetic coil **709** is

$$V = -N \frac{d\Psi}{dt} \approx -j\omega \mu_r \mu_0 H A_{CS}, \quad (62)$$

where the variables are defined above. The magnetic coil **709** may be tuned to the guided surface wave frequency either as a distributed resonator or with an external capacitor

across its output terminals **729**, as the case may be, and then impedance-matched to an external electrical load **736** through a conjugate impedance matching network **733**.

Assuming that the resulting circuit presented by the magnetic coil **709** and the electrical load **736** are properly adjusted and conjugate impedance matched, via impedance matching network **733**, then the current induced in the magnetic coil **709** may be employed to optimally power the electrical load **736**. The receive circuit presented by the magnetic coil **709** provides an advantage in that it does not have to be physically connected to the ground.

With reference to FIGS. **19A**, **19B**, and **20**, the receive circuits presented by the linear probe **703**, the tuned resonator **706**, and the magnetic coil **709** each facilitate receiving electrical power transmitted from any one of the embodiments of guided surface waveguide probes **400** described above. To this end, the energy received may be used to supply power to an electrical load **716/726/736** via a conjugate matching network as can be appreciated. This contrasts with the signals that may be received in a receiver that were transmitted in the form of a radiated electromagnetic field. Such signals have very low available power and receivers of such signals do not load the transmitters.

It is also characteristic of the present guided surface waves generated using the guided surface waveguide probes **400** described above that the receive circuits presented by the linear probe **703**, the tuned resonator **706**, and the magnetic coil **709** will load the excitation source **413** (FIG. **4**) that is applied to the guided surface waveguide probe **400**, thereby generating the guided surface wave to which such receive circuits are subjected. This reflects the fact that the guided surface wave generated by a given guided surface waveguide probe **400** described above comprises a transmission line mode. By way of contrast, a power source that drives a radiating antenna that generates a radiated electromagnetic wave is not loaded by the receivers, regardless of the number of receivers employed.

Thus, together one or more guided surface waveguide probes **400** and one or more receive circuits in the form of the linear probe **703**, the tuned resonator **706**, and/or the magnetic coil **709** can together make up a wireless distribution system. Given that the distance of transmission of a guided surface wave using a guided surface waveguide probe **400** as set forth above depends upon the frequency, it is possible that wireless power distribution can be achieved across wide areas and even globally.

The conventional wireless-power transmission/distribution systems extensively investigated today include "energy harvesting" from radiation fields and also sensor coupling to inductive or reactive near-fields. In contrast, the present wireless-power system does not waste power in the form of radiation which, if not intercepted, is lost forever. Nor is the presently disclosed wireless-power system limited to extremely short ranges as with conventional mutual-reactance coupled near-field systems. The wireless-power system disclosed herein probe-couples to the novel surface-guided transmission line mode, which is equivalent to delivering power to a load by a wave-guide or a load directly wired to the distant power generator. Not counting the power required to maintain transmission field strength plus that dissipated in the surface waveguide, which at extremely low frequencies is insignificant relative to the transmission losses in conventional high-tension power lines at 60 Hz, all the generator power goes only to the desired electrical load. When the electrical load demand is terminated, the source power generation is relatively idle.

Referring next to FIG. 21A shown is a schematic that represents the linear probe 703 and the tuned resonator 706. FIG. 21B shows a schematic that represents the magnetic coil 709. The linear probe 703 and the tuned resonator 706 may each be considered a Thevenin equivalent represented by an open-circuit terminal voltage source V_s and a dead network terminal point impedance Z_s . The magnetic coil 709 may be viewed as a Norton equivalent represented by a short-circuit terminal current source I_s and a dead network terminal point impedance Z_s . Each electrical load 716/726/736 (FIGS. 19A, 19B and 20) may be represented by a load impedance Z_L . The source impedance Z_s comprises both real and imaginary components and takes the form $Z_s = R_s + jX_s$.

According to one embodiment, the electrical load 716/726/736 is impedance matched to each receive circuit, respectively. Specifically, each electrical load 716/726/736 presents through a respective impedance matching network 719/723/733 a load on the probe network specified as Z_L' expressed as $Z_L' = R_L' + jX_L'$, which will be equal to $Z_L' = Z_s^* = R_s - jX_s$, where the presented load impedance Z_L' is the complex conjugate of the actual source impedance Z_s . The conjugate match theorem, which states that if, in a cascaded network, a conjugate match occurs at any terminal pair then it will occur at all terminal pairs, then asserts that the actual electrical load 716/726/736 will also see a conjugate match to its impedance, Z_L' . See Everitt, W. L. and G. E. Anner, *Communication Engineering*, McGraw-Hill, 3rd edition, 1956, p. 407. This ensures that the respective electrical load 716/726/736 is impedance matched to the respective receive circuit and that maximum power transfer is established to the respective electrical load 716/726/736.

Operation of a guided surface waveguide probe 400 may be controlled to adjust for variations in operational conditions associated with the guided surface waveguide probe 400. For example, a probe control system 418 (FIG. 4) can be used to control the coupling circuit 409 and/or positioning of the charge terminal T_1 and/or compensation terminal T_2 to control the operation of the guided surface waveguide probe 400. Operational conditions can include, but are not limited to, variations in the characteristics of the lossy conducting medium 403 (e.g., conductivity σ and relative permittivity ϵ_r), variations in field strength and/or variations in loading of the guided surface waveguide probe 400. As can be seen from Equations (52)-(55), the index of refraction (n), the complex Brewster angle ($\theta_{i,B}$ and $\psi_{i,B}$), the wave tilt ($|W|e^{j\psi}$) and the complex effective height ($h_{eff} = h_p e^{j\Phi}$) can be affected by changes in soil conductivity and permittivity resulting from, e.g., weather conditions.

Equipment such as, e.g., conductivity measurement probes, permittivity sensors, ground parameter meters, field meters, current monitors and/or load receivers can be used to monitor for changes in the operational conditions and provide information about current operational conditions to the probe control system 418. The probe control system 418 can then make one or more adjustments to the guided surface waveguide probe 400 to maintain specified operational conditions for the guided surface waveguide probe 400. For instance, as the moisture and temperature vary, the conductivity of the soil will also vary. Conductivity measurement probes and/or permittivity sensors may be located at multiple locations around the guided surface waveguide probe 400. Generally, it would be desirable to monitor the conductivity and/or permittivity at or about the Hankel crossover distance R_h for the operational frequency. Conductivity measurement probes and/or permittivity sensors may be located at multiple locations (e.g., in each quadrant) around the guided surface waveguide probe 400.

FIG. 22A shows an example of a conductivity measurement probe that can be installed for monitoring changes in soil conductivity. As shown in FIG. 22A, a series of measurement probes are inserted along a straight line in the soil. For example, the probes may be 9/16-inch diameter rods with a penetration depth of 12 inches or more, and spaced apart by $d=18$ inches. DS1 is a 100 Watt light bulb and R1 is a 5 Watt, 14.6 Ohm resistance. By applying an AC voltage to the circuit and measuring V1 across the resistance and V2 across the center probes, the conductivity can be determined by the weighted ratio of $\sigma=21(V1/V2)$. The measurements can be filtered to obtain measurements related only to the AC voltage supply frequency. Different configurations using other voltages, frequencies, probe sizes, depths and/or spacing may also be utilized.

Open wire line probes can also be used to measure conductivity and permittivity of the soil. As illustrated in FIG. 22B, impedance is measured between the tops of two rods inserted into the soil (lossy medium) using, e.g., an impedance analyzer. If an impedance analyzer is utilized, measurements ($R+jX$) can be made over a range of frequencies and the conductivity and permittivity determined from the frequency dependent measurements using

$$\sigma = \frac{8.84}{C_0} \left[\frac{R}{R^2 + X^2} \right] \text{ and } \epsilon_r = \frac{10^6}{2\pi f C_0} \left[\frac{R}{R^2 + X^2} \right], \quad (63)$$

where C_0 is the capacitance in pF of the probe in air.

The conductivity measurement probes and/or permittivity sensors can be configured to evaluate the conductivity and/or permittivity on a periodic basis and communicate the information to the probe control system 418 (FIG. 4). The information may be communicated to the probe control system 418 through a network such as, but not limited to, a LAN, WLAN, cellular network, or other appropriate wired or wireless communication network. Based upon the monitored conductivity and/or permittivity, the probe control system 418 may evaluate the variation in the index of refraction (n), the complex Brewster angle ($\theta_{i,B}$ and $\psi_{i,B}$), the wave tilt ($|W|e^{j\psi}$) and/or the complex effective height ($h_{eff} = h_p e^{j\Phi}$) and adjust the guided surface waveguide probe 400 to maintain the wave tilt at the Hankel crossover distance so that the illumination remains at the complex Brewster angle. This can be accomplished by adjusting, e.g., h_p , Φ_L , Φ_C and/or h_d . For instance, the probe control system 418 can adjust the height (h_d) of the compensation terminal T_2 or the phase delay (Φ_C , Φ_L) applied to the charge terminal T_1 and/or compensation terminal T_2 , respectively, to maintain the electrical launching efficiency of the guided surface wave at or near its maximum. The phase applied to the charge terminal T_1 and/or compensation terminal T_2 can be adjusted by varying the tap position on the coil 909, and/or by including a plurality of predefined taps along the coil 909 and switching between the different predefined tap locations to maximize the launching efficiency.

Field or field strength (FS) meters (e.g., a FIM-41 FS meter, Potomac Instruments, Inc., Silver Spring, Md.) may also be distributed about the guided surface waveguide probe 400 to measure field strength of fields associated with the guided surface wave. The field or FS meters can be configured to detect the field strength and/or changes in the field strength (e.g., electric field strength) and communicate that information to the probe control system 418. The information may be communicated to the probe control system 418 through a network such as, but not limited to, a

LAN, WLAN, cellular network, or other appropriate communication network. As the load and/or environmental conditions change or vary during operation, the guided surface waveguide probe 400 may be adjusted to maintain specified field strength(s) at the FS meter locations to ensure appropriate power transmission to the receivers and the loads they supply.

For example, the phase delay (Φ_L , Φ_C) applied to the charge terminal T_1 and/or compensation terminal T_2 , respectively, can be adjusted to improve and/or maximize the electrical launching efficiency of the guided surface waveguide probe 400. By adjusting one or both phase delays, the guided surface waveguide probe 400 can be adjusted to ensure the wave tilt at the Hankel crossover distance remains at the complex Brewster angle. This can be accomplished by adjusting a tap position on the coil 909 to change the phase delay supplied to the charge terminal T_1 and/or compensation terminal T_2 . The voltage level supplied to the charge terminal T_1 can also be increased or decreased to adjust the electric field strength. This may be accomplished by adjusting the output voltage of the excitation source 412 (FIG. 4) or by adjusting or reconfiguring the coupling circuit 409 (FIG. 4). For instance, the position of the tap 924 (FIG. 4) for the AC source 912 (FIG. 4) can be adjusted to increase the voltage seen by the charge terminal T_1 . Maintaining field strength levels within predefined ranges can improve coupling by the receivers, reduce ground current losses, and avoid interference with transmissions from other guided surface waveguide probes 400.

Referring to FIG. 23A, shown is an example of an adaptive control system 430 including the probe control system 418 of FIG. 4, which is configured to adjust the operation of a guided surface waveguide probe 400, based upon monitored conditions. The probe control system 418 can be implemented with hardware, firmware, software executed by hardware, or a combination thereof. For example, the probe control system 418 can include processing circuitry including a processor and a memory, both of which can be coupled to a local interface such as, for example, a data bus with an accompanying control/address bus as can be appreciated by those with ordinary skill in the art. A probe control application may be executed by the processor to adjust the operation of the guided surface waveguide probe 400 based upon monitored conditions. The probe control system 418 can also include one or more network interfaces for communicating with the various monitoring devices. Communications can be through a network such as, but not limited to, a LAN, WLAN, cellular network, or other appropriate communication network. The probe control system 418 may comprise, for example, a computer system such as a server, desktop computer, laptop, or other system with like capability.

The adaptive control system 430 can include one or more ground parameter meter(s) 433 such as, but not limited to, a conductivity measurement probe of FIG. 22A and/or an open wire probe of FIG. 22B. The ground parameter meter(s) 433 can be distributed about the guided surface waveguide probe 400 at about the Hankel crossover distance (R_c) associated with the probe operating frequency. For example, an open wire probe of FIG. 22B may be located in each quadrant around the guided surface waveguide probe 400 to monitor the conductivity and permittivity of the lossy conducting medium as previously described. The ground parameter meter(s) 433 can be configured to determine the conductivity and permittivity of the lossy conducting medium on a periodic basis and communicate the information to the probe control system 418 for potential adjustment

of the guided surface waveguide probe 400. In some cases, the ground parameter meter(s) 433 may communicate the information to the probe control system 418 only when a change in the monitored conditions is detected.

The adaptive control system 430 can also include one or more field meter(s) 436 such as, but not limited to, an electric field strength (FS) meter. The field meter(s) 436 can be distributed about the guided surface waveguide probe 400 beyond the Hankel crossover distance (R_c) where the guided field strength curve 103 (FIG. 1) dominates the radiated field strength curve 106 (FIG. 1). For example, a plurality of field meters 436 may be located along one or more radials extending outward from the guided surface waveguide probe 400 to monitor the electric field strength as previously described. The field meter(s) 436 can be configured to determine the field strength on a periodic basis and communicate the information to the probe control system 418 for potential adjustment of the guided surface waveguide probe 400. In some cases, the field meter(s) 436 may communicate the information to the probe control system 418 only when a change in the monitored conditions is detected.

Other variables can also be monitored and used to adjust the operation of the guided surface waveguide probe 400. For instance, the ground current flowing through the ground stake 915 (FIGS. 9A-9B, 17 and 18) can be used to monitor the operation of the guided surface waveguide probe 400. For example, the ground current can provide an indication of changes in the loading of the guided surface waveguide probe 400 and/or the coupling of the electric field into the guided surface wave mode on the surface of the lossy conducting medium 403. Real power delivery may be determined by monitoring of the AC source 912 (or excitation source 412 of FIG. 4). In some implementations, the guided surface waveguide probe 400 may be adjusted to maximize coupling into the guided surface waveguide mode based at least in part upon the current indication. By adjusting the phase delay supplied to the charge terminal T_1 and/or compensation terminal T_2 , the wave tilt at the Hankel crossover distance can be maintained for illumination at the complex Brewster angle for guided surface wave transmissions in the lossy conducting medium 403 (e.g., the earth). This can be accomplished by adjusting the tap position on the coil 909. However, the ground current can also be affected by receiver loading. If the ground current is above the expected current level, then this may indicate that unaccounted for loading of the guided surface waveguide probe 400 is taking place.

The excitation source 412 (or AC source 912) can also be monitored to ensure that overloading does not occur. As real load on the guided surface waveguide probe 400 increases, the output voltage of the excitation source 412, or the voltage supplied to the charge terminal T_1 from the coil, can be increased to increase field strength levels, thereby avoiding additional load currents. In some cases, the receivers themselves can be used as sensors monitoring the condition of the guided surface waveguide mode. For example, the receivers can monitor field strength and/or load demand at the receiver. The receivers can be configured to communicate information about current operational conditions to the probe control system 418. The information may be communicated to the probe control system 418 through a network such as, but not limited to, a LAN, WLAN, cellular network, or other appropriate communication network. Based upon the information, the probe control system 418 can then adjust the guided surface waveguide probe 400 for continued operation. For example, the phase delay (Φ_L , Φ_C) applied to the charge terminal T_1 and/or compensation terminal T_2 , respectively, can be adjusted to improve and/or

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maximize the electrical launching efficiency of the guided surface waveguide probe 400, to supply the load demands of the receivers. In some cases, the probe control system 418 may adjust the guided surface waveguide probe 400 to reduce loading on the excitation source 412 and/or guided surface waveguide probe 400. For example, the voltage supplied to the charge terminal T_1 may be reduced to lower field strength and prevent coupling to a portion of the most distant load devices.

The guided surface waveguide probe 400 can be adjusted by the probe control system 418 using, e.g., one or more tap controllers 439. In FIG. 23A, the connection from the coil 909 to the upper charge terminal T_1 is controlled by a tap controller 439. In response to a change in the monitored conditions (e.g., a change in conductivity, permittivity, and/or electric field strength), the probe control system can communicate a control signal to the tap controller 439 to initiate a change in the tap position. The tap controller 439 can be configured to vary the tap position continuously along the coil 909 or incrementally based upon predefined tap connections. The control signal can include a specified tap position or indicate a change by a defined number of tap connections. By adjusting the tap position, the phase delay of the charge terminal T_1 can be adjusted to improve the launching efficiency of the guided surface waveguide mode.

While FIG. 23A illustrates a tap controller 439 coupled between the coil 909 and the charge terminal T_1 , in other embodiments the connection 442 from the coil 909 to the lower compensation terminal T_2 can also include a tap controller 439. FIG. 23B shows another embodiment of the guided surface waveguide probe 400 with a tap controller 439 for adjusting the phase delay of the compensation terminal T_2 . FIG. 23C shows an embodiment of the guided surface waveguide probe 400 where the phase delay of both terminal T_1 and T_2 can be controlled using tap controllers 439. The tap controllers 439 may be controlled independently or concurrently by the probe control system 418. In both embodiments, an impedance matching network 445 is included for coupling the AC source 912 to the coil 909. In some implementations, the AC source 912 may be coupled to the coil 909 through a tap controller 439, which may be controlled by the probe control system 418 to maintain a matched condition for maximum power transfer from the AC source.

Referring back to FIG. 23A, the guided surface waveguide probe 400 can also be adjusted by the probe control system 418 using, e.g., a charge terminal positioning system 448 and/or a compensation terminal positioning system 451. By adjusting the height of the charge terminal T_1 and/or the compensation terminal T_2 , and thus the distance between the two, it is possible to adjust the coupling into the guided surface waveguide mode. The terminal positioning systems 448 and 451 can be configured to change the height of the terminals T_1 and T_2 by linearly raising or lowering the terminal along the z-axis normal to the lossy conducting medium 403. For example, linear motors may be used to translate the charge and compensation terminals T_1 and T_2 upward or downward using insulated shafts coupled to the terminals. Other embodiments can include insulated gearing and/or guy wires and pulleys, screw gears, or other appropriate mechanism that can control the positioning of the charge and compensation terminals T_1 and T_2 . Insulation of the terminal positioning systems 448 and 451 prevents discharge of the charge that is present on the charge and compensation terminals T_1 and T_2 . For instance, an insulating structure can support the charge terminal T_1 above the compensation terminal T_2 . For example, an RF insulating

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fiberglass mast can be used to support the charge and compensation terminals T_1 and T_2 . The charge and compensation terminals T_1 and T_2 can be individually positioned using the charge terminal positioning system 448 and/or compensation terminal positioning system 451 to improve and/or maximize the electrical launching efficiency of the guided surface waveguide probe 400.

As has been discussed, the probe control system 418 of the adaptive control system 430 can monitor the operating conditions of the guided surface waveguide probe 400 by communicating with one or more remotely located monitoring devices such as, but not limited to, a ground parameter meter 433 and/or a field meter 436. The probe control system 418 can also monitor other conditions by accessing information from, e.g., the ground current ammeter 927 (FIGS. 23B and 23C) and/or the AC source 912 (or excitation source 412). Based upon the monitored information, the probe control system 418 can determine if adjustment of the guided surface waveguide probe 400 is needed to improve and/or maximize the launching efficiency. In response to a change in one or more of the monitored conditions, the probe control system 418 can initiate an adjustment of one or more of the phase delay (Φ_c , Φ_L) applied to the charge terminal T_1 and/or compensation terminal T_2 , respectively, and/or the physical height (h_p , h_d) of the charge terminal T_1 and/or compensation terminal T_2 , respectively. In some implementations, the probe control system 418 can evaluate the monitored conditions to identify the source of the change. If the monitored condition(s) was caused by a change in receiver load, then adjustment of the guided surface waveguide probe 400 may be avoided. If the monitored condition(s) affect the launching efficiency of the guided surface waveguide probe 400, then the probe control system 418 can initiate adjustments of the guided surface waveguide probe 400 to improve and/or maximize the launching efficiency.

In some embodiments, the size of the charge terminal T_1 may also be adjusted to control the coupling into the guided surface waveguide mode. For example, the self-capacitance of the charge terminal T_1 can be varied by changing the size of the terminal. The charge distribution can also be improved by increasing the size of the charge terminal T_1 , which can reduce the chance of an electrical discharge from the charge terminal T_1 . Control of the charge terminal T_1 size can be provided by the probe control system 418 through the charge terminal positioning system 448 or through a separate control system.

FIGS. 24A and 24B illustrate an example of a variable terminal 203 that can be used as a charge terminal T_1 of the guided surface waveguide probe 400. For example, the variable terminal 203 can include an inner cylindrical section 206 nested inside of an outer cylindrical section 209. The inner and outer cylindrical sections 206 and 209 can include plates across the bottom and top, respectively. In FIG. 24A, the cylindrically shaped variable terminal 203 is shown in a contracted condition having a first size, which can be associated with a first effective spherical diameter. To change the size of the terminal, and thus the effective spherical diameter, one or both sections of the variable terminal 203 can be extended to increase the surface area as shown in FIG. 24B. This may be accomplished using a driving mechanism such as an electric motor or hydraulic cylinder that is electrically isolated to prevent discharge of the charge on the terminal.

It should be emphasized that the above-described embodiments of the present disclosure are merely possible examples of implementations set forth for a clear understanding of the principles of the disclosure. Many variations

and modifications may be made to the above-described embodiment(s) without departing substantially from the spirit and principles of the disclosure. All such modifications and variations are intended to be included herein within the scope of this disclosure and protected by the following claims. In addition, all optional and preferred features and modifications of the described embodiments and dependent claims are usable in all aspects of the disclosure taught herein. Furthermore, the individual features of the dependent claims, as well as all optional and preferred features and modifications of the described embodiments are combinable and interchangeable with one another.

Therefore, the following is claimed:

1. A guided surface waveguide probe, comprising:
 - a charge terminal elevated over a lossy conducting medium; and
 - a coupling circuit configured to couple an excitation source to the charge terminal, the coupling circuit configured to provide a voltage to the charge terminal that establishes an electric field having a wave tilt (W) that intersects the lossy conducting medium at a tangent of a complex Brewster angle ($\psi_{i,B}$) at a Hankel crossover distance (R_x) from the guided surface waveguide probe.
2. The guided surface waveguide probe of claim 1, wherein the coupling circuit comprises a coil coupled between the excitation source and the charge terminal.
3. The guided surface waveguide probe of claim 2, wherein the coil is a helical coil.
4. The guided surface waveguide probe of claim 2, wherein the excitation source is coupled to the coil via a tap connection.
5. The guided surface waveguide probe of claim 4, wherein the tap connection is at an impedance matching point on the coil.
6. The guided surface waveguide probe of claim 4, wherein an impedance matching network is coupled between the excitation source and the tap connection on the coil.
7. The guided surface waveguide probe of claim 2, wherein the excitation source is magnetically coupled to the coil.
8. The guided surface waveguide probe of claim 2, wherein the charge terminal is coupled to the coil via a tap connection.
9. The guided surface waveguide probe of claim 1, wherein the charge terminal is positioned at a physical height (h_p) corresponding to a magnitude of an effective height of the guided surface waveguide probe, where the effective height is given by $h_{eff}=R_x \tan \psi_{i,B}=h_p e^{j\Phi}$, with $\psi_{i,B}=(\pi/2)-\theta_{i,B}$ and Φ is a phase of the effective height.
10. The guided surface waveguide probe of claim 9, wherein the phase Φ is approximately equal to an angle W of the wave tilt of illumination that corresponds to the complex Brewster angle.
11. The guided surface waveguide probe of claim 1, wherein the charge terminal has an effective spherical diameter, and the charge terminal is positioned at a height that is at least four times the effective spherical diameter.
12. The guided surface waveguide probe of claim 11, wherein the charge terminal is a spherical terminal with the effective spherical diameter equal to a diameter of the spherical terminal.
13. The guided surface waveguide probe of claim 11, wherein the height of the charge terminal is greater than a physical height (h_p) corresponding to a magnitude of an effective height of the guided surface waveguide probe,

where the effective height is given by $h_{eff}=R_x \tan \psi_{i,B}=h_p e^{j\Phi}$, with $\psi_{i,B}=(\pi/2)-\theta_{i,B}$ and Φ is a phase of the effective height.

14. The guided surface waveguide probe of claim 13, further comprising a compensation terminal positioned below the charge terminal, the compensation terminal coupled to the coupling circuit.

15. The guided surface waveguide probe of claim 14, wherein the compensation terminal is positioned below the charge terminal at a distance equal to the physical height (h_p).

16. The guided surface waveguide probe of claim 15, wherein Φ is a complex phase difference between the compensation terminal and the charge terminal.

17. The guided surface waveguide probe of claim 1, wherein the lossy conducting medium is a terrestrial medium.

18. A system, comprising:

a guided surface waveguide probe, including:

- a charge terminal elevated over a lossy conducting medium; and
- a coupling circuit configured to provide a voltage to the charge terminal that establishes an electric field having a wave tilt (W) that intersects the lossy conducting medium at a tangent of a complex Brewster angle ($\psi_{i,B}$) at a Hankel crossover distance (R_x) from the guided surface waveguide probe; and
- an excitation source coupled to the charge terminal via the coupling circuit.

19. The system of claim 18, further comprising a probe control system configured to adjust the guided surface waveguide probe based at least in part upon characteristics of the lossy conducting medium.

20. The system of claim 19, wherein the lossy conducting medium is a terrestrial medium.

21. The system of claim 19, wherein the coupling circuit comprises a coil coupled between the excitation source and the charge terminal, the charge terminal coupled to the coil via a variable tap.

22. The system of claim 21, wherein the coil is a helical coil.

23. The system of claim 21, wherein the probe control system adjusts a position of the variable tap in response to a change in the characteristics of the lossy conducting medium.

24. The system of claim 23, wherein the adjustment of the position of the variable tap adjusts the wave tilt of the electric field to correspond to a wave illumination that intersects the lossy conducting medium at the complex Brewster angle ($\psi_{i,B}$) at the Hankel crossover distance (R_x).

25. The system of claim 22, wherein the guided surface waveguide probe further comprises a compensation terminal positioned below the charge terminal, the compensation terminal coupled to the coupling circuit.

26. The system of claim 25, wherein the compensation terminal is positioned below the charge terminal at a distance equal to a physical height (h_p) corresponding to a magnitude of an effective height of the guided surface waveguide probe, where the effective height is given by $h_{eff}=R_x \tan \psi_{i,B}=h_p e^{j\Phi}$, with $\psi_{i,B}=(\pi/2)-\theta_{i,B}$ and wherein Φ is a complex phase difference between the compensation terminal and the charge terminal.

27. The system of claim 25, wherein the probe control system adjusts a position of the compensation terminal in response to a change in the characteristics of the lossy conducting medium.

28. A method, comprising:

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positioning a charge terminal at a defined height over a lossy conducting medium;
 positioning a compensation terminal below the charge terminal and over the lossy conducting medium, the compensation terminal separated from the charge terminal by a defined distance; and
 exciting the charge terminal and the compensation terminal with excitation voltages having a complex phase difference, where the excitation voltages establish an electric field having a wave tilt (W) that corresponds to a wave illuminating the lossy conducting medium at a complex Brewster angle ($\psi_{i,B}$) at a Hankel crossover distance (R_x) from the charge terminal and the compensation terminal.

29. The method of claim 28, wherein the charge terminal has an effective spherical diameter, and the charge terminal is positioned at the defined height is at least four times the effective spherical diameter.

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30. The method of claim 28, wherein the defined distance is equal to a physical height (h_p) corresponding to a magnitude of an effective height of the charge terminal, where the effective height is given by $h_{eff} = R_x \tan \psi_{i,B} = h_p e^{j\Phi}$, with $\psi = (\pi/2) - \theta_{i,B}$ and wherein Φ is the complex phase difference between the compensation terminal and the charge terminal.

31. The method of claim 28, wherein the charge terminal and the compensation terminal are coupled to an excitation source via a coil, the charge terminal coupled to the coil by a variable tap.

32. The method of claim 31, further comprising adjusting a position of the variable tap to establish the electric field with the wave tilt intersecting the lossy conducting medium at the complex Brewster angle ($\psi_{i,B}$) at the Hankel crossover distance (R_x).

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MÉTODOS, SISTEMAS Y SONDAS DE GUÍA DE ONDA SUPERFICIAL GUIADA PARA EXCITAR MODOS DE ONDA SUPERFICIAL GUIADOS EN MEDIOS CON PÉRDIDAS

Detalle del pago

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